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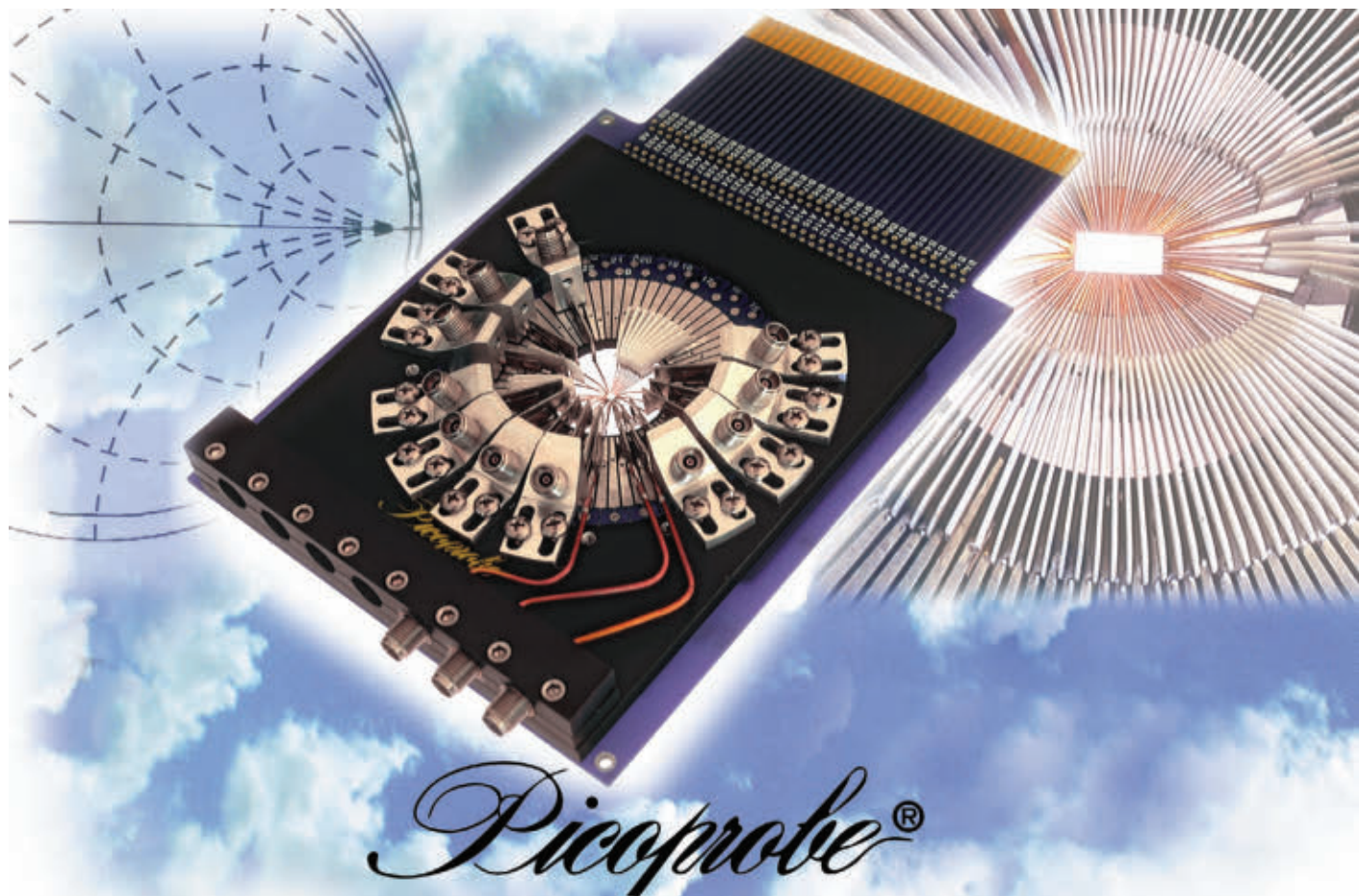
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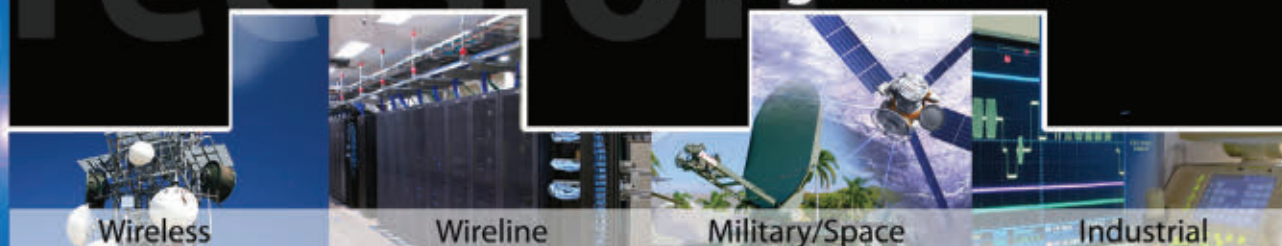
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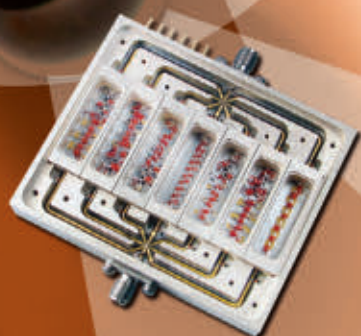
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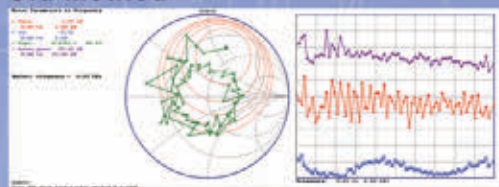
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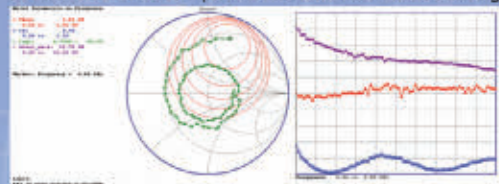
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Old Method

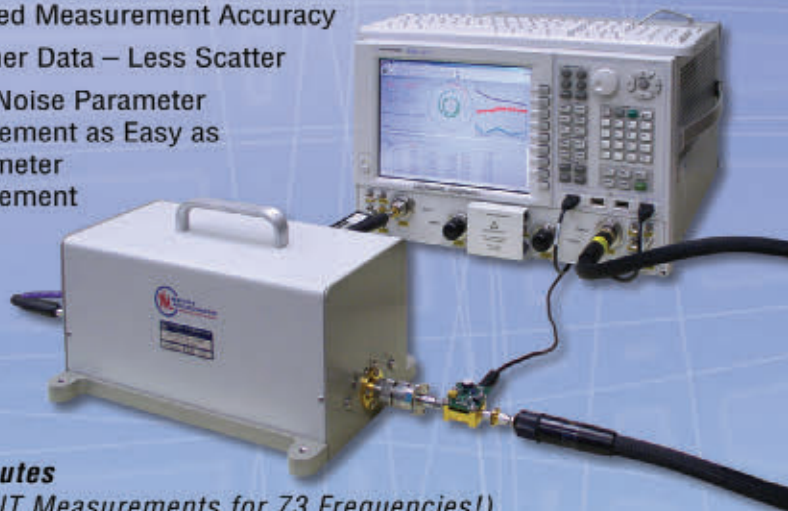


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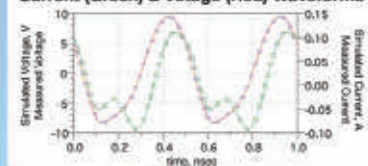
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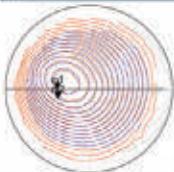
Excellent Agreement – Simulated vs Measured

Current (Green) & Voltage (Red) Waveforms



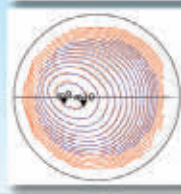
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— Simulated (Blue)
— Measured (Red)

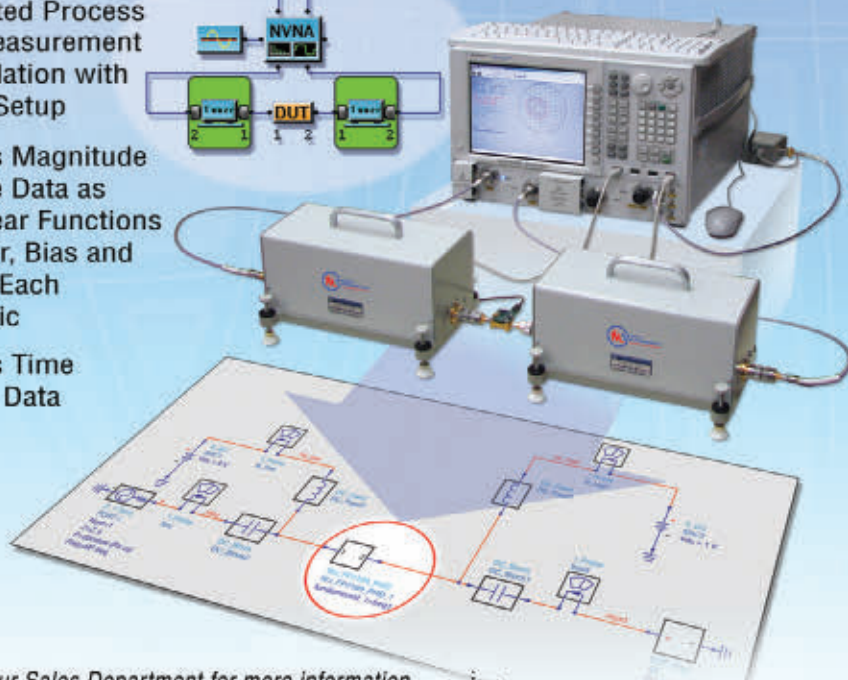
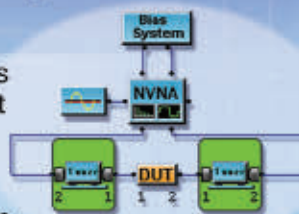


Pout Contours

— Simulated (Blue)
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Microwave Journal

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Microwave Journal (USPS 396-250) (ISSN 0192-6225) is published monthly by Horizon House Publications Inc., 685 Canton St., Norwood, MA 02062. Periodicals postage paid at Norwood, MA 02062 and additional mailing offices.

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112 Network Analysis Duo Offers Extended Features

Rohde & Schwarz

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HUBER+SUHNER AG

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I have just finished reading the RFID article on page 58 of the March issue. I would like to correct the author's description of the Cardullo/Parks device covered by US Patent # 3,713,148. I am the co-inventor and designer of the device and I am also a co-founder of the company that designed the device. The author states the device is a "passive" transponder. My understanding of passive devices is that they use "backscatter" as the retransmission technique. Our device had an RF transmitter stage. This was necessary as we needed much more range than is possible with passive backscatter devices. The device was also RF carrier powered and therefore needed no batteries. Finally, the device had a rewriteable memory. That was a lot of technology for 1970.

We thought we had a device that would revolutionize such chores as collecting tolls, keeping track of railroad cars, etc. Sadly, when we presented the device to the Port Authority of New York and New Jersey they turned us down. One of the reasons they gave was because it "violated driver's rights" to photograph them for failing to pay the toll and therefore they were not interested. The Southern Rail Road had a barcode scanner and they were not interested. San Francisco's BART also turned us down. And so it went. It's hell being first and a small business.

Yours,

William Parks

PS: I enjoyed the article.

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Expert Advice

Dr. Ali Muhammad Abuelma'atti, Device Modeling Engineer at **RFMD (UK)**, talks about the design and optimization of low power, low noise and power amplifiers.



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Thilo Bednorz, Product Management & Applications Engineering, Spectrum and Network Analysis, Rohde & Schwarz

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Dr. Mike Heimlich, AWR

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Correcting Imperfections in IQ Modulators Improves RF Signal Fidelity

Eamon Nash, Analog Devices

More on the New Power Brokers

Read the full responses to our questionnaire on the state of LDMOS, GaN, SiC and HV-FETs from contributors RFMD, Freescale, NXP, Cree, Nitronex and HVVi. Go to www.mwjjournal.com/powerbrokers.

Executive Interview

Dr. Bernd Niedermann, Head of Corporate Communications at **HUBER+SUHNER**, explains the company's evolution since its formation following the merger of two independent companies 40 years ago, its commitment to providing connectivity solutions and its strategies for developing new technologies.

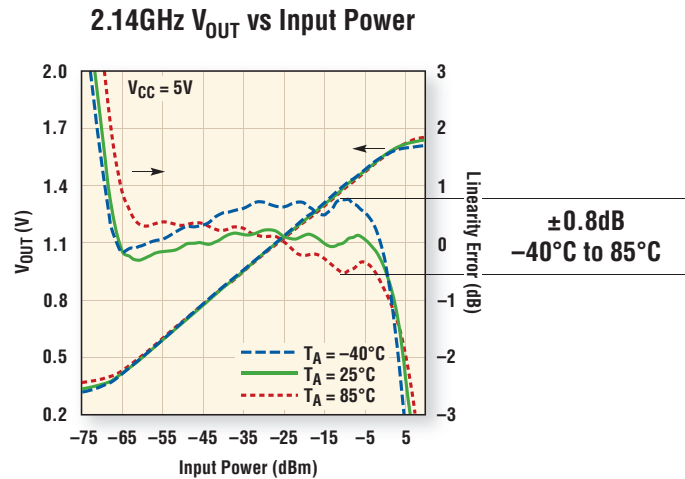


MWJ Blog

Our Blog section now includes guest bloggers from the industry, discussing the state of business and technology. Follow (RF) Leonard Pelletier of Freescale Semiconductor and Sherry Hess of AWR along with the various musings of *Microwave Journal* editors. Go to www.mwjjournal.com for details.

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	LT5538	75dB	40MHz to 3.8GHz	29mA @ 3V	3mm x 3mm DFN
RMS Detector	LT5570	60dB	40MHz to 2.7GHz	26.5mA @ 5V	3mm x 3mm DFN
	LT5581	40dB	10MHz to 6GHz	1.4mA @ 3.3V	3mm x 2mm DFN
Schottky Peak	LTC [®] 5505	34dB	0.3GHz to 3GHz	0.5mA @ 3.3V	SOT-23
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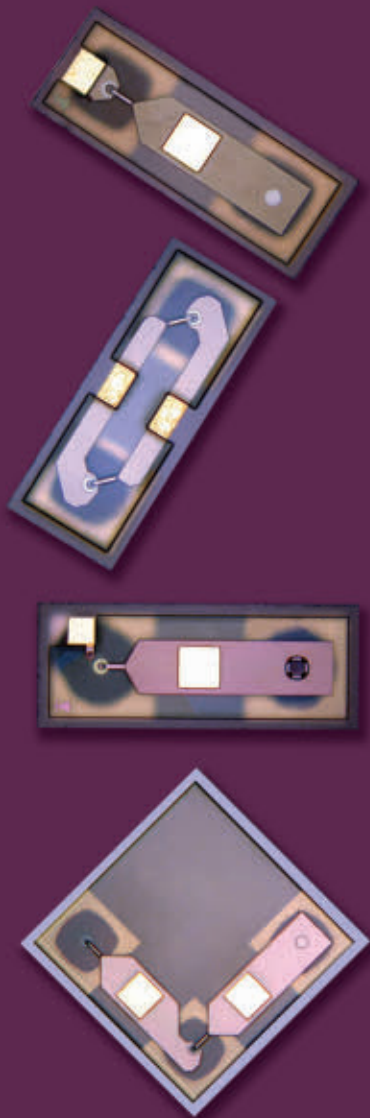
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SUNDAY	MONDAY	TUESDAY	WEDNESDAY	THURSDAY	FRIDAY	SATURDAY
28	29	30	1	2	3	4
5	6	7	8	9	10	11
			←..... 43 rd Annual Microwave Power Symposium Washington, DC			UK Microwave Group Yorkshire Roundtable, Finningley
12	13	14	15	16	17	18
UK Microwave Group Yorkshire Roundtable, Finningley		43 rd Annual Microwave Power Symposium	ASQED 2009 The 1 st Asia Symposium on Quality Electronic Design Kuala Lumpur, Malaysia	Ansoft Product Training San Jose, CA		
19	20	21	22	23	24	25
.....→		MWJ/Besser Webinar: OFDM and OFDMA Besser Associates AWR			←..... UK Microwave Group Amsat-UK Colloquium, Manchester University	
26	27	28	29	30	31	1
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THE NEW POWER BROKERS: HIGH VOLTAGE RF DEVICES

Ever since Bell Lab physicists Shockley, Bardeen and Brattain invented the transistor, this little solid state device has been constantly evolving; leveraging the advantages of different semiconductor and process technologies and addressing an increasing number of applications once reserved for tubes. Sixty-plus years later—driven by a number of promising commercial and defense-related markets—transistors (and MMICs) specifically targeting high power applications in the RF and microwave frequency range continue to be the focus of sizable research and development.

Among the changing landscape of RF/microwave semiconductor developments, devices with material properties that can sustain high electric breakdown are of particular interest. To understand the state of the high power transistor market, we spoke to a number of leading vendors. Our discussion was mostly concerned with devices that could produce in excess of 30 W at UHF/VHF frequencies and above (up to X-band). These are the high-power transistors required for avionics, radar, EW and wireless infrastructure applications. Although these devices are also found in medical equipment, those applications will not be part of our focus in this article. The following is a summary of our correspondence.

HIGH POWER TRANSISTOR TECHNOLOGIES AND APPLICATIONS

Within the last six months alone, the *Journal* has published over a dozen papers on Laterally Diffused MOS (LDMOS), Gallium Nitride (GaN), Silicon Carbide (SiC) and High-Voltage Vertical FETs (HVVFET). The principle market segments for high-power, high-frequency transistors are wireless infrastructure (3G, 3G+, WiMAX/LTE base stations and backhaul), defense and military applications (radar, jamming, counter-measures, guided weapons, etc.) and broadcast and communication satellites (SatCom). The factors that will decide whether a technology dominates a given application include performance (linearity, efficiency), reliability (ruggedness and thermal considerations), size, cost and legacy.

DAVID VYE *Microwave Journal*

LEONARD PELLETIER *Freescale Semiconductor*

STEVEN THEEUWEN *NXP Semiconductors*

DAVE AICHELE *RFMD*

RAY CRAMPTON *Nitronex*

RAY PENGELLY *Cree Inc.*

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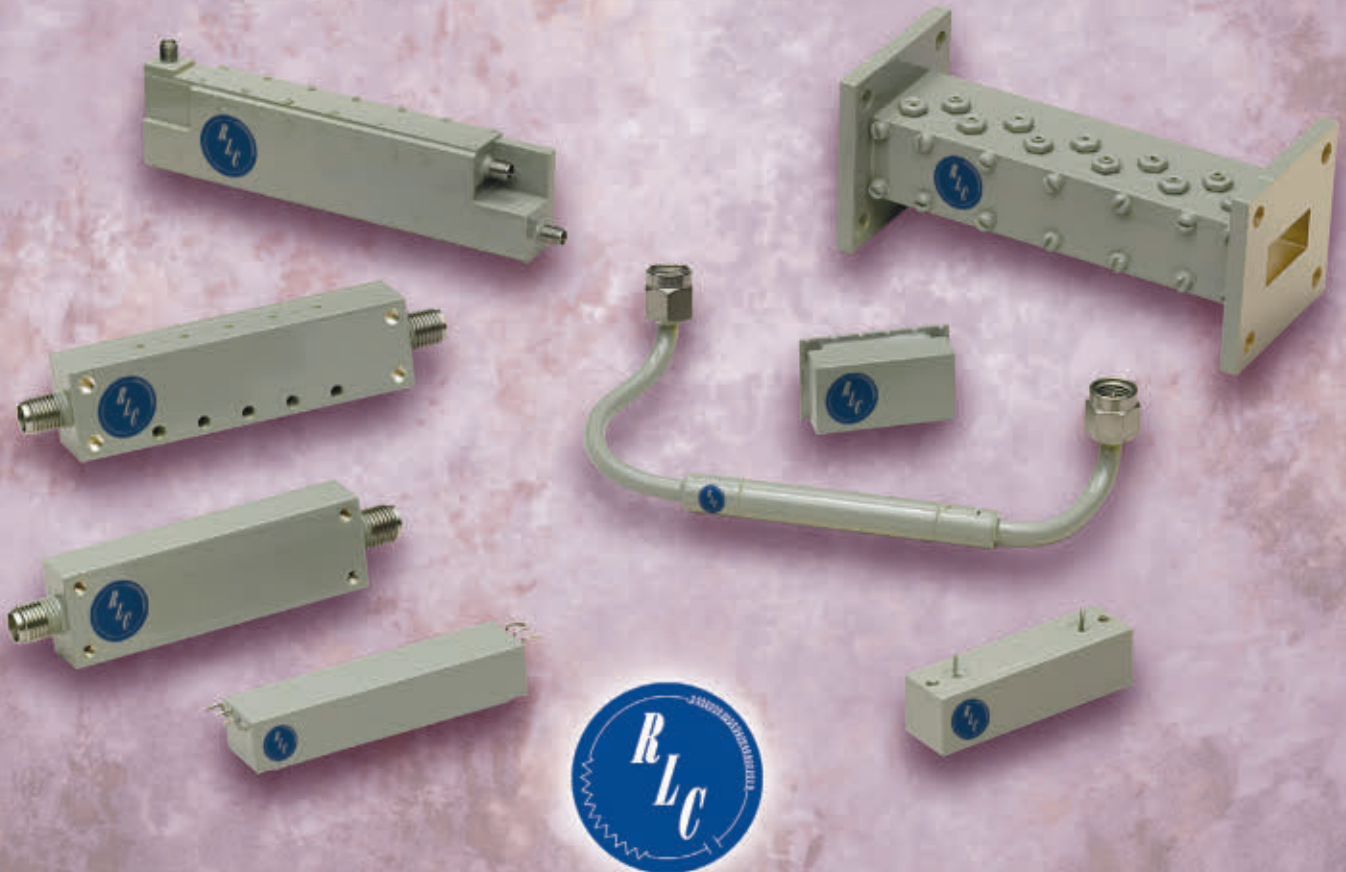
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Figure 1 maps the various high-power semiconductor technologies relative to their operating frequencies and available output power. With an understanding of the power and frequency requirements for a given application, this graph provides a rough guide to the leading technologies today. Implicit in this representation are regions where one technology overlaps another due to its cost advantage. This cost can be related to higher production costs (complexity, less mature processes or lower volume production all drive up costs) as well as replacement costs (a technology missed the critical time-to-market). As process technology advances and new standards (i.e. 4G) provide new opportunities to enter a market, technology dominance in any particular region is subject to change. These factors will be discussed later in this article.

RADAR AND AVIONICS

According to ABI Research, the demand for the pulsed RF power devices (greater than 5 W of peak output power and frequencies up to 3.8 GHz) is expected to show solid growth over the next five years, in part due to a worldwide upgrade of air traffic control systems including new avionics transponders and air navigation systems.¹ In response, many semiconductor manufacturers are attempting to enter the avionics, L-band, S-band and sub-1 GHz radar markets. Competitive technologies such as GaN and SiC devices will be vying for market share along with the more established silicon-based technologies. With the entry of many would-be players, competition will be fierce. Companies that have an established track record

working with government agencies and defense contractors will naturally have an advantage over new entrants.

Long-range radar systems operating from VHF thru S-band are demanding increased performance from the RF power amplifier in order to support the required improvements in system ranging and sensitivity. A key lesson learned from the crisis on 9/11 was the need to extend the pulse width to at least 300 μ s for long-range radar as well as the ability to increase the operating dynamic range of the power amplifier.²

UHF/VHF RADAR

Historically, silicon Class C amplifiers were limited by heat dissipation due to the potential for thermal runaway during long pulses ($> 300 \mu$ s) and high peak powers. Military applications were among the first to use wide band gap (WBG) devices, especially with the SiC MESFETs being developed through broadly financed DARPA and DoD programs in the US.³ Recently, Microsemi's Microwave RF Power Division developed its WBG SiC technology in support of the new longer pulse radar systems and avionics being developed from VHF thru S-band.

The state of material technology has progressed to the point where Microsemi can build high power devices with reasonable yields and consistent performance. In 2008, the company introduced its first two RF power transistors utilizing silicon carbide technology for high power VHF and UHF band pulsed radar applications. The two Common Gate N-Channel, Class AB, SiC Static Induction Transistors (SIT) are capable of providing 1000 W, pulsed (300 μ sec pulse width, 10 percent duty cycle) from 406 to 450 MHz and 1250 W pulsed at 150 to 160 MHz.

In January, the company made good on its promise to extend SiC technology to higher frequencies by introducing a new family of power transistors and modules designed for S-band (3.1 to 3.4

GHz) pulsed radar. The new products include a 65 and 100 W power transistor and two Power Solution Modules TM rated at 180 and 200 W (100 μ sec pulse width and 10 percent duty cycle). The modules demonstrate 40 percent collector efficiency and power flatness of less than 0.5 dB, utilizing the company's advanced chip design and processing enhancements for high power and high gain.

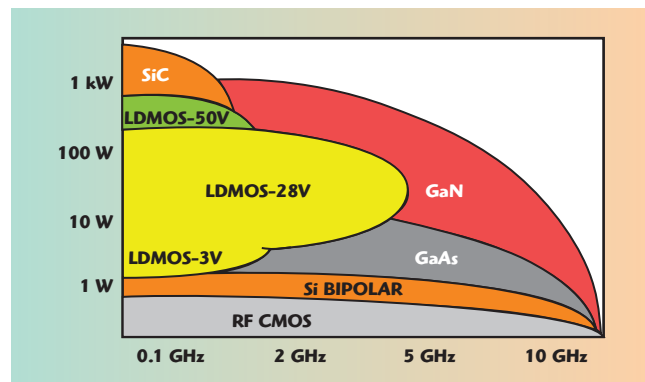
Around the same timeframe (December 2008), HVVi Semiconductors announced its first product to target the UHF-band weather and long-range radar markets using its High Voltage Vertical Field Effect Transistor (HVVFETTM) architecture. The company's 50 V device offered 175 W pulsed, 55 percent drain efficiency, 25 dB of gain for a pulse width of 300 μ sec and pulse duty cycle of 10 percent at VDD = 50 V and IDQ = 50 mA. The UHF part also provided a boost to system reliability by withstanding an output load mismatch corresponding to a 20:1 VSWR across all phase angles at rated output power and operating voltage across the entire frequency band.

L-BAND RADAR

This new device, based on the company's HVVFET, followed the earlier releases (October 2008 at European Microwave Week) of three devices with pulsed output powers of 60, 100 and 250 W operating in the 1025 to 1150 MHz frequency band. These devices targeted airborne Distance Measuring Equipment (DME) applications, a transponder-based radio navigation technology that measures distance by timing the propagation delay of radio signals. The company also targeted ground-based DME (960 to 1215 MHz) with a 50 V device that provides 150 W, 20 dB gain and 43 percent drain efficiency.

These products expanded the company's portfolio across three L-band, pulsed radar applications: 1025 to 1150 MHz, 1030 to 1090 MHz and 1.2 to 1.4 GHz. The 1030 to 1090 MHz frequency band is used for IFF, TCAS and mode-S applications. For this market, HVVi introduced a pulsed (50 μ s pulse width, 5 percent duty cycle) 35 W device (20 dB gain, 52 percent drain efficiency) and 300 W device (18 dB gain, 48 percent drain efficiency).

Meanwhile, Silicon Bipolar devices

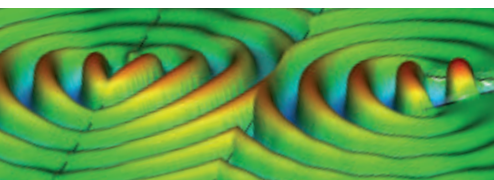


▲ Fig. 1 An overview of preferred transistor technologies for 2008 design-ins as a function of power and frequency (courtesy of NXP Semiconductors).



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RWP02080-10	35	80
RWP02160-10	35	160

20-1000MHz products

Part Number	Gain (dB)	Psat (W)
RWP05020-10	37	20
RWP05040-10	37	40
RWP05080-10	35	80
RWP05200-10	35	200

450-870MHz products

Part Number	Gain (dB)	Psat (W)
RWP06005-10	20	5
RWP06020-10	37	20
RWP06040-10	37	40
RWP06080-10	35	80
RWP06200-10	35	200

500-2500MHz products

Part Number	Gain (dB)	Psat (W)	Size (mm)
RUP15010-10	14	10	55x30
RUP15010-11	57	10	120x80
RUP15020-10	15	20	60.4x30.2
RUP15020-11	57	20	120x80
RUP15030-10	14	30	90x50
RUP15050-10	11	50	100x50
RUP15100-10	55	100	130x50

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continue to be introduced into the market. Companies such as ST Microelectronics, NEC, Motorola and NXP have large Si-BJT product portfolios (to name a few). Last summer, M/A-COM announced a line-up of new high-power bipolar transistors designed for pulsed avionics applications such as ATC, DME and IFF systems, ranging from 960 to 1215 MHz. The Class C, Si-BJT pulse power transistors provide peak powers of 50, 350 and 500 W with gains of approximately 9 dB and 40 to 45 percent collector efficiencies. Integra Technologies also has an extensive portfolio of Si-BJT high power transistors targeting VHF through S-band pulsed radar applications, but they are also offering LDMOS devices as this technology continues to challenge the supremacy of the Si-BJT in the avionics and radar markets.

At last year's IMS in Atlanta, Freescale Semiconductor introduced the world's first 50 V LDMOS device for L-band radar with a demonstration of a class AB, long-pulse (300 μ sec, 12 percent duty cycle) amplifier with peak power of 330 W, 17 dB gain and 60 percent drain efficiency operating between 1200 to 1400 MHz, a band used for ground-based, long-range surveillance radar applications. Freescale pointed to advantages, such as a standard voltage supply, low cooling costs and high reliability of pallet design and expected to demonstrate gain, efficiency and thermal resistance characteristics that would outperform other similar products in the market.

A year later at IMS in Boston, HVVi introduced its 500 W (19 dB gain, 50 percent drain efficiency) device operating with a 50 μ sec pulse width, and 5 percent duty cycle adding to its portfolio of products with pulsed output powers of 25, 75 and 120 W (200 μ sec pulse width, 10 percent duty cycle). The 500 W power level was also achieved by NXP Semiconductors this past November with an LDMOS device demonstrating greater than 50 percent drain efficiency and 17 dB of gain operating at 100 μ sec pulse width and a 25 percent duty cycle at 1.4 GHz.

Japanese manufacturer Eudyna hit the 500 W mark and then some with an AlGaIn/GaN HEMT 1.5 GHz power amplifier reported back in 2006 at the MTT-S IMS that year and an 800

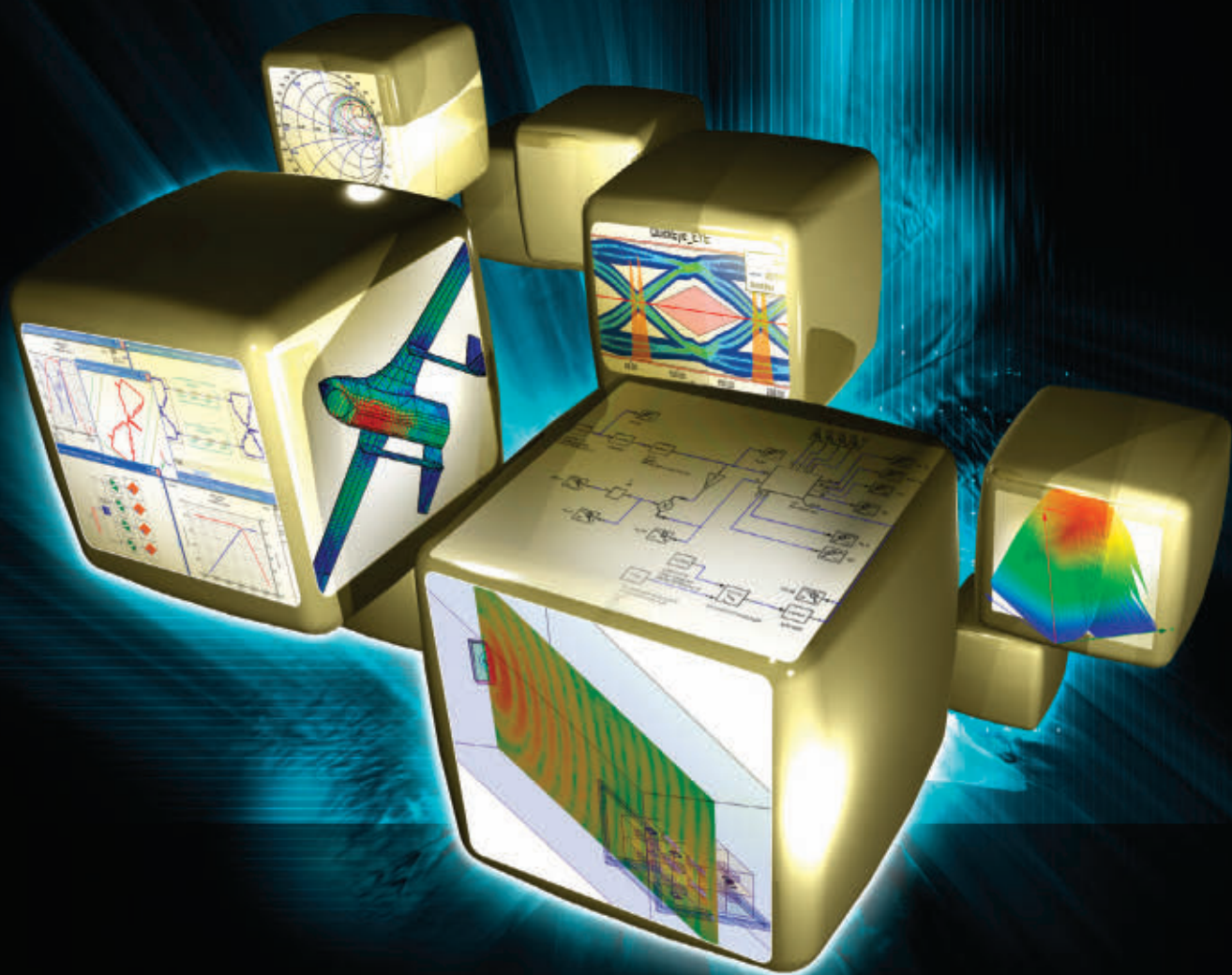
W S-band transistor with linear gain of 14.0 dB, 56.4 percent drain efficiency covering a wide frequency range of 2.9 to 3.3 GHz (operating at 65 V, pulse width of 200 μ sec and 10 percent duty cycle) reported just one year later at CS MANTECH. While Eudyna holds a strong position in the market, the company is at a disadvantage to domestic suppliers when it comes to US military opportunities due to (offshore) sourcing concerns. Not surprisingly, Eudyna markets its GaN HEMTs primarily to the WiMAX and LTE infrastructure markets where the majority of GaN manufacturers also have made considerable in-roads.

S-BAND RADAR

Integra Technologies addresses the S-band radar market with a comprehensive family of Si-bipolar devices (drivers, medium and high power amplifiers) operating from 2.2 up to 3.5 GHz (in bandwidths ranging from 200 to 400 MHz). The high power amplifiers have peak output powers up to 125 W (3.1 to 3.4 GHz) at 300 μ sec pulse width (PW), 10 percent DC and 140 W (3.1 to 3.5 GHz) at the shorter 100 μ sec PW, 10 percent duty cycle. The company offers a LDMOS device operating at the same frequency and pulse conditions, which yields an output power of 154 W (29 W more) and an extra dB of gain (10.4 dB) at a lower drain voltage (32 vs. 36 V). This improvement in performance underlines the competition between technologies, even within the same company.

One domestic manufacturer going after the S-band radar market with GaN technology is RFMD. At last year's MTT-S IMS in Atlanta, the company debuted a 400 W pulsed output power GaN HEMT amplifier operating over the 2.9 to 3.5 GHz band (17 percent bandwidth). Under pulsed RF drive, with 10 percent duty cycle and 100 μ sec pulse width, the amplifier delivers an output power in the range of 401 to 446 W over the band, with a drain efficiency of 48 to 55 percent when biased at a drain voltage of 65 V.

The wideband nature of GaN-based amplifiers, with the ability to easily cover 500 MHz to 3 GHz, make them well-suited for use in frequency agile pulsed applications such as military radar, air traffic control radar and communications jamming.



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In speaking with the *Journal*, RFMD remarked on GaN's higher efficiency for pulsed, CW saturated and linear applications, which improves thermal requirements and energy usage; showing 5 to 10 percent improvement over LDMOS and Si-Bipolar.

Ray Crampton of Nitronex further added that, "Radar applications require pulsed power in the hundreds of watts up to very high frequencies. This fits well because GaN devices offer improved robustness, higher efficiency, higher power density, higher gain and faster switching speed than competing technologies for today's broadband radar systems. GaN also offers the ability to replace TWTs with more reliable and robust devices." An example of Nitronex recent product offerings is the NPT1007, released last February. This is a 200 W device (based on two 100 W transistors) that targets military communication applications below 1.5 GHz and has notable "design-ins" in the 30 to 512 MHz band as well as bands up to 1 GHz, according to Crampton.

Meanwhile, TriQuint Semiconductor began investigating GaN technology back in 1999, and through subsequent years developed a baseline process that led to a DARPA contract focusing on technology maturity and wideband performance in 2005. This research and development effort resulted in a production-released 0.25 micron gate process supporting products from DC to 18 GHz and achieving power levels in excess of 100 W.

COMMERCIAL MARKETS – WIRELESS INFRASTRUCTURE

Until four years ago, LDMOS covered about 90 percent of the high power PA applications above 2 GHz; the remaining market share belonged mostly to GaAs PHEMT technology.

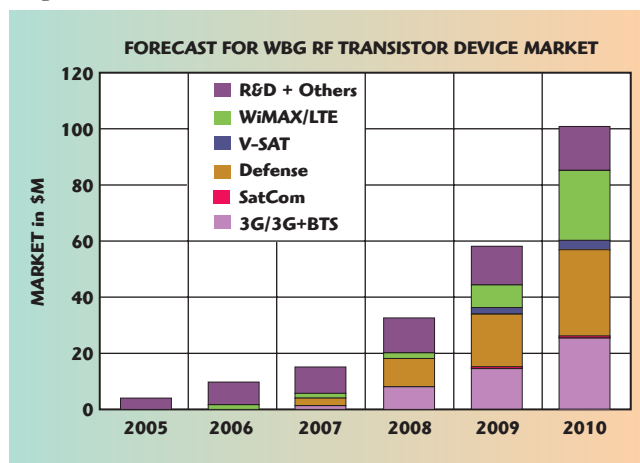
WBG devices made a significant commercial breakthrough in 2006 when Eudyna and NTT jointly announced the first 3G network "test" deployment using

GaN HEMT in Tokyo. New commercial offerings from Cree, RFMD and Nitronex soon followed, targeting both base station (3G, WiMAX) and general purpose applications. According to a 2008 GaN RF market report by Yole Développement, "GaN is currently positioned to challenge silicon dominance in the high power RF amplifier market estimated to be about \$900 M in 2008."³ ABI Research has the RF power market somewhat below this figure at a predicted \$800 M in 2011.¹ But this challenge is not across the board, as LDMOS maintains an upper hand with pricing and legacy in certain sectors.

In the power market below 4 GHz, RF LDMOS transistors captured almost 70 percent of the total market in 2006. However, that number is predicted to go to 50 percent share of the RF power market in 2011, the ABI report forecasts. GaN may dominate most of the high-power markets at frequencies above 4 GHz, beyond the performance range of Si LDMOS. Eudyna Devices and Toshiba have wisely targeted the microwave (> 4 GHz) markets for much of their participation with GaN.

4G OPPORTUNITIES

Market analysts point to product announcements by GaN manufacturers as indicators of their increased focus on WiMAX/LTE markets and a shift away from existing 3G/3G+ infrastructure, where LDMOS is the entrenched technology. Unfortunately, the WiMAX market in 2009 has been hit rather hard by the economic downturn. Building-out brand new networks from scratch, as is the



▲ Fig. 2 Projected RF markets for WBG transistors indicates most significant growth coming from 4G (courtesy of Yole Développement).



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case with WiMAX, requires hundreds of millions of dollars of capital. The current credit crunch along with a decrease in demand for broadband due to weakened consumer spending has led to many network build-outs being put on hold or delayed into next year.

Total sales of fixed and mobile WiMAX equipment fell 21 percent to US\$245 M in the third quarter of 2008, from the second quarter's figure, and are expected to slide further in 2009 (a report in early May 2009

shows component makers revenue down 20 to 30 percent versus the year-ago quarter). Prior to the current slowdown, the GaN RF Market 2008 from Yole Développement had forecasted that the market size for GaN RF transistors could reach a level of about \$100 M by 2010, largely due to strong penetration of WiMAX/LTE systems, as shown in **Figure 2**.

Still LTE rollouts are expected to be coming in the 2010 to 2011 timeframe and any WiMAX delays will

shorten its current time to market advantage over LTE. Therefore, WiMAX deployment cannot afford to be postponed for too long. According to ABI Research, the LTE standard is being driven by operators, which is the key differentiator between it and preceding wireless technologies. CDMA and Asian operators who are early adopters will be the first to launch LTE. Existing UMTS operators will probably delay launch to extend the life of their existing HSPA networks and simplify the upgrade to LTE by slowly evolving their current architectures.

When network operators introduced HSPA, packet data traffic quickly exceeded voice traffic. In some cases, a four fold increase in data traffic occurred in just three months. Future WiMAX and LTE build-outs will be needed in order to serve 1.8 billion broadband subscriptions by 2012, according to a five year projection made by Ericsson in 2007.⁴ To get there, high power transistors will need to deliver on performance, size, reliability and price.

TECHNOLOGY

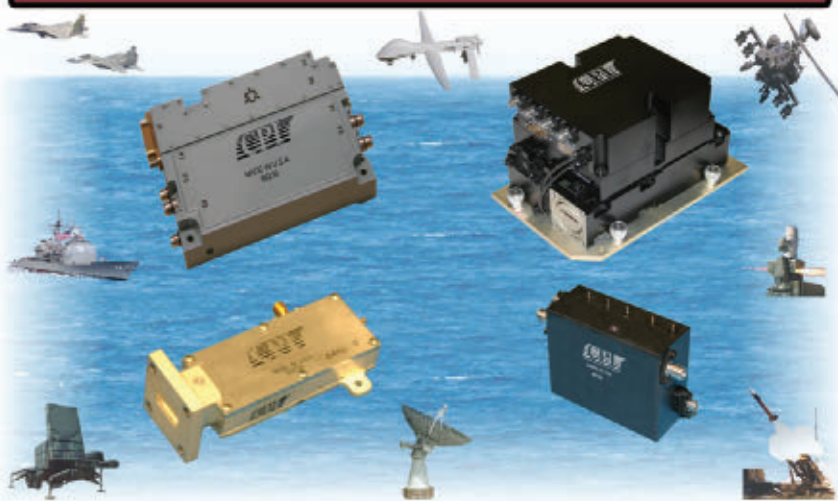
WiMAX faces strong competition from existing wireless services, making it essential that WiMAX infrastructure equipment be as cost-effective as possible. A rough rule of thumb is that for high volume cellular base station applications, LDMOS prices are on the order of \$0.30 per W, GaAs is about \$0.9/W and GaN is about \$1/W. Performance-wise, linearity and efficiency for both WiMAX and LTE are also critical.

THE IMPORTANCE OF LINEARITY AND EFFICIENCY

Both WiMAX and LTE use OFDM as the core modulation technology in the downlink direction and thus have roughly similar performance for any given RF bandwidth and set of conditions. However, the uplink modulation techniques are somewhat different. While WiMAX uses OFDMA for the uplink, LTE uses single carrier frequency division multiple access (SC-FDMA), which has a significantly reduced Peak to Average Power Ratio (PAPR). WiMAX's OFDMA has a peak-average ratio of about 10 dB, while LTE's SC-FDMA's peak-average ratio is about 5 dB.

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Model	Bands	Step Size	BW (GHz)	Typical Phase Noise						Output Frequency	Output Power (dBm, Min.)
				10	100	1K	10K	100K	1M		
BTE	L - Ku	1 kHz	2.2	-73	-80	-96	-96	-97	-123	12.72 GHz	13
MFS	L - K	1 kHz	2	-60	-75	-90	-95	-95	-120	5.3 GHz	13
CFS	L - K	1 Hz	2	-62	-75	-85	-89	-97	-110	14.84 GHz	13
Ku3LS	X - Ku	1 kHz	2.2	-62	-70	-75	-85	-97	-115	12.50 GHz	13
C3LS	C	1 kHz	1.1	-63	-88	-90	-100	-100	-115	5.50 GHz	13
UWB	S - K	1 kHz	Multi octave	-60	-71	-80	-90	-96	-105	12 GHz	13
MOS	VHF - K	1 kHz	Multi octave	-55	-65	-75	-85	-90	-100	20 GHz	13
SLS	L - Ku	125 kHz	1	-70	-80	-86	-88	-105	-115	3.3 GHz	13
SLFS	VHF - Ku	100 kHz	2	-70	-75	-80	-90	-115	-125	5 GHz	13
LFTS	VHF - Ku	100 Hz	1	-78	-88	-98	-98	-110	-130	350 MHz	13
VFS	L - Ku	>25 MHz	1.5	-60	-80	-110	-115	-115	-130	12.5 GHz	13

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WiMAX and OFDMA requires that the amplifier handle the occasional high power levels that can greatly exceed the average signal strength without introducing unacceptable levels of distortion. One way to do this is to use a larger transistor operating far below its compression point, otherwise known as backing-off the amplifier. Unfortunately, amplifier efficiency takes a hit when the device is backed-off. At 2 GHz, the latest LDMOS has

about 18 dB gain and is 65 percent efficient at the 1 dB compression point. At a 6 dB back off point, the devices are typically -45 dBc WCDMA ACPR and 30 percent efficient. GaN offers slightly higher efficiency at 6 dB OBO.

SAVING SOME GREEN

According to Steven Theeuwes of NXP Semiconductors, "All the developments particularly for base stations and broadcast applications

are driven by an ever increasing demand for higher efficiency, generally speaking. In turn this means less lost power, which means "greener" amplifiers. Higher efficiency does not only mean better use of RF power, but also reduces the energy necessary to remove the dissipated energy (cooling systems). Hence, improved efficiency helps twice, on amplifier and system level, to reduce overall power consumption. NXP claims leadership in delivering high efficient transistors and high efficiency concepts: developing the world's first fully integrated Doherty amplifier and the highest efficiency, discrete Doherty setup to date." (Ed. note: Based on LDMOS technology.)

At Mobile World Congress (Barcelona, Spain) in February, Freescale introduced its next generation (HV8) of LDMOS high power transistors, specifically targeting the stringent demands of high-data rates called for by WCDMA, WiMAX, LTE and Multicarrier GSM. The company claims that a primary benefit of the HV8 technology is the increase in operating efficiency, reducing the total power consumption of a base station system. This growing concern in "green" technology is driven by a global desire to cut energy costs and reduce the industry's carbon footprint along with the telecom provider's interest in lowering operating expenses.

The new devices introduced in February operate over the 860 to 960 MHz range, providing a power output range of 100 to 300 W and can be used in Class AB or C configurations. A symmetrical Doherty reference design using two transistors designed for multicarrier GSM applications was shown to deliver 58.0 dBm (630 W) peak power, 16.3 dB gain and a drain efficiency of 42.5 percent at an average output power level of 49.4 dBm (87 W) with good broadband linearity. Digital pre-distortion (DPD) evaluations showed the reference design to correct very well with six GSM carriers in signal bandwidths of up to 20 MHz.

According to Leonard Pelletier of Freescale, one of the most substantial system-related issues to consider when working with LDMOS is creating higher linearity through digital pre-distortion or feed forward error correction systems. With improve-



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ments in the correction capability of the architectures, the RF devices can be operated closer to their P1dB compression point, where the DC to RF conversion efficiencies are at their highest level. Improved linearity translates to improved efficiency and lower overall system costs.

Linearity and efficiency are also addressed with similar circuit architectures designed using GaN devices. According to Dave Aichele of RFMD, "The high terminal impedances of high

voltage GaN devices make the amplifiers suitable for higher bandwidth Class AB amplifiers as well as applications that attempt to improve efficiency such as Doherty, linearity such as push-pull, and extreme bandwidth such as distributed techniques. Thanks to the high impedances (and low parasitics) of GaN HEMTs, these higher bandwidth amplifiers can utilize most any standard circuit architecture with enhanced simultaneous bandwidth/efficiency/power performance."

Ray Pengelly from Cree noted that, "There has also been much success designing very high efficiency Class E, F, inverse F, J, etc. PAs (with GaN). Doherty (Class A/B/C) with DPD have addressed a range of telecommunications applications. We today achieve efficiencies > 50 percent at peak power levels as high as 500 W. PAs associated with Envelope Tracking (ET), where the high breakdown aspects of GaN, allow drain voltage operation anywhere from 20 to 65 V again with efficiencies exceeding 50 percent. ET is particularly promising for multi-band telecom applications."

TriQuint recently introduced its PowerBand™ family of wideband, high power discrete transistors employing a "revolutionary" (and somewhat secretive) circuit architecture and process technology. The product portfolio is based on different semiconductor technologies, including TriQuint's GaAs PHEMT, LDMOS and GaN materials and processes. The first released LDMOS device operates from 500 MHz to 2 GHz and produces 30 W, P1dB (instantaneous bandwidth), while a GaN-based product that will produce 100 W P1dB CW is expected this year.

Changes to infrastructure architecture will have an impact on how devices will compete. There is a desire by network operators to move the power amplifier from the base of the radio tower closer to the antenna, so that the losses attributed to long cable runs can be eliminated. This will reduce the power required out of the amplifier. The Remote Radio Head (RRH) architecture can increase overall efficiency of the network from 13 to 15 percent up to 30 percent, but requires smaller and lighter amplifiers than those found in the cabinet of a base station. In addition, since the amplifier is on top of a tower, reliability takes on a new importance. The higher operating temperature, higher power density (and therefore smaller device periphery) and better efficiency are strong drivers for using GaN or SiC in the growing RRH market.

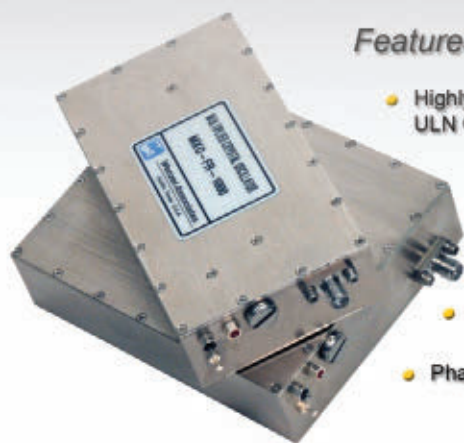
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MXO-500	500 MHz	+13	-115	-143	-158	-160	≤ -25	≤ -80	≤ -80	+15	2.25 x 4 x 1"
MXO-640	640 MHz	+13	-110	-137	-153	-155	≤ -25	≤ -80	≤ -80	+15	3.205 x 4 x 1"
MXO-1000	1 GHz	+13	-108	-136	-151	-153	≤ -25	≤ -70	≤ -80	+15	2.25 x 4 x 1"
MXO-1280	1.28 GHz	+13	-103	-130	-146	-148	≤ -25	≤ -80	≤ -80	+15	3.205 x 4 x 1"
MXO-2560	2.56 GHz	+13	-98	-123	-139	-141	≤ -25	≤ -80	≤ -80	+15	4.16 x 4 x 1"
MXO-5120	5.12 GHz	+13	-89	-116	-132	-134	≤ -25	≤ -80	≤ -80	+15	4.16 x 4 x 1"
MXO-10000	10 GHz	+13	-87	-115	-130	-132	≤ -25	≤ -80	≤ -80	+15	4.16 x 4 x 1"

Notes:
1. Contact factory for custom frequency options, to 12 GHz.
2. Output levels to +21 dBm on some models.
3. +12 VDC supply voltage option available on some models.



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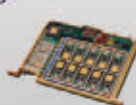
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choice for cellular and 3G base station applications, completely replacing the BJT with its higher gain and efficiency, and superior linearity. A typical 28 V LDMOS FET has a power density in the range of 0.7 to 1 W/mm with improvements occurring for each new generation.

Cree has reported GaN-on-SiC power densities of approximately 4 W/mm, meaning that less die size is required for GaN for the same amount of output power compared to LD-

MOS. Higher power density helps offset GaN's higher cost by increasing the number of die per wafer, yet not enough to surpass the price advantage held by LDMOS. Despite more chips per wafer, GaN is processed on smaller (SiC) wafer substrates whereas LDMOS is processed on much larger and cheaper Si wafers.

Benefits: Costs—LDMOS has the lowest cost per watt (\$/W) ratio of any of the high power RF amplifier technologies. LDMOS also has some of

the best Class AB linearity, gain, reliability and thermal resistance of any popular RF power technologies.

Where to use: LDMOS excels in high volume, medium to high power, linear systems with very stringent cost goals and very high reliability requirements.

Working with the technology: After years in the field, LDMOS has a solid track record. There are very highly developed and extensively used MMICs in the market place as multi-stage RF drivers and gain blocks. Freescale, for example, has a very extensive internal library of on-chip silicon passive components to design a wide variety of internally matched, temperature compensated, multi-stage RF MMIC devices with power levels ranging from 10 to 100 W. Large signal model (MET) includes thermal behavior.

Downside: LDMOS performance is excellent up to 3.8 GHz, but degrades rapidly beyond 4 GHz.

The Power Brokers: Freescale Semiconductor, RFMD, TriQuint, NXP Semiconductors, Integra Technologies, Infineon Technologies and ST Microelectronics.

GaN

Summary: GaNs early development dates back to the late 1990s, with funding largely from defense agencies such as DARPA. By the second half of this decade, GaN began to enter commercial markets with performance that challenged the prevailing technologies. Adoption of GaN has hinged on performance, cost and reliability, all of which has been favorable enough for the technology to make impressive penetration into several key high power markets.

Thermal management is key to achieving acceptable reliability. Because of this, GaN manufacturers use varying techniques to manage thermal rise. Most GaN suppliers use silicon carbide (SiC) as the substrate of choice due to its inherent high thermal conductivity. GaN-on-Si manufacturers use the ability to process very thin wafers with large die areas to achieve the same result. Along with SiC and Si, GaN is also processed on diamond, sapphire and silicon substrates. The diversity of substrates by individual vendors further segments the GaN family of devices.

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Frequency (MHz)	Gain Typ. (dB)	NF (dB)	OIP3 Typ. (dBm)	OP ₁ dB	Vdc (V)	Quiescent Current Typ. (mA)	Package (mm)	Part Number
LF-7	12.5	5.5	29	12.5	3.5	40	SOT-89	SKY65013-70LF
LF-12	12.5	5.8	29	12.5	3.5	40	SC-88	SKY65013-92LF
LF-6	16	4.8	36	18	4.7	70	SOT-89	SKY65014-70LF
LF-9	15	5.4	36	18	4.7	70	SC-88	SKY65014-92LF
LF-6	18	4.2	35	17	4.7	70	SOT-89	SKY65015-70LF
LF-6	18	4.8	35	18	4.7	70	SC-88	SKY65015-92LF
LF-3	20	4.8	27	14	3.5	40	SOT-89	SKY65016-70LF
LF-3	20	5.4	27	14	3.5	40	SC-88	SKY65016-92LF
LF-6	20	4.5	35	20	5	100	SOT-89	SKY65017-70LF

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- Typical gain up to 20 dB
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Frequency (MHz)	Gain Typ. (dB)	NF (dB)	OIP3 Typ. (dBm)	OP ₁ dB	Vdc (V)	Quiescent Current Typ. (mA)	Package (mm)	Part Number
0.25-2.7	16	5.5	42	25	3.3 or 5	125	3-pin MCM 4 x 4	SKY65004
0.25-2.7	20	3	33	21	3.3	76	3-pin MCM 4 x 4	SKY65008
0.25-2.5	12	4.3	42	27	3.3 or 5	100	4-pin SOT-89	SKY65009-70LF
0.25-2.7	16	5.5	42	25	3.3 or 5	125	4-pin SOT-89	SKY65028-70LF
0.25-6	15	2	40	21.5	3 to 5	140	4-pin SOT-89	SKY65038-70LF
0.39-1.5	14	1.8	37.5	25	5	46	4-pin SOT-89	SKY65045-70LF
1.5-2.5	14	2.1	38	21	5	47	4-pin SOT-89	SKY65080
0.4-2.3	18		39	27	5	260	SOIC-8 Exposed Paddle	SKY65112-84LF
0.4-2.3	20		40	30	5	450	SOIC-8 Exposed Paddle	SKY65113-84LF

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- WLAN
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- High gain
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SiC Pros:

- Greater than 3x better thermal conductivity of SiC vs Si (4.9 W/cm²K vs. 1.5 W/cm²K), supporting higher junction temperatures, reducing system complexity and weight
- Lower parasitic capacitance
- Epitaxial growth of GaN is better on SiC due to smaller lattice mismatch (3.4 percent on SiC vs. 17 percent on Si)
- Lower TEC mismatch on SiC (+25 percent for SiC vs. +100 percent on Si)

Si Pros:

- Silicon can be readily processed in very thin finished form, compensating for the higher thermal conductivity of the substrate relative to SiC
- The low cost and high yield of silicon allows larger die to be used, letting die designers spread heat over a larger area than SiC
- Lower cost than SiC, although this factor is expected to decrease with increasing volume of SiC substrates manufactured over time
- Supply chain advantage from wafer procurement, wafer processing, die attach and packaging can be second sourced by several existing well respected companies to avoid single thread manufacturing steps as well as the ability to scale production to support high volume requirements.

Benefits: GaN has high breakdown voltages (typically 100 to 200 V), higher power densities than LDMOS and higher ft depending on gate length (anywhere from 20 to > 150 GHz). The transistors have low capacitance per

watt resulting in higher output impedances, which leads to easier matching networks and relatively wide band performance.

Where to use: GaN is the high power transistor of choice above 4 GHz and is making inroads at lower frequencies with applications that can afford the higher price compared to LDMOS.

Working with the technology: GaN HEMTs in hybrid, discrete designs are most suited to Class A/B, Doherty, push-pull, feedback and lossy match, etc. For MMICs, a range of amplifier techniques ranging from distributed, through multi-stage and cascode implementations have been proven and many are now in production or pre-production. Today's commercially available GaN-on-SiC HEMTs usually use either copper-moly-copper or copper-tungsten flanged packages. In some special cases more elaborate heat-sinking is required using advanced materials, such as those containing diamond, but they are less mature and tend to be expensive. In some critical applications where liquid cooling may not be available, that option may be acceptable. The transistors can also be "spread out" to reduce heat density, but this can have an impact on the frequency of operation of the devices as well as the number of parts that can be produced on each wafer. Models are available for popular RF/microwave design software depending on the device manufacturer.

Downside: Currently more expensive than LDMOS, relative lack of field data and minimal reliability data based on life history of the technology.



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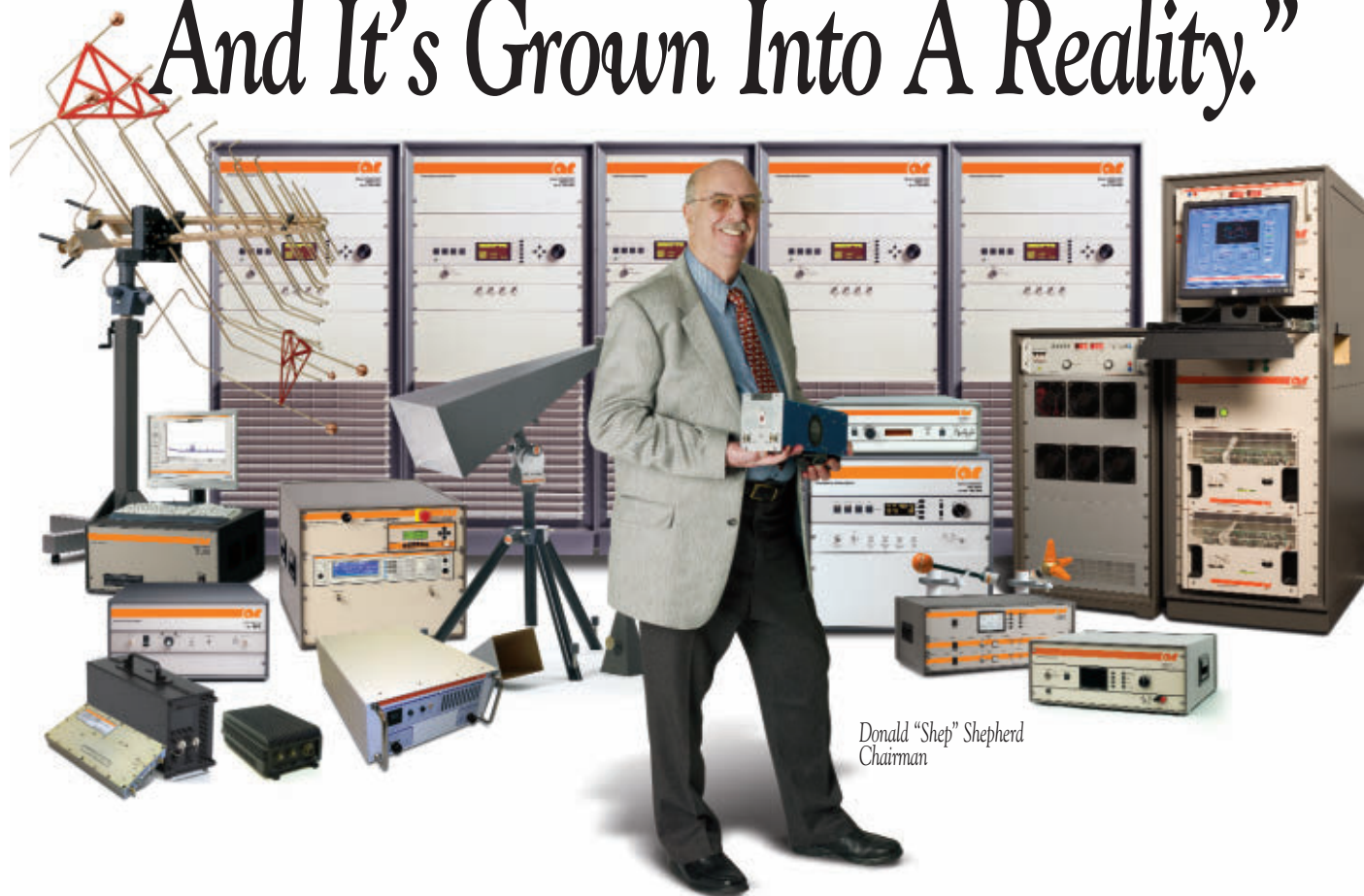
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The Power Brokers: RFMD, Nitronex, TriQuint, Eudyna, Cree, Toshiba, NEC, Fujitsu and Matsushita MEI/Panasonic.

SiC

Summary: The larger thermal conductivity of SiC and GaN enables lower temperature rise due to self heating. The five to six times' higher breakdown field of SiC and GaN is what gives those materials the advantage over Si and GaAs for RF power devices.⁵ SiC is a wide bandgap material (3.26 eV), but suffers from poor electron transport properties, which hinders its use in very high frequency amplifiers. SiC has also been limited by expensive, small and low-quality substrate wafers.

In addition, the new SiC devices from Microsemi are fabricated with 100 percent gold metallization and gold wires in hermetically sealed packages (measuring a compact 0.9×0.4 in, which is 50 percent smaller than the highest power devices in BJT or LDMOS). This gives the technology the highest reliability in weather radar and long-range tracking radar applications (i.e. providing military-grade long-term reliability), according to the company. The product capability at 10:1 load mismatch tolerance performance also improves system yields. Cree boosts using the same epoxy sealed (gross leak proof) ceramic/metal packages used for GaN HEMTs. The semiconductors are fully passivated providing MTTFs greater than 1 million hours at transistor junction temperatures of 225°C.

Benefits: Microsemi says that typical silicon-based RF

power transistor solutions offered throughout the industry, such as BJT (bipolar junction transistor) or LDMOS (laterally diffused metal oxide semiconductor) devices must use complex push-pull circuit designs to achieve similar power levels. In contrast, the SiC RF power transistors have a single-ended design with simplified impedance matching.

Where to use: Radar and avionics where higher power levels (up to the kilowatt range) at UHF and VHF frequencies are required. Development is pushing the frequency range higher.

Downside: Smaller number of suppliers and limited frequency.

The Power Brokers: Microsemi and Cree Inc.

References

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3. "GaN RF Market 2008," Yole Développement. Available at <http://www.yole.fr/pagesAn/products/ganrf.asp>.
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5. C.E. Weitzel, "RF Power Devices for Wireless Communications," *IEEE MTT-S Digest*, Vol. 1, 2-7 June 2002, pp. 285-288.

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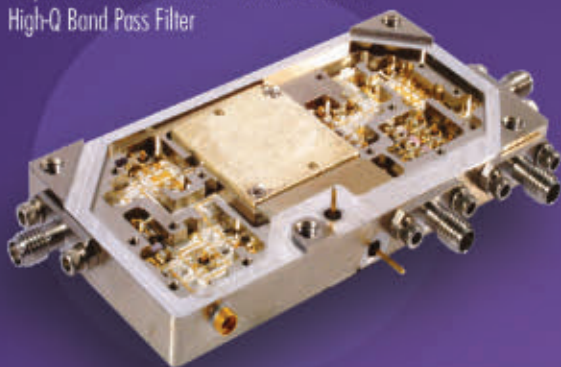
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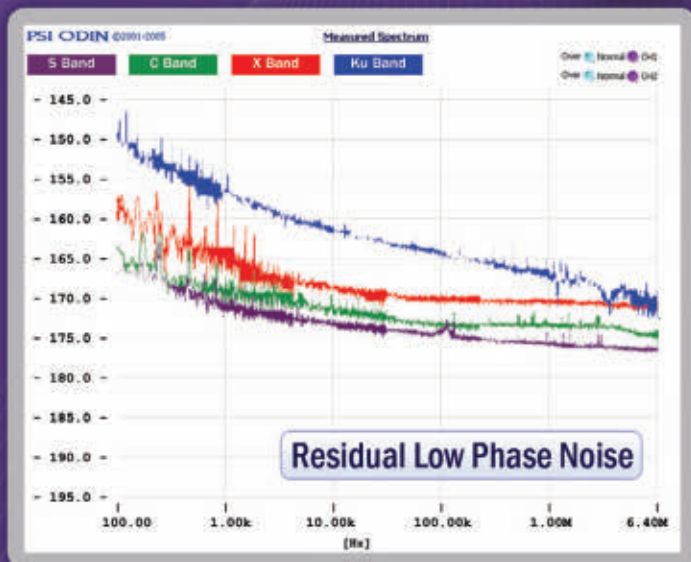
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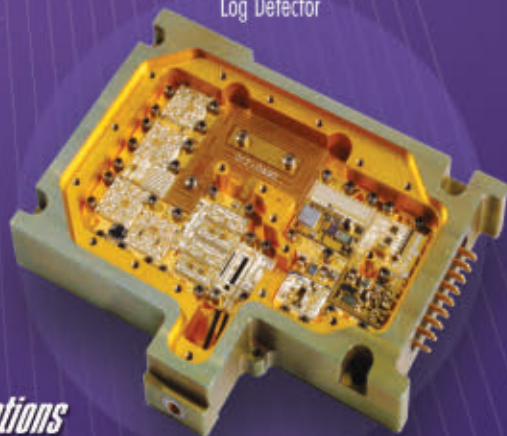
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Description	Frequency (GHz)	Power (Vpp or dBm)	Gain (dB)	Noise Figure (dB)	Voltage / Current (V / mA)	Package Style	Part Number
10.7 Gb/s Diff. TIA	DC - 10	-	8K dB Ω SE	6pA $\sqrt{\text{Hz}}$	3.3 / 80	Die	TGA4815
10.7 Gb/s Diff. TIA	DC - 10	-	1.6K dB Ω SE	6pA $\sqrt{\text{Hz}}$	3.3 / 60	Die	TGA4816
10.7 Gb/s Diff. TIA	DC - 10	-	3.2K dB Ω SE	11pA $\sqrt{\text{Hz}}$	3.3 / 70	Die	TGA4817
9.9 - 12.5 Gb/s 3V - 7V Driver	DC - 13	3 - 7 Vpp	20	-	3.3 - 5 / 100	SM-A5-28	TGA4955-SM**
9.9 - 12.5 Gb/s 3V - 7V Driver	DC - 13	3 - 7 Vpp	32	-	3.3 - 5 / 115	SM-A8-28	TGA4956-SM*
40 Gb/s LN / MZ Mod. Driver	DC - 35	5 - 8 Vpp	30	-	8 / 300	SL-A7-21	TGA4942-SL**
28 Gb/s 8Vpp SE Driver	DC - 30	3 - 9Vpp	32	-	6 - 7 / 270	SL-A7-21	TGA4943-SL*
9.9 - 12.5 Gb/s Mod. Driver	DC - 16	3V - 10V	35	2.5	5.5 - 8 / 210	SL-A2-18	TGA4953-SL
9.9 - 12.5 Gb/s Mod. Driver	DC - 16	3V - 10V	35	2.5	5.5 - 8 / 210	SL-A4-18	TGA4954-SL
12.5 Gb/s NRZ Driver	DC - 18	11V	16	-	8 / 285	Die	TGA4807
12.5 Gb/s NRZ Driver	DC - 18	24 dBm	16	3.5	5 - 8 / 70 - 175	Die	TGA1328-SCC
12.5 Gb/s NRZ Driver	DC - 18	8V	16	3.5	8 / 175	SL-A1-12	TGA8652-SL
12.5 Gb/s RZ Driver	DC - 25	7V	15	-	9 / 100	Die	TGA4802
43 Gb/s NRZ Driver	DC - 35	7V	15	-	6.5 / 170	Die	TGA4801
Wideband Driver (40 Gb/s)	DC - 35	4V	12	-	5 / 135	Die	TGA4832
40 Gb/s TIA, SE	DC - 40	-	250 dB Ω	15pA $\sqrt{\text{Hz}}$	5 / 30	Die	TGA4812
LNA / Gain Block	DC - 40	11.5 dBm	13	3.2	5 / 50	Die	TGA4830
LNA / Gain Block	DC - 60	13 dBm	15	3	6 / 50	Die	TGA4811
43 Gb/s Driver	DC - 78	3V	8	5	6 / 82	Die	TGA4803
10.7 - 12.5 Gb/s Linear Mod. Driver	0.03 - 8	25 dBm	20	-	8 / 310	SM-A8-28	TGA4823-2-SM
CATV TIA / Gain Block, SB	0.04 - 1	27 dBm	20	1.5	8 / 350	SM-O8-20	TGA2803-SM

NOTES: * = New, ** = Coming Soon, SB = Self Biased, SE = Single-Ended

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OCTAVE BAND LOW NOISE AMPLIFIERS

Model No.	Freq (GHz)	Gain (dB) MIN	Noise Figure (dB)	Power-out @ P1-dB	3rd Order ICP	VSWR
CA01-2110	0.5-1.0	28	1.0 MAX, 0.7 TYP	+10 MIN	+20 dBm	2.0:1
CA12-2110	1.0-2.0	30	1.0 MAX, 0.7 TYP	+10 MIN	+20 dBm	2.0:1
CA24-2111	2.0-4.0	29	1.1 MAX, 0.95 TYP	+10 MIN	+20 dBm	2.0:1
CA48-2111	4.0-8.0	29	1.3 MAX, 1.0 TYP	+10 MIN	+20 dBm	2.0:1
CA812-3111	8.0-12.0	27	1.6 MAX, 1.4 TYP	+10 MIN	+20 dBm	2.0:1
CA1218-4111	12.0-18.0	25	1.9 MAX, 1.7 TYP	+10 MIN	+20 dBm	2.0:1
CA1826-2110	18.0-26.5	32	3.0 MAX, 2.5 TYP	+10 MIN	+20 dBm	2.0:1

NARROW BAND LOW NOISE AND MEDIUM POWER AMPLIFIERS

CA01-2111	0.4 - 0.5	28	0.6 MAX, 0.4 TYP	+10 MIN	+20 dBm	2.0:1
CA01-2113	0.8 - 1.0	28	0.6 MAX, 0.4 TYP	+10 MIN	+20 dBm	2.0:1
CA12-3117	1.2 - 1.6	25	0.6 MAX, 0.4 TYP	+10 MIN	+20 dBm	2.0:1
CA23-3111	2.2 - 2.4	30	0.6 MAX, 0.45 TYP	+10 MIN	+20 dBm	2.0:1
CA23-3116	2.7 - 2.9	29	0.7 MAX, 0.5 TYP	+10 MIN	+20 dBm	2.0:1
CA34-2110	3.7 - 4.2	28	1.0 MAX, 0.5 TYP	+10 MIN	+20 dBm	2.0:1
CA56-3110	5.4 - 5.9	40	1.0 MAX, 0.5 TYP	+10 MIN	+20 dBm	2.0:1
CA78-4110	7.25 - 7.75	32	1.2 MAX, 1.0 TYP	+10 MIN	+20 dBm	2.0:1
CA910-3110	9.0 - 10.6	25	1.4 MAX, 1.2 TYP	+10 MIN	+20 dBm	2.0:1
CA1315-3110	13.75 - 15.4	25	1.6 MAX, 1.4 TYP	+10 MIN	+20 dBm	2.0:1
CA12-3114	1.35 - 1.85	30	4.0 MAX, 3.0 TYP	+33 MIN	+41 dBm	2.0:1
CA34-6116	3.1 - 3.5	40	4.5 MAX, 3.5 TYP	+35 MIN	+43 dBm	2.0:1
CA56-5114	5.9 - 6.4	30	5.0 MAX, 4.0 TYP	+30 MIN	+40 dBm	2.0:1
CA812-6115	8.0 - 12.0	30	4.5 MAX, 3.5 TYP	+30 MIN	+40 dBm	2.0:1
CA812-6116	8.0 - 12.0	30	5.0 MAX, 4.0 TYP	+33 MIN	+41 dBm	2.0:1
CA1213-7110	12.2 - 13.25	28	6.0 MAX, 5.5 TYP	+33 MIN	+42 dBm	2.0:1
CA1415-7110	14.0 - 15.0	30	5.0 MAX, 4.0 TYP	+30 MIN	+40 dBm	2.0:1
CA1722-4110	17.0 - 22.0	25	3.5 MAX, 2.8 TYP	+21 MIN	+31 dBm	2.0:1

ULTRA-BROADBAND & MULTI-OCTAVE BAND AMPLIFIERS

Model No.	Freq (GHz)	Gain (dB) MIN	Noise Figure (dB)	Power-out @ P1-dB	3rd Order ICP	VSWR
CA0102-3111	0.1-2.0	28	1.6 Max, 1.2 TYP	+10 MIN	+20 dBm	2.0:1
CA0106-3111	0.1-6.0	28	1.9 Max, 1.5 TYP	+10 MIN	+20 dBm	2.0:1
CA0108-3110	0.1-8.0	26	2.2 Max, 1.8 TYP	+10 MIN	+20 dBm	2.0:1
CA0108-4112	0.1-8.0	32	3.0 MAX, 1.8 TYP	+22 MIN	+32 dBm	2.0:1
CA02-3112	0.5-2.0	36	4.5 MAX, 2.5 TYP	+30 MIN	+40 dBm	2.0:1
CA26-3110	2.0-6.0	26	2.0 MAX, 1.5 TYP	+10 MIN	+20 dBm	2.0:1
CA26-4114	2.0-6.0	22	5.0 MAX, 3.5 TYP	+30 MIN	+40 dBm	2.0:1
CA618-4112	6.0-18.0	25	5.0 MAX, 3.5 TYP	+23 MIN	+33 dBm	2.0:1
CA618-6114	6.0-18.0	35	5.0 MAX, 3.5 TYP	+30 MIN	+40 dBm	2.0:1
CA218-4116	2.0-18.0	30	3.5 MAX, 2.8 TYP	+10 MIN	+20 dBm	2.0:1
CA218-4110	2.0-18.0	30	5.0 MAX, 3.5 TYP	+20 MIN	+30 dBm	2.0:1
CA218-4112	2.0-18.0	29	5.0 MAX, 3.5 TYP	+24 MIN	+34 dBm	2.0:1

LIMITING AMPLIFIERS

Model No.	Freq (GHz)	Input Dynamic Range	Output Power Range Psat	Power Flatness dB	VSWR
CLA24-4001	2.0 - 4.0	-28 to +10 dBm	+7 to +11 dBm	+/- 1.5 MAX	2.0:1
CLA26-8001	2.0 - 6.0	-50 to +20 dBm	+14 to +18 dBm	+/- 1.5 MAX	2.0:1
CLA712-5001	7.0 - 12.4	-21 to +10 dBm	+14 to +19 dBm	+/- 1.5 MAX	2.0:1
CLA618-1201	6.0 - 18.0	-50 to +20 dBm	+14 to +19 dBm	+/- 1.5 MAX	2.0:1

AMPLIFIERS WITH INTEGRATED GAIN ATTENUATION

Model No.	Freq (GHz)	Gain (dB) MIN	Noise Figure (dB)	Power-out @ P1-dB	Gain Attenuation Range	VSWR
CA001-2511A	0.025-0.150	21	5.0 MAX, 3.5 TYP	+12 MIN	30 dB MIN	2.0:1
CA05-3110A	0.5-5.5	23	2.5 MAX, 1.5 TYP	+18 MIN	20 dB MIN	2.0:1
CA56-3110A	5.85-6.425	28	2.5 MAX, 1.5 TYP	+16 MIN	22 dB MIN	1.8:1
CA612-4110A	6.0-12.0	24	2.5 MAX, 1.5 TYP	+12 MIN	15 dB MIN	1.9:1
CA1315-4110A	13.75-15.4	25	2.2 MAX, 1.6 TYP	+16 MIN	20 dB MIN	1.8:1
CA1518-4110A	15.0-18.0	30	3.0 MAX, 2.0 TYP	+18 MIN	20 dB MIN	1.85:1

LOW FREQUENCY AMPLIFIERS

Model No.	Freq (GHz)	Gain (dB) MIN	Noise Figure dB	Power-out @ P1-dB	3rd Order ICP	VSWR
CA001-2110	0.01-0.10	18	4.0 MAX, 2.2 TYP	+10 MIN	+20 dBm	2.0:1
CA001-2211	0.04-0.15	24	3.5 MAX, 2.2 TYP	+13 MIN	+23 dBm	2.0:1
CA001-2215	0.04-0.15	23	4.0 MAX, 2.2 TYP	+23 MIN	+33 dBm	2.0:1
CA001-3113	0.01-1.0	28	4.0 MAX, 2.8 TYP	+17 MIN	+27 dBm	2.0:1
CA002-3114	0.01-2.0	27	4.0 MAX, 2.8 TYP	+20 MIN	+30 dBm	2.0:1
CA003-3116	0.01-3.0	18	4.0 MAX, 2.8 TYP	+25 MIN	+35 dBm	2.0:1
CA004-3112	0.01-4.0	32	4.0 MAX, 2.8 TYP	+15 MIN	+25 dBm	2.0:1

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Harris Corp. Awarded \$600 M to Modernize US Strategic Satellite Communications

the worldwide backbone for high-priority military communications and missile defense systems. As prime contractor, Harris will develop, test and certify four unique terminal configurations during a 30-month, First Article Test phase. In addition, Harris will provide production hardware under the five-year base contract, with five additional option years, and will support field activities such as site preparation, installation, test, operations and maintenance. The program will be managed by Team DCATS—Project Manager, Defense Communications and Army Transmission Systems.

Harris will replace up to 80 AN/GSC-52, AN/GSC-39, AN/FSC-78 and other aging strategic satellite communications terminals around the world with new, simultaneous X- and Ka-band terminals capable of interfacing with the new Wideband Global Satellite constellation as well as with legacy satellite systems. The new terminals will support Internet Protocol and Dedicated Circuit Connectivity within the Global Information Grid, providing critical reach-back capability for the warfighter.

"MET leverages our long and successful track record of success on the AN/GSC-52 terminal modernization program to provide PMDCATS with an advanced, strategic terminal architecture that achieves a high level of equipment and integration commonality, thereby lowering acquisition and logistics costs," said Wes Covell, President of Defense Programs for Harris Government Communications Systems. "Harris is proud to provide the next generation of strategic, multiband terminals for the Department of Defense, and we look forward to expanding our successful relationship with PMDCATS through the MET program."

Harris teammates on the MET program include General Dynamics SATCOM Technologies, a leader in X- and Ka-band satellite communications products; O'Neil & Associates, a supplier of world-class logistics and interactive, electronic technical manuals; and Janus Research Group, an innovator in training simulation. The hardware will include various fixed ground terminal configurations; a hardened, transportable terminal and a small terminal suitable for rooftop mounting. General Dynamics SATCOM Technologies will develop the X-band antenna feed as well as a dual/simultaneous X- and Ka-band antenna feed capable of meeting the stringent requirements for low intermodulation products. They will also develop 12.2-meter antennas for fixed ground terminals, 7.2-meter antennas for transportable terminals and 4.8-meter antennas for small terminals. The first terminal is scheduled for fielding in early 2011.

Lockheed Martin Rolls Out THAAD Launchers, Fire Control and Communications

Lockheed Martin officially rolled out the new Terminal High Altitude Area Defense (THAAD) Weapon System launcher and Fire Control and Communications unit in a ceremony at the company's THAAD Launcher Integration Complex in Camden, AR. The ceremony, attended by US Senator Mark Pryor and US Congressman Mark Ross, commemorated the delivery of the first THAAD ground segment vehicles to come off the production line in Camden.

The new hardware will be delivered to soldiers at Fort Bliss, TX, who will have a fully operational THAAD battery (equipment and personnel) by the end of 2009. "What the hardworking employees of Lockheed Martin's Camden Operations have accomplished in such a short time is a testament to their dedication to our troops," said US Senator Mark Pryor. "It gives me great pride to know that one of the world's most advanced and proven air defense systems are produced, in part, here in the great state of Arkansas."

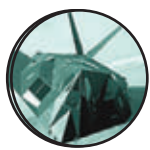
"The THAAD system will play a pivotal role in our nation's missile defense, and today's rollout is an encouraging sign of the tremendous progress we are making in this vital technology," said US Congressman Mike Ross. "The Camden area employees of Lockheed Martin have a long history of success and today is no exception. I thank them for their hard work in providing our military with the technology it needs to protect and defend our troops and our homeland."

"This is truly a great day for air defenders," said Tom McGrath, Vice President of the THAAD program at Lockheed Martin. "We are proud to deliver this proven air defense capability to our forces. We are seeing the incredible power of THAAD to protect our warfighters and population centers with each successful test flight, and now we are seeing the reality of production hardware rolling off the line."

Lockheed Martin is the prime contractor and systems integrator for the THAAD Weapon System. The company's new 200,000 square-foot Launcher Integration Complex at Camden Operations currently has an employee population of approximately 600. "This is an outstanding example of government/industry partnership to achieve great things for the warfighter," said Glenn David Woods, Camden Operations Plant Manager for Lockheed Martin Missiles and Fire Control. "Our commitment is to produce the world's most advanced and effective air defense capability for our soldiers and allies."

Northrop Grumman Space & ISR Systems Joins Raytheon-led Team IBCS

Another industry partner has joined the Raytheon Co.-led team for the US Army's Integrated Battle Command System (IBCS) program. Northrop Grumman Corp.'s Space & ISR Systems Division facility in



Boulder, CO, joins the other partners of Team IBCS including Raytheon, General Dynamics, Teledyne Brown Engineering, Davidson Technologies, IBM and Carlson Technologies, as well as academia partners. The new team member brings expertise in evaluating warfighter benefits of space-based data to the IBCS architecture. The Northrop Grumman Space & ISR Systems Division performs work at Buckley and Schriever Air Force Bases elsewhere in Colorado.

IBCS is a US Army and joint development program with a modular, open architecture, system-of-systems construct allowing air and missile defense warfighters to use any sensor and any shooter within an integrated fire control network. Raytheon won the first stage of a competitive, multi-phase Army award for IBCS in late September 2008.

Team IBCS was formed using OpenAIR™, Raytheon's open business model that uses the best of large and small businesses and academia to provide the best value solution. "The addition of Northrop Grumman Space & ISR Systems to the team reinforces our commitment to providing warfighters with advanced capabilities early as well as exemplifying the tenets of our open air objective and best-of-breed approach," said Dan Kirby, the win leader for Team IBCS.

"Raytheon's Team IBCS is a specifically tailored team devoted to partnering with our Army customer to provide our warfighters the next 'unfair advantage' on current and future battlefields against all aerial threats," added John Urias, Vice President of the Raytheon Battlespace Integration Directorate.

Air and Missile Defense systems included in the IBCS program architecture are weapon and sensor systems already developed and produced by Raytheon, including the Patriot air and missile defense system; JLENS (Joint Land-Attack Cruise Missile Defense Elevated Netted Sensor System); SLAMRAAM (Surface-Launched Advanced Medium-Range Air-to-Missile); the Sentinel Radar; and the THAAD (Terminal High-Altitude Air Defense) radar.

A preliminary design review for the Integrated Battle Command System was scheduled for May 2009, and a single award for phase two of the program is expected in late August 2009. Integrated Defense Systems is Raytheon's leader in Global Capabilities Integration providing affordable, integrated solutions to a broad international and domestic customer base, including the United States Missile Defense Agency, the United States Armed Forces and the Department of Homeland Security.

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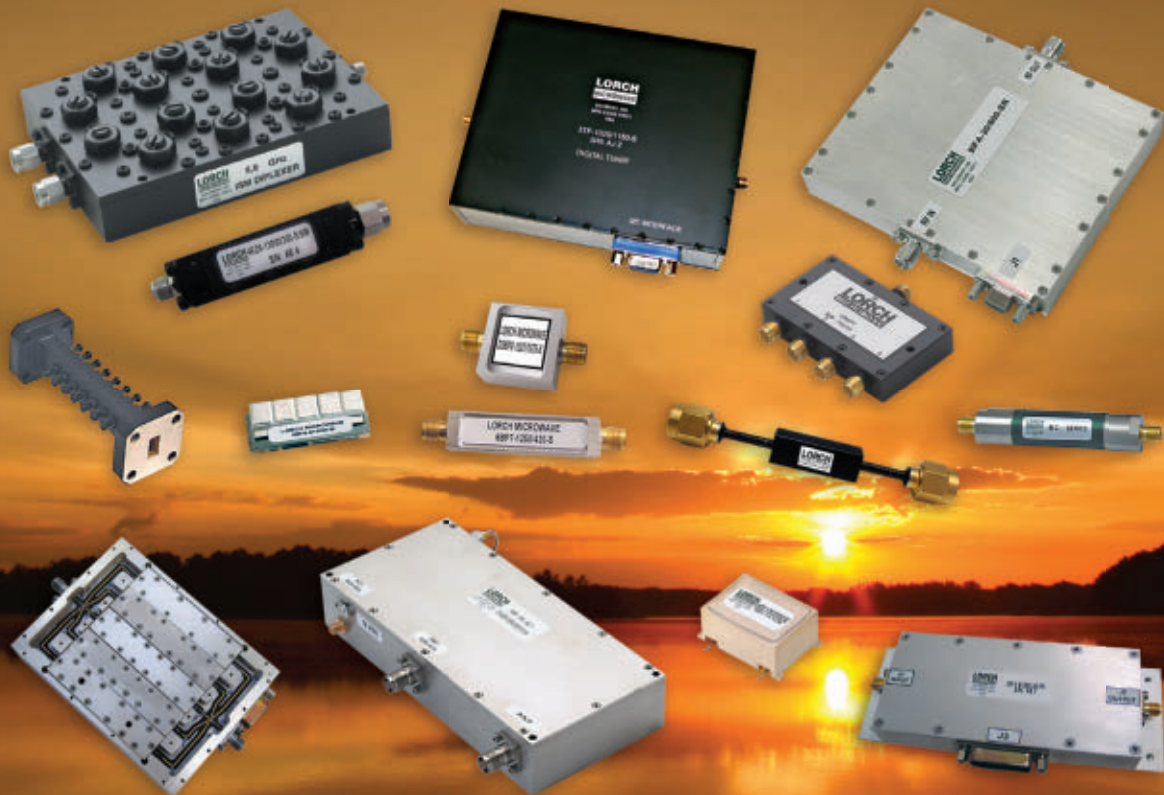
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20 - 150 MHz, minimum	≥ 40 dB @ 200 MHz & ≥ 50 dB @ 300 - 600 MHz
20 - 220 MHz, minimum	≥ 40 dB @ 300 MHz & ≥ 50 dB @ 450 - 900 MHz
20 - 335 MHz, minimum	≥ 40 dB @ 440 MHz & ≥ 50 dB @ 660 - 1400 MHz
20 - 500 MHz, minimum	≥ 35 dB @ 670 MHz & ≥ 50 dB @ 1005 - 2000 MHz
20 - 700 MHz, minimum	≥ 40 dB @ 980 MHz & ≥ 50 dB @ 1470 - 2000 MHz
20 - 1010 MHz, minimum	≥ 35 dB @ 1400 MHz & ≥ 50 dB @ 2100 - 3000 MHz
20 - 1400 MHz, minimum	≥ 40 dB @ 2000 MHz & ≥ 50 dB @ 3000 - 4200 MHz
20 - 2000 MHz, minimum	≥ 40 dB @ 2800 MHz & ≥ 50 dB @ 4200 - 5000 MHz
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EADS DS and Larsen & Toubro Join Forces in India

EADS Defence & Security (DS) and Indian engineering giant Larsen & Toubro (L&T), Mumbai, are to join forces in the fields of defence technology. Subject to approval by the Indian Government the plan is for the formation of a joint venture company for defence electronics in India, based in Talegaon near Pune.

The proposed joint venture has the potential to become the leading Indian Electronics House for defence and security. The new company will aim at design, development, manufacturing and related services in the fields of electronic warfare, radar, military avionics and mobile systems for military applications.

The Indian defence and security market is growing fast and EADS intends to grow with it. Via this joint venture EADS plans to move beyond just providing high technology sales to India by creating an Indian industrial base with the development of a long-term partnership, including the transfer of technology wherever necessary.

The joint venture company will develop and manufacture indigenous solutions for military requirements of Indian customers as well as the world market. Thus, the Indian JV company will provide the armed forces with locally produced high tech equipment and assured life-time support.

A.M. Naik, chairman and managing director of L&T, said, "For over two decades, L&T has been a major supplier of critical systems to India's defence forces. These include a wide range of products like weapon launchers, naval systems, radar systems, etc. We welcome the formation of this joint venture that will create opportunities for development of state-of-the-art defence electronic products and systems for the Indian defence forces and for the rest of the world."

Dr. Stefan Zoller, CEO of EADS Defence & Security, added, "EADS DS is a high tech company driving the development of integrated system solutions for armed forces and civil security worldwide. We are proud of joining forces with one of India's biggest technology companies. Our joint venture is proof of our commitment to India."

TSB Funds Ultra Fast Broadband Initiative

A new initiative by the Technology Strategy Board (TSB), which addresses the development of Ultra Fast Broadband, looks set to be accelerated following the start of over a dozen innovative research and development feasibility projects. The result could be a major change in the way that businesses operate across the world.

TSB, the organisation that drives technological innovation in the UK, is investing £1 M to help companies carry out initial research that will ultimately lead to the introduction of Internet access technology with speeds of between 1 and 10Gb/s—100 to 1,000 times faster than current broadband speeds.

The feasibility projects—each costing between £30,000 and £100,000—will, in turn, help establish European collaborations that will participate in larger EU-funded research and development initiatives. The ultimate aim, the development of pan-European Ultra Fast Broadband, could see European companies gaining a massive competitive advantage on a global scale.

Commenting on the decision to fund the projects, Mike Biddle, lead technologist at the Technology Strategy Board, said, "The challenge is to identify ways to address the technical issues facing the introduction of Ultra Fast Broadband within the next decade and to build European collaborations to exploit the technology, while generating wealth for the UK. Our intention in providing this funding is to help British companies establish future European collaborations that will participate in larger EU funding initiatives."

NEC Mobile WiMAX Base Station Selected for Japan

UQ Communications Inc., a nationwide Japanese telecommunications carrier capitalizing on mobile WiMAX technologies, has selected NEC Corp. to supply mobile WiMAX base stations. The company has chosen to adopt NEC's recently developed PasoWings BS202 mobile WiMAX base station, which

is the first to be equipped with Uplink-Beam Forming (UL-BF) technologies. These technologies improve communications speed and increase the base station coverage area by reducing radio frequency interference between base stations and data transmission terminals.

The system's adoption follows NEC's work to acquire the WiMAX Forum's Wave 2 (2.5 GHz, 3.5 GHz) authentication and its actions to secure international standardization. A wide variety of functions and an external interface based on international standards enable the PasoWings BS202 system to be integrated with a broad range of vendors' equipment, which contributes to the smooth construction of WiMAX networks in short periods of time.

The base stations are compact and the adoption of a high efficiency amplifier enables the integration of outdoor units (ODU), which send and receive transmissions, with indoor units (IDU), which convert signals and control access. Also, reducing the space required to accommodate base stations, the time needed to construct them, and the resources necessary for maintenance reduces costs. NEC regards its selection to provide the PasoWings BS202 to UQ Communications as evidence of the high regard held for its products and services on a worldwide level.



ITP-IET Join Forces to Raise Standards

The Institute of Telecommunications Professionals (ITP) has formed a collaborative partnership with the Institution of Engineering and Technology (IET) to create a joint service exclusively for its members aimed at raising professional standards across the ICT sector. This joint ITP-IET member registration programme means that ITP members can apply for professional registration, using the IET, which is licensed by the Engineering Council UK to award professional qualifications. ITP members of this programme will be entitled to use qualification designatory letters CEng, IEng, EngTech or ICTTech after their name once they are awarded ECUK registration.

Michelle Richmond, IET Membership and Professional Development Director, said, "In the current economic climate it is more important than ever to set oneself apart from the competition. Professional registration does just this and shows commitment and dedication, as well as demonstrating to employers a range of skills. We are delighted to have formed this partnership, which is part of the IET's collaborative approach to raising professional standards and competence across the industry worldwide."

Motorola and Apprion Complete OEM Agreement

Apprion has signed an OEM agreement with Motorola Inc. that enables the two companies to jointly develop and market integrated wireless application networks for industrial enterprises. By integrating Apprion's industrial-focused wireless appliances and applications with Motorola's comprehensive line of indoor and outdoor wireless networking solutions, industrial enterprises will now be able to leverage best-of-class wireless networks, enabling them to support dozens of applications that utilize numerous wireless radios and protocols.

Through the OEM agreement, the two companies will initially incorporate wireless broadband systems and wireless LAN solutions from Motorola into the Apprion ION System. The second phase of enhancements will result in the full integration of Motorola products and technologies as modular components of Apprion's IONosphere and IONizer solutions.

The combination of technologies from the two companies will enable a wide range of applications. Examples include mobile safety applications, unified voice communications, perimeter security, predictive maintenance, and remote monitoring and optimization of critical assets.

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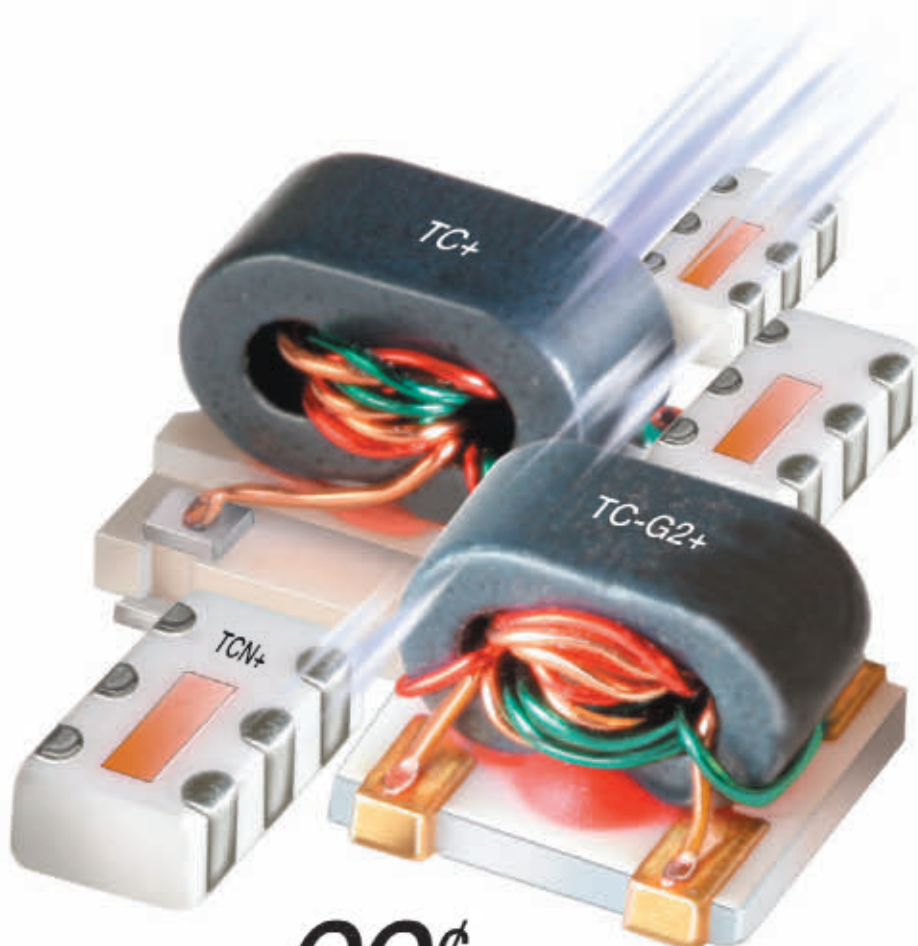
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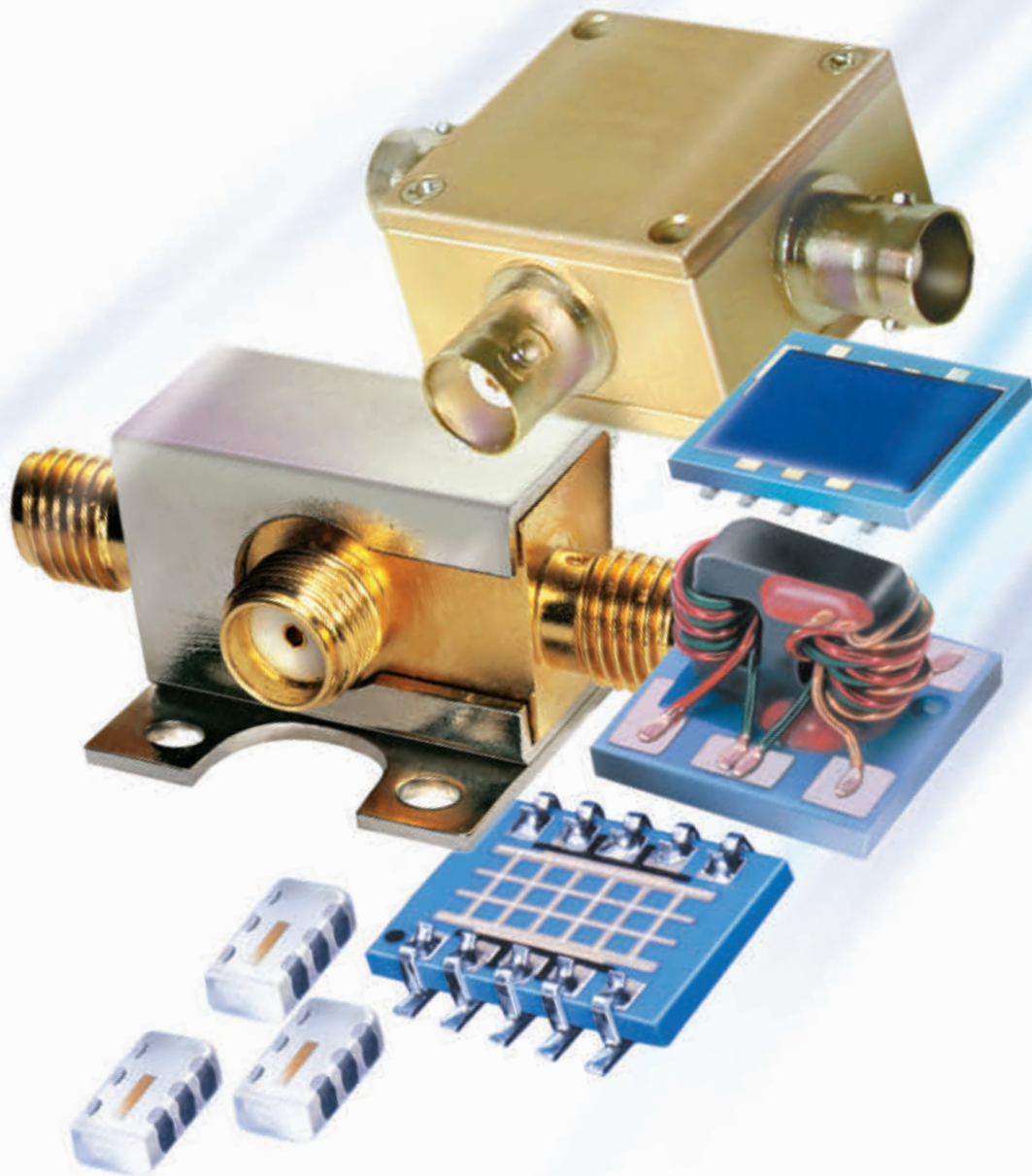


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Recession or Not, Wireless Backhaul Expansion Continues Strongly

performance? According to ABI Research senior analyst Nadine Manjaro, the main driver is the effort by mobile operators to prepare for an upgrade to LTE. "Operators might not deploy LTE immediately," she says, "but they know that before they do, they'll have to upgrade their backhaul capacity."

Backhaul is the bottleneck that can prevent a satisfactory 3G user experience. "AT&T Mobility has found that one iPhone user typically generates as much data traffic as 30 basic feature phone users," notes Manjaro. Wireless network traffic will dramatically increase as iPhone-like devices become the norm and laptop PC card usage increases. Another indicator is the growing capital expenditure on microwave backhaul, which will exceed \$8.5 B in 2009.

The market opportunities generated by this growth in backhaul are spread around the backhaul equipment vendors and fixed line operators. Some backhaul infrastructure vendors like Ericsson, Alcatel-Lucent and Nokia Siemens Network will benefit from operators' strong interest in Carrier Ethernet solutions. Major microwave equipment vendors like DragonWave and Harris Stratex will also benefit from increased microwave adoption. And fixed-line operators such as BT, Embarq, AT&T and Verizon Communications will develop new revenue streams by providing leased backhaul services.

Even the business models for backhaul are in flux. "We have observed a movement towards backhaul as a managed service," says Manjaro. "This enables mobile operators to focus on their core business, while guaranteeing a backhaul capacity matched to their changing traffic demands. BT provides that service to four of the top five European operators. In the US, Embarq is moving in the same direction, and I think more cable companies will follow suit. Wireline operators, who typically were losing business to wireless operators, can now get a piece of that wireless pie."

ABI Research's new study, "Mobile Backhaul—Global Market Analysis and Forecast," provides a comprehensive analysis of the global mobile backhaul market, including forecasts by region and technology. It is part of the firm's Mobile Networks Research Service.

ABI Research provides in depth analysis and quantitative forecasting of emerging trends in global connectivity.

Worldwide revenues from backhaul leasing are expected to double over the next 30 months, according to a new study from ABI Research. The growth curve even accelerates after 2012, resulting in a five-fold revenue increase between 2009 and 2014.

Why this powerful perfor-

Wireless Communications Sector to Benefit from \$6.8 B Stimulus Funding

is examined in depth by a new study from ABI Research.

"The ARRA represents a windfall for wireless service providers as well as for satellite service providers," comments vice president Stan Schatt. "It will have an enormous impact on Wi-Fi and wireless broadband vendors. It will also immediately benefit a number of specific vertical industries including healthcare, education, homeland security, the environment, and the nation's electricity infrastructure."

In healthcare, the scope for adding wireless to the technology mix encompasses Wi-Fi-enabled mobile devices and sensors, communications systems linking health networks, telepresence, wireless LAN equipment, and Wi-Fi-enabled video surveillance systems.

In education, already a leading adopter of Wi-Fi solutions, equipment vendors are developing templated solutions in such areas as WLANs for "learning anywhere," voice-over-Wi-Fi, and WLAN equipment and software to track students' progress for "No Child Left Behind" record keeping.

The Department of Homeland Security and US Customs and Border Protection are potential goldmines for wireless vendors because of the many agencies within them that will use ARRA funds for tactical communications equipment, infrastructure equipment, and security equipment. Even critical infrastructure construction projects such as bridges and tunnels often require wireless video surveillance systems.

Mobile Consumers Prepared to Support Green Initiatives

The results of a recent consumer survey conducted in North America by ABI Research suggest that nearly half of those mobile consumers surveyed are somewhat likely or very likely to be influenced by suppliers' green credentials when purchasing services or devices.

Respondents were asked whether they'd be more likely to purchase mobile services or mobile handsets from an operator that makes use of 'green' initiatives, which were described as:

"...gives money to organizations seeking to help the environment, actively employs programs that reduce its carbon footprint, buys network equipment from 'green' equipment vendors."

Paying more than just lip service, 41% (for services) and 45% (for devices) of the 1,000+ respondents indicated that



they'd be significantly or somewhat more likely to do so. Younger consumers showed a greater willingness to pursue "eco-groovy" mobile activities than older ones.

The service providers first to connect with environmentally conscious businesses and consumer subscribers will have an edge in this growing trend. Additional education remains necessary to communicate issues surrounding battery disposal and the accumulation of e-waste.

"If consumers are simply unaware of the environmental issues surrounding mobile devices and services," Orr adds, "then the industry should increase its efforts to get the message across. Some other verticals—the inkjet print industry, for example—are more proactive in motivating consumers to help. And other ABI Research studies have found little motivation among handset vendors, except the two or three largest, to offer 'green' mobile device product lines."

Mobile Computing and Consumer Electronics Devices to Drive GPS Growth

Although cellular handset assets will continue to dominate shipments of devices with integrated GPS, the next growth spurt will come from mobile consumer electronics (CE) and mobile computing applications, reports In-Stat. Mobile computing and CE

devices will comprise over 100 million units in 2013.

"With growing attach rates and market maturity, GPS chipset providers must carefully evaluate which technologies to integrate into single chip solutions," says Jim McGregor, In-Stat's chief technology strategist.

Recent research by In-Stat found the following:

- Although the number of devices shipping with integrated GPS is increasing, the attach rates and the devices shipments have been hampered by the faltering economy.
- By 2012, there will be more CE devices with integrated GPS shipping than there are stand alone personal navigation devices.
- Mobile computing holds a lot of promise for GPS with 26 million GPS enabled units shipping in 2013, but there are barriers. In the netbook segment, for example, cost, integrating yet another antenna, only one mini-card slot will inhibit adoption.
- CPUs must be integrated (ARM, x86, Mips, etc.) to manage the host processor load.
- Infrastructure radios (802.11, WiMAX, LTE, etc.) are likely candidates for integration.
- The research, "GPS—'Locating' Its Way into Mobile Devices," covers the worldwide market for GPS chipsets and end products. It includes:
 - Total Available Market and GPS attach rate forecasts for mobile CE and mobile computing through 2013.
 - GPS chipset unit and revenue forecasts through 2013.
 - GPS supplier breakdowns.
 - Analysis of device OEM needs by market segment.



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■ **Harris Corp.**, an international communications and information technology company, has signed a definitive agreement to acquire the **Tyco Electronics Wireless Systems** business (formerly known as M/A-COM), an established provider of mission-critical wireless communications systems for law enforcement, fire and rescue, and public service organizations. Tyco Electronics Wireless Systems, a business segment of Tyco Electronics Ltd., was formed in 1999 and grew through the acquisition of ComNet Ericsson in 2001 to create Tyco Electronics Wireless Systems (Wireless Systems). Wireless Systems will be combined with the Harris RF Communications business segment, creating a dynamic new organization that will provide end-to-end wireless network solutions to the growing \$9 B global land mobile radio systems market. Under the definitive agreement, Harris will purchase the Wireless Systems assets of Tyco Electronics for \$675 M in cash, subject to post-closing adjustments.

■ **Microsemi Corp.**, a manufacturer of high performance analog mixed signal integrated circuits and high reliability semiconductors, and **Endwave Corp.**, a provider of high frequency RF solutions for mobile communications markets, announced that Microsemi has acquired Endwave's defense electronics and security (D&S) business. Microsemi intends to combine Endwave's high frequency product portfolio with its own, creating one of the leading high reliability RF product offerings in the market today and covering the technology spectrum up to 100 GHz. Under the terms of the agreement, Microsemi is acquiring the D&S assets for a total equity value of \$28 M in cash plus the assumption of specified liabilities. Microsemi expects the acquisition to be accretive immediately.

■ **Codan Ltd.** has announced a strategic expansion of its satellite communications business, acquiring Pennsylvania-based **Locus Microwave Inc.** Locus is a specialist microwave technology company based in State College, PA, primarily focused on the design, manufacture and supply of microwave radio products for satellite communications. Under Codan's ownership, Locus will remain a US-based business with its design, manufacturing and sales led by the company's founders and current executive team comprising Jim Dixon, Gary McGovern and Dana Wilt. The acquisition will enable Codan to establish closer contact with the North American Satellite market with the addition of Locus's product development and manufacturing base in State College.

■ **Superconductor Technologies Inc.** (STI), a provider of advanced wireless solutions, innovative adaptive filtering and world class cryogenic products for commercial and government applications, will be participating with a major wireless original equipment manufacturer (OEM)

in a long-term evolution (LTE) field trial with a tier-one US wireless operator for its new 700 MHz network. The trial is scheduled to be completed in the fourth quarter of 2009.

■ **Centellax Inc.**, a manufacturer of high performance, low cost test equipment, announced the opening of its first international sales office in Shenzhen, China, as well as the expansion of its international sales team to meet the growing demand from their customers. Centellax made the decision to open an office in China because of an increase of business opportunities in the region.

■ Asylum Research's wholly owned UK subsidiary has moved and expanded its offices. **Asylum Research UK** opened for business nearly three years ago and its successful growth has led to the need for more office space to accommodate staff and demonstration equipment, including the new Cypher™ AFM. The new office is located in Bicester, Oxfordshire.

■ **Aeroflex** announced support for new NXDN radios being developed for the land mobile radio market. As a member of the NXDN™ Forum, Aeroflex is leading the way with new test features that aid in the research and development of this exciting new radio technology.

■ **Texas Instruments Inc.** (TI) announced the company's strong endorsement of the ZigBee Alliance's recent announcement to integrate Internet Protocol (IP) and open standards. The plan to incorporate global IT standards from the Internet Engineering Task Force (IETF) will allow continued growth of smart grid applications beyond the smart meter with the proven ZigBee Smart Energy public application profile.

■ **Agilent Technologies Inc.** introduced a new option—arbitrary load impedance X-parameters—for its PNA-X Nonlinear Vector Network Analyzer. The option, when used in conjunction with **Maury Microwave** tuners and software, enables the capability to accurately measure and simulate nonlinear component behavior at all load impedances. The result is the highest level of insight into nonlinear DUT behavior, making the NVNA capability especially useful for scientists researching new RF technologies and engineers involved in designing today's high performance active devices.

■ **AWR**, an innovation leader in high frequency electronic design automation (EDA), announced that users of AWR's Microwave Office design software now have access to XML library data for a broad array of microwave amplifiers from **TriQuint Semiconductor Inc.**'s San Jose design center (formerly WJ Communications). The devices include packaged gain-blocks, field effect transistors (FET) and heterojunction bipolar transistor (HBT) amplifiers. The library provides measurement-based models and footprints used for printed circuit board (PCB) and module layouts. It is available to users

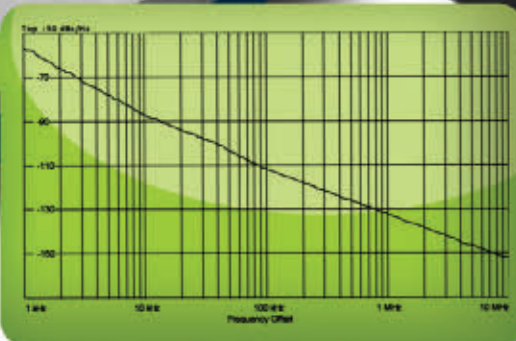
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DCO170340-5	1700 - 3400	0.5 - 24	+5 @ 24 mA	-90	
DCO200400-5	2000 - 4000	0.5 - 18	+5 @ 35 mA	-90	
DCO200400-3			+3 @ 35 mA	-89	0.3 x 0.3 x 0.1
DCO300600-5	3000 - 6000	0.5 - 18	+5 @ 35 mA	-80	
DCO300600-3			+3 @ 35 mA	-78	0.3 x 0.3 x 0.1
DCO400800-5	4000 - 8000	0.5 - 18	+5 @ 35 mA	-78	
DCO400800-3			+3 @ 35 mA	-76	0.3 x 0.3 x 0.1
DCO432493-5	4325 - 4950	0.5 - 11	+5 @ 17 mA	-88	0.3 x 0.3 x 0.1
DCO432493-3			+3 @ 17 mA	-86	
DCO473542-5	4730 - 5420	0.5 - 22	+5 @ 20 mA	-88	0.3 x 0.3 x 0.1
DCO473542-3			+3 @ 20 mA	-86	
DCO490517-5	4900 - 5175	0.5 - 5	+5 @ 22 mA	-88	0.3 x 0.3 x 0.1
DCO490517-3			+3 @ 22 mA	-86	
DCO495550-5	4950 - 5500	0.5 - 12	+5 @ 22 mA	-87	0.3 x 0.3 x 0.1
DCO495550-3			+3 @ 22 mA	-85	
DCO608634-5	6080 - 6340	0.5 - 5	+5 @ 22 mA	-86	0.3 x 0.3 x 0.1
DCO608634-3			+3 @ 22 mA	-84	
DCO615712-5	6150 - 7120	0.5 - 18	+5 @ 22 mA	-85	0.3 x 0.3 x 0.1
DCO615712-3			+3 @ 22 mA	-83	
DXO Series					
DXO810900-5	8100 - 8800	0.5 - 16	+5 @ 22 mA	-82	0.3 x 0.3 x 0.1
DXO810900-3			+3 @ 22 mA	-80	
DXO900965-5	9000 - 9650	0.5 - 16	+5 @ 22 mA	-80	0.3 x 0.3 x 0.1
DXO900965-3			+3 @ 22 mA	-78	

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of AWR's Microwave Office software through the XML library link accessible from the software.

■ **Metelics Inc.**, Sunnyvale, CA, was named the Discrete Semiconductor Commodity Supplier of the Year 2009 by Rockwell Collins. The award was presented during the company's Annual Supplier Conference. The Supplier of the Year award is an acknowledgment of significant contributions made during the year by suppliers and is based upon quality, delivery, total cost of ownership, lead time and customer service.

■ **Teledyne Storm Products'** Microwave Group recently obtained AS9100(B) certification. As an AS9100 registered company, Teledyne Storm-Microwave's quality management system meets not only ISO 9001 standards, but also the additional standards formulated by the International Aerospace Quality Group (IAQG) to specifically address specialized requirements of the aviation, space and defense industries. Teledyne Storm Products-Microwave provides high performance interconnect solutions to domestic and international defense/aerospace, telecommunications, and test & measurement markets.

■ **Electronic Assembly Manufacturing Inc. (EAM)**, an RF/microwave coaxial cable assembly supplier, has recently announced the receipt of its ISO 9001:2000 certification. The certificate of registration assures adherence to the BS EN ISO 9001:2000 standard as it applies to the manufacture of standard and custom cable assemblies, and related products for military, medical and commercial applications. The certification was granted through IMS International, which has been improving and enhancing the technical excellence of its clients since 1989.

■ In an effort to reduce the company's carbon footprint, use less energy and water, and significantly increase efficiencies, **Jazz Semiconductor Inc.**, a Tower Group company, and leading Orange County chipmaker, is conducting an ongoing efficiency overhaul. To be more energy efficient in the operation of its globally competitive 24/7 fabrication facility, the company has already instituted new technology and practices that have resulted in a savings of more than 7.5 million kilowatt hours per year, resulting in the avoidance of 5,386 tons of greenhouse gas (GHG) emissions—the equivalent of taking 986 cars off the road.

■ The 17th Annual SMT Vision Award has announced **LPKF Laser & Electronics** as the winner for innovation and excellence in products and service, within the Assembly Tools category. The ProtoLaser U is a UV laser for depaneling of flex, rigid and rigid-flex material.

■ **L-com**, a leader in the manufacture of wired and wireless connectivity solutions, announced that it is the recipient of the prestigious 2008 Boeing Performance Excellence Award (BPEA).

CONTRACTS

■ **XIO Strategies Inc.**, a supply chain management and communications consulting firm, announced that it has been awarded a subcontract by **Northrop Grumman** to provide active RFID consulting services to the US Department of Defense under their RFID III contract, a multiple award, indefinite delivery/indefinite quantity contract with a \$429 M ceiling available for task orders.

■ **Cobham plc** has received a contract modification from the US Navy to produce 51 ALQ-99 Low Band Transmitters (LBT) and provide spare parts for US\$72 M. This contract, initially valued at US\$37 M, was previously announced by the company in October 2008.

■ **Micronetics Inc.** announced that its New Jersey-based subsidiary, **Microwave Concepts** (Micro-Con), has received advanced funding of approximately \$5 M from a major defense OEM for highly integrated microwave subassemblies. These subassemblies are used as part of a complex jamming system. In addition to this advanced funding, full funding of production quantities is expected within 90 days. The anticipated period of performance on this program is approximately 24 months.

■ **Radio Waves Inc.** has announced that a North American wireless communications carrier has selected its high quality microwave antenna systems. Both Radio Waves SP standard performance and HP high performance products as well as Radio Waves newest UHP ultra high performance models will be utilized by the carrier. These microwave antennas will support the carrier's geographical expansion and network capacity enhancement. Radio Waves was selected for this expansion due to its ability to deliver high quality antennas made in the US at its Billerica, MA global headquarters more rapidly than other manufacturers.

■ **Communications & Power Industries Inc. (CPI)** has been awarded approximately \$3.1 M by **Sierra Nevada Corp.** to supply integrated microwave assemblies and transmitters for use in the US Navy's AN/APN-245 Automatic Carrier Landing System (ACLS) Beacon. CPI, a subsidiary of CPI International Inc. (CPII), is a provider of microwave, radio frequency, power and control solutions for critical defense, communications, medical, scientific and other applications.

■ **Comtech Telecommunications Corp.** announced that its New York-based subsidiary, **Comtech PST Corp.**, received a \$2 M contract for broadband, solid-state, high power RF microwave amplifier system spares from an international original equipment manufacturer (OEM). These spares are being provided in support of previously fielded communications jamming high power amplifier systems for the electronic warfare market.

■ **RF Micro Devices Inc. (RFMD)**, a leader in the design and manufacture of high performance semiconductor components, announced that the company has been selected by a smartphone manufacturer to supply its RF2815 GPS LNA module for use in a soon to be released CDMA smartphone. This new smartphone is

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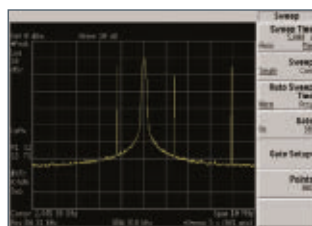
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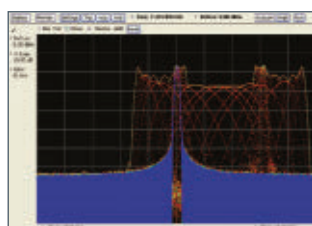
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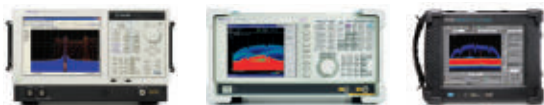
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expected to launch in the second half of calendar 2009 in North America. The feature-rich, dual-band CDMA device will be manufactured by the leading Taiwan-based smartphone manufacturer and will feature a leading open source mobile operating system.

FINANCIAL NEWS

■ **WiSpry Inc.**, a leader in programmable RF semiconductor products for the wireless industry, announced its first closing for a Series C financing of \$10 M dollars. The round was led by a new investor in the company, Paladin Capital Group, which is also gaining a seat on WiSpry's board of directors, as well as existing investors L-Capital Partners and Blue Print Ventures. A new strategic investor, MuRata Manufacturing Co. Ltd., and additional existing investors American River Ventures, In-Q-Tel, Tech Coast Angels and Shepherd Ventures also participated. A second close of the Series C, anticipated to be at least \$5 M, is expected to be completed this summer.

PERSONNEL

■ Park Electrochemical Corp. announced the appointment of **Marty Kendrick** as Vice President of Operations. In this new position, Kendrick will be responsible for the Park's operations in Asia, Europe and North America with the exception of the company's advanced composite materials operation located in Waterbury, CT. Most recently, Kendrick was Vice President of North American Operations of Park with responsibility for Park's Neltec Inc., Nelco Products Inc., Park Aircraft Technologies Corp. and Park Aerospace Structures Corp. subsidiaries. The company also announced the appointment of **Tom Pursch** as the President of the company's aircraft composite parts subsidiary in Lynnwood, WA and the company's aircraft composite materials and technologies subsidiary. Since joining the company in October of 2008, Pursch was President of Park's Nelco Products Inc. electronics materials subsidiary located in Fullerton, CA.

■ Peregrine Semiconductor Corp., a supplier of high performance RF CMOS and mixed-signal



▲ Jay Biskupski

communications ICs, announced that it has appointed **Jay Biskupski** to the role of chief financial officer, responsible for the company's financial and site services organizations. Prior to joining Peregrine, Biskupski served as chief financial officer of publicly traded Xantrex Technology Inc.

■ Emerson & Cuming Microwave Products Inc. announced the appointment of **Devin Sullivan** as RFID Program Manager. This addition comes as a prelude to the launch of MetalTag™ Impact, a ruggedized addition to the MetalTag product line. In response to the growing RFID industry, and the need for Read-On-Metal and Liquid solutions, the company is expanding its presence

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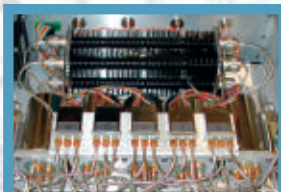
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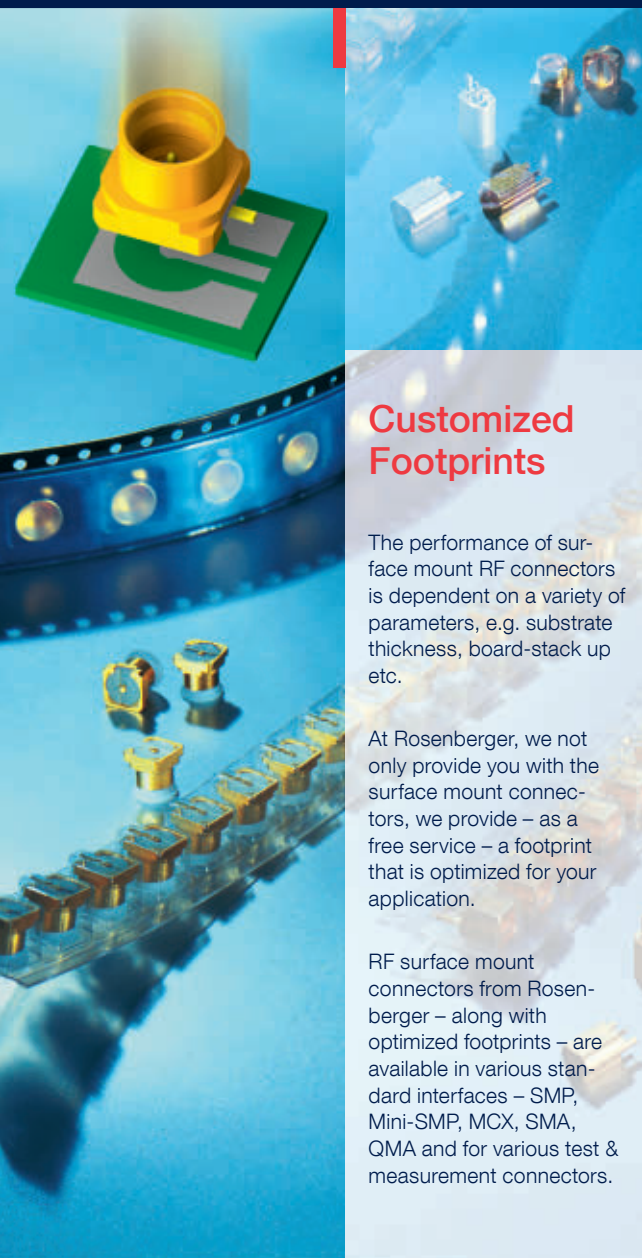
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by adding a dedicated individual to focus on the need for its Read-On-Metal, RFID transponder product line. Sullivan will be responsible for sales of products into the RFID sales channel. His responsibilities will include identifying trade partners, setting market pricing and making recommendations for product promotion, and related marketing support.

■ MI Technologies announced the appointment of **Jan Kendall** as Director, Product Marketing, and **Bill Hawkins**, Strategic Account Manager.



▲ Jan Kendall



▲ Bill Hawkins

In the new position of Director, Product Marketing, Kendall is responsible for ensuring the company's product management and customer support

efforts align with overall strategies and market trends by providing focused product marketing and marketing communications management. Hawkins comes to MI Technologies with more than 17 years sales experience. Prior to joining the company, Hawkins served as a Field Sales Engineer for Agilent Technologies where he coordinated all facets of sales of multimillion-dollar testing solutions to the semiconductor industry.

REP APPOINTMENTS

■ **Reactel Inc.**, a manufacturer of RF and microwave filters, multiplexers, switched filter banks and sub-assemblies to the commercial, military, industrial and medical industries, announced the appointment of WES-K as the company's representative in Southern California. For more information about WES-K, visit www.wes-k.com or telephone Randy Salmont at (661) 714-5414.

■ **International Manufacturing Services Inc. (IMS)**, a manufacturer and supplier of high quality thick film resistors, terminations, attenuators, thermal management products, planar dividers and planar filters to the electronics industry, announced the appointment of Joe Ruvolo of **K&R Engineering** as its Northern New Jersey sales representative. Ruvolo has more than twenty years' experience in the electronics industry working in purchasing and sales. He worked for ITT for seven years before joining K&R Engineering of Succasunna, NJ. He has been with K&R Engineering since 1995, covering Northern New Jersey. Contact Joe Ruvolo, K&R Engineering, 275 Route 10 East, Suite 220-285, Succasunna, NJ 07876; e-mail: joe@kreng.com; ph: (973) 584-5235.

■ **Precision Connector Inc.**, a manufacturer of precision coaxial connectors, has appointed **RF Connections LLC** as Sales Representative in the Southeast United States. RF Connections will cover the states of Florida, Georgia, North Carolina, South Carolina, Tennessee, Mississippi and Alabama.



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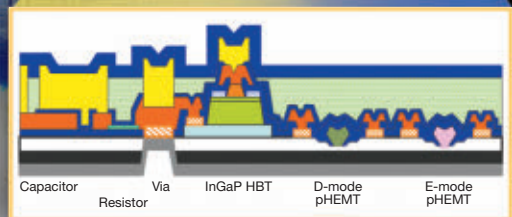
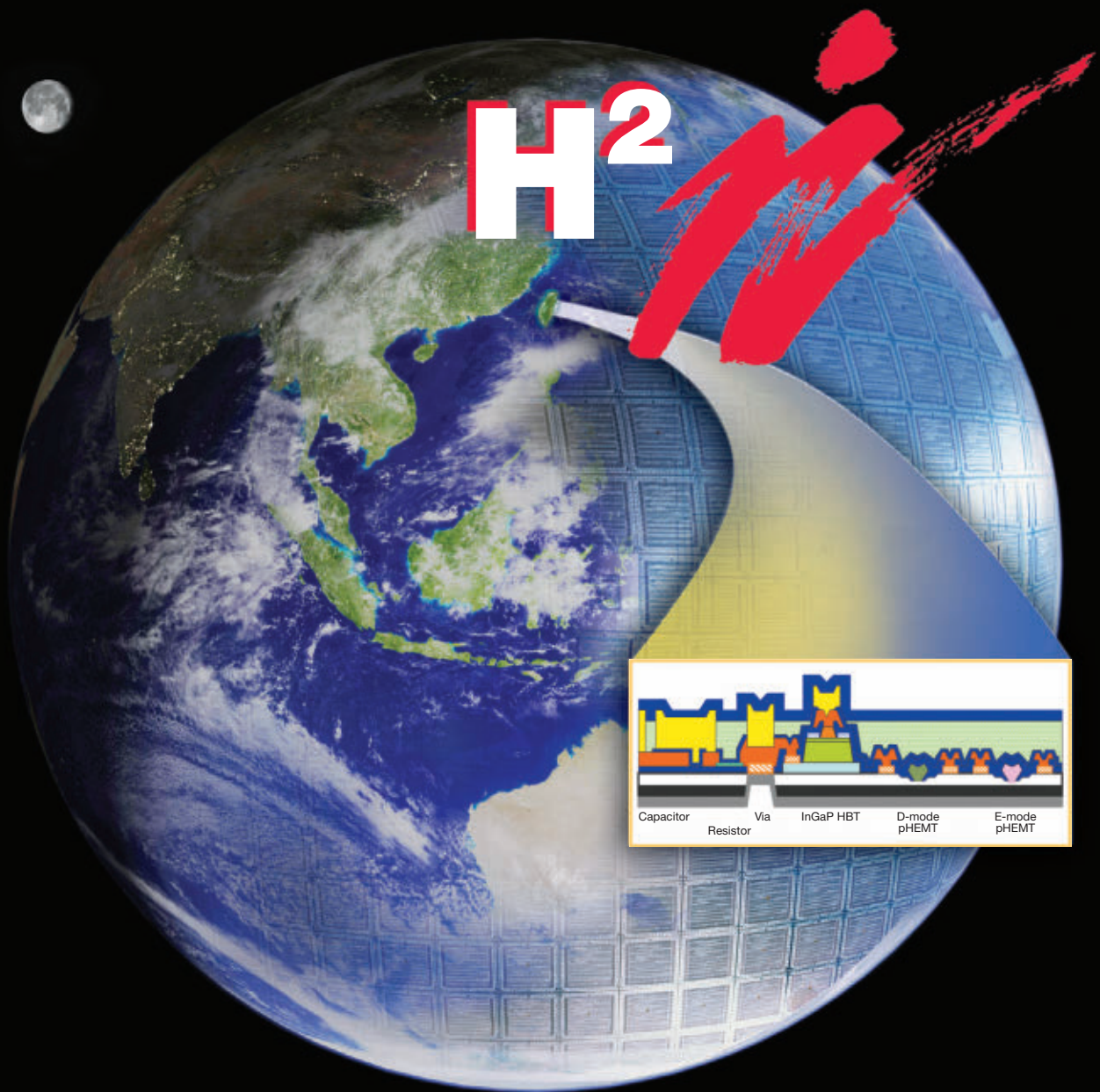
This article describes a handy design method for a long backfire antenna, called for short a backfire antenna (BFA). It consists of the following basic elements: A feed F (dipole or assembly of crossed dipoles), a surface wave (SW) structure S (dipole array, metal disk-on-rod, dielectric rod, dielectric-covered metal rod or endfire dipole array), and two parallel disk reflectors: A small or feed R_1 and a big or surface-wave reflector R_2 . The SW structure in use is a metal disk-on-rod (cigar) construction, although the same design method can be applied to backfire antennas with other types of SW rods. The presented design scheme is based on simple empirical equations, graphs and tables, and is validated by measurements of BFA prototypes with disk-on-rod structures, two to four wavelengths long, though by a simple extrapolation the scheme can be extended to antennas up to six wavelengths long. The gain range from 17 to 25 dB is covered by 2 to 5λ backfire antennas operating at the lower microwave WLAN, ISM, GPS and other bands between 1.5 and 3.5 GHz.

As a specific case, a 4λ backfire disk-on-rod antenna for the WLAN/ISM frequency band 2.4 to 2.5 GHz was designed, built and studied experimentally. To obtain a maximum gain of approximately 24 dBi, the big antenna reflector was made with a plane-conical profile. This

BFA was contrasted to a commercial parabolic antenna of similar gain and dimensions, and it was found that for the chosen frequency band and required gain the well optimized BFA is a more compact and effective radiator.

The backfire antenna (BFA) was created by H.W. Ehrenspeck and his associates at the Air Force Cambridge Research Center, Bedford, MA, in 1959.^{1,5} Because of its compact and robust construction and very good radiation performance, this antenna has been used in various wireless systems, mostly military, earth and spacecraft. A BFA comprises an axial surface wave (SW) structure typically 2 to 4 wavelengths long. If the BFA is equal or shorter than one wavelength, the SW structure becomes unnecessary and the antenna is converted into a short backfire antenna (SBFA). The SBFA is very popular today, mainly in satellite communications and WLAN links. It has a medium directivity and gain of approximately 12 to 16 dB. For long-range point-to-point applications, say WLAN, WISP and satellite links, a bigger

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	Ft	30 GHz
	Fmax	110 GHz
	BVceo	19 V
	Gm_Peak	500 mS/mm
e-pHEMT	Idss	0.01 uA/mm
	BVdg	21 V
	Vth	0.35 V
	Fmin	0.44 dB
	Ft	30 GHz
d-pHEMT	Fmax	90 GHz
	Gm_Peak	330 mS/mm
	Idss	230 mA/mm
	BVdg	20 V
	Vp	-1.0 V
	Ron	2.0 Ohm-mm
	Fmin	0.31 dB
	Ft	30 GHz
	Fmax	70 GHz

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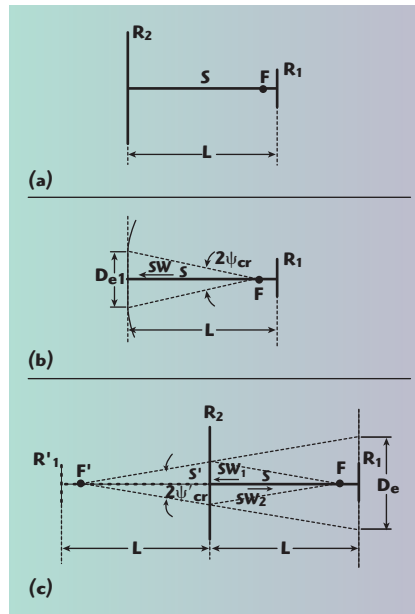
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gain from 17 to 25 dB is desired, and the BFA along with the parabolic dish antenna (PDA) and antenna dipole arrays proved to be very good choices. For comparison, a 4λ long S-band BFA, with a Yagi-type SW structure, is almost comparable in gain to an array of 16 (4×4) Yagi antennas, each of them comprised of nine elements.⁶ Both antennas, the BFA and the Yagi array, have a gain of approximately 23.5 dB, but while the BFA has sidelobe levels more than 20 dB below the main lobe, the Yagi array sidelobes are much higher (-11 dB). Furthermore, the BFA is more compact, has a simpler feed system and reduced complexity.

The BFA geometry is illustrated in **Figure 1**. It consists of the following basic elements: A feed F (dipole or assembly of crossed dipoles), SW rod S (dipole array, metal disk-on-rod, dielectric rod, dielectric-covered metal rod or endfire dipole array), and two parallel disk reflectors: A small or feed reflector R_1 and a big or surface-wave reflector R_2 . In the figure, the antenna length L is the distance between R_1 and R_2 .

The dipole feed location between the two reflectors is of great importance for the BFA radiation and input characteristics. The antenna works normally only for two feed locations: Superior, if the feed F is near the small reflector R_1 , and inferior, if F is near the big reflector R_2 . In both cases, the distance between the feed and respective reflector is $\lambda/4$. Other feed location points along the SW structure are not recommended. In this article, only a BFA with superior feed location has been considered, since it has approximately 3 to 4 dB higher gain, compared to the BFA with inferior feed location.^{6,7}

The simplified radiation mechanism of a BFA has been described in early references¹⁻⁵ and can be summarized as follows. A larger amount of the spherical wave radiated from F is transformed by S into a traveling wave, aimed at the big reflector R_2 . The feed or launching efficiency is measured as the ratio between the power carried by the surface wave and the total radiated power. Thus, the feed efficiency is considered big if the power coupled to the spherical wave is small compared to power tied to



▲ **Fig. 1** Simplified operation of the back-fire antenna: (a) geometry, (b) end-fire antenna model and (c) image model.

the surface wave. If R_2 is not present, the assembly R_1 -F-S acts as an endfire antenna (EFA) with an effective aperture of diameter D_{e1} radiating in the axial direction. The big reflector R_2 turns back the surface wave towards the BFA virtual aperture, where it is partially reflected by the small reflector R_1 . Thus, according to this simple image approach, R_2 forces the surface wave to traverse the physical antenna length L at least twice. As a result, the BFA operates as an EFA of effective length equal to double the physical length, or $L_e = 2L$. Consistent with the Hansen-Woodyard (HW) condition,^{5,8} the maximum gain of the EFA is proportional to the length of its surface wave structure, provided that the SW phase velocity v is adjusted to its optimum value corresponding to the effective length L_e . This implies that the BFA design may have an effective radiation aperture of diameter D_e much larger than the corresponding endfire aperture D_{e1} . The BFA with an optimum SW phase velocity v ($L_e = 2L$) should yield as a minimum four times (6 dB) higher gain than the EFA having an optimum SW phase velocity $v(L)$.

More rigorous theoretical and further experimental studies of the BFA^{6,8} have revealed that the successive SW reflections (and diffractions) by the small and big reflectors produce more complicated standing-wave field modes between them. The best BFA

gain performance is obtained if the antenna physical length is approximately equal to a multiple of the free-space half wavelength. Our experiments with backfire antennas have shown that L_e equal to $6L$ is a better choice in finding the optimum surface wave velocity. Such approximation of the inner standing wave process corresponds to six forward and backward travels along the surface wave structure or to a triple wave reflection from the big reflector.

RELATIONS BETWEEN SURFACE-WAVE PHASE VELOCITY AND ANTENNA LENGTH

Based on the experimental and computer phase visualization of the EFA, it is assumed^{2,6,8} that at its end plane, in the limits of so-called critical angle Ψ_c (or if $\Psi \leq \Psi_c$), the SW has a quasi-plane phase front and effective radiation aperture of diameter D_{e1} . Otherwise, if $\Psi > \Psi_c$, the phase surface wave front looks like a spherical one. This deviation from the plane SW is due to the primary feed field radiated directly as a free-space spherical wave. The critical angle depends on the SW phase velocity v and is approximately found by^{2,4}

$$\tan \Psi_{cr} = \sqrt{\xi_s^2 (L/\lambda) - 1} \quad (1)$$

where

$$\xi_s(L/\lambda) = \frac{c}{v(L/\lambda)} = 1 + 0.23 \frac{\lambda}{L} \quad (2)$$

Here, $v(L/\lambda)$ is the SW velocity delay factor as a function of the length expressed in wavelengths. Equation 2 is derived from the simplified single-image model of BFA and the Hansen-Woodyard optimum phase condition for a surface wave rod with an effective length $L_e = 2L$; c is the free-space wave velocity.^{2,5} The ideal image model is introduced² for the case of a big reflector of infinite dimension. The multiple reflection and diffraction effects on both reflectors and the feed dipole should also be taken into account. The studies have shown⁶⁻⁸ that the simple image model and Equation 2 are not suitable for making a correct BFA design, and thus, a bigger L_e should be chosen.

Here, an effective BFA length that is equal to six physical lengths is supposed, that is $L_e = 6L$. This assump-



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Ft	70 GHz
IDSS	480 mA/mm
Idmax	630 mA/mm
Gm (peak)	540 mS/mm
Vb	14 V
Pinchoff Voltage	-1.15 V
P1dB*	600 mW/mm
Ron	1 Ohm-mm
Epi Resistor	135 ohm/sq
Thin Film Resistor	50 ohm/sq
MIM Capacitor	600 pF/mm ²

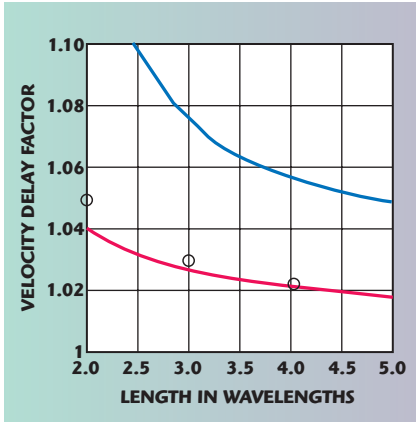
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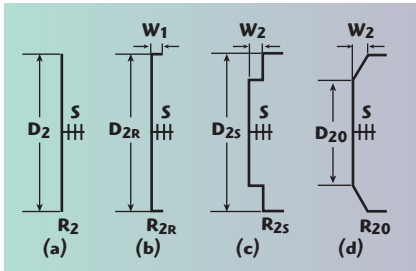
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▲ Fig. 2 Phase velocity factor vs. length for different number of reflections from the big reflector.



▲ Fig. 3 Big reflector profiles.

tion corresponds to six wave travels along the physical antenna length or three reflections from the big reflector. For $L_e = 6L$, Equation 2 is modified to

$$\xi_s(L/\lambda) = 1 + 0.08 \frac{\lambda}{L} \quad (3)$$

Figure 2 illustrates the change of velocity delay factor ξ_s as a function of the BFA antenna physical length L in wavelengths, calculated for an effective length L_e equal to $2L$ (blue line or Equation 2) and $6L$ (red line or Equation 3). Three measured values^{3,7} of the SW velocity delay factor versus the physical antenna length expressed in wavelengths, or $\Psi_s(L/\lambda)$, for an optimally designed disk-on-rod BFA SW rod: $\Psi_s = 1.05, 1.03$ and 1.02 for $L/\lambda = 2, 3$ and 4 , are shown with circles. These points agree well with Equation 3 and the corresponding red line.

As mentioned in the previous section, the BFA can be considered as a parallel-plane resonator antenna with a standing surface wave field excited inside. In the antenna aperture that is partially closed by the small reflector R_1 two basic wave phenomena take place: Multiple partial reflections

from R_1 and multiple intensive radiations from the open aperture area. The length of such radiating cavity can be expressed as

$$L = n \frac{\lambda_s}{2} + \Delta L, \text{ for } n = 1, 2, 3, \dots, \quad (4)$$

where $\lambda_s = v/f$ is the surface-wave wavelength, ΔL is the length correction due to the radiation, n is a real integer called standing-wave number and f is the design (resonance) frequency.

On the other hand, the BFA studies have shown that its length L takes discrete resonance values, equal to n free-space half wavelengths, or

$$L = n \frac{\lambda}{2} \quad (5)$$

where n has the same integral values as in Equation 4.

In practice, the standing-wave number n usually takes values from 4 to 8 to which correspond the next five values of $L/\lambda = 2, 2.5, 3, 3.5$ and 4 . For $n = 1$, the BFA is just a half-wavelength long and becomes a short backfire antenna or SBFA. In this case, the SW structure is missing.

The length correction ΔL in Equation 4 is found by the equality of Equations 4 and 5, or

$$\Delta L = n \frac{\lambda}{2} \left(1 - \frac{1}{\xi_s(L/\lambda)} \right) \quad (6)$$

From Equations 3 and 5, the backfire antenna Equation 6 becomes

$$\Delta L = L \left[1 - \frac{1}{1 + 0.08 \frac{L}{\lambda}} \right] \quad (7)$$

ΔL is small compared to the BFA length L . For instance, if L/λ varies from 2 to 4, the ratio ΔL ranges from 0.038 to 0.02.

BIG REFLECTOR PROFILES

Four different profiles of the big reflector are shown in **Figure 3**: (a) disk reflector R_2 of diameter D_2 , (b) rimmed disk reflector R_{2R} of diameter D_{2R} , (c) rimmed stepped-corrected disk reflector R_{2S} of diameter D_{2S} and (d) rimmed conically-corrected disk reflector R_{2C} of diameter D_{2C} .⁷ The effective diameter D_{e1} of the EFA effective aperture area depends on the

antenna length L and the critical angle Ψ_{cr} or

$$D_{e1} = 2L \tan \Psi_{cr} \quad (8)$$

which, having in mind Equation 4, can be approximately given as a function of L/λ as

$$D_{e1} = 1.4 \lambda \sqrt{\frac{L}{\lambda}} \quad (9)$$

In the image model, the big reflector of BFA lays in the EFA effective aperture plane and its minimum diameter D_2 is equal to the constant-phase effective aperture, or $D_2 = D_{e1}$.

With the increase of the disk diameter, so that $\Psi > \Psi_{cr}$, the phase front becomes spherical and a quadratic phase distortion on the reflector plane occurs. If the tolerable phase distortion at the disk edge is $\pi/2$, the disk diameter D_2 set equal to D_e will be bigger than D_{e1} , and can be found roughly as²

$$D_2 = 2 \lambda \sqrt{\frac{L}{\lambda}} \quad (10)$$

The disk reflector R_{2R} with a quarter-wavelength rim ($w_1 = 0.25 \lambda$) has a diameter D_{2R} equal to that of reflector R_2 , that is $D_{2R} = D_2$. The rim reduces the sidelobe and backlobe levels, and results in an antenna gain increase.

The step-phase correction in reflector R_{2S} and the conical-phase correction in reflector R_{2C} allow further enlargement of reflector diameter and antenna gain. These two reflectors are normally used for antenna lengths equal or greater than 3λ . The inner or disk area diameter D_{20} , and the outer (peripheral) diameters D_{2S} and D_{2C} of the two reflectors R_{2S} and R_{2C} , respectively, are given by^{2,6}

$$D_{20} = (1.9 \div 2.0) \lambda \sqrt{L/\lambda} \quad (11)$$

$$D_{2C} = D_{2S} = (2.9 \div 3) \lambda \sqrt{L/\lambda} \quad (12)$$

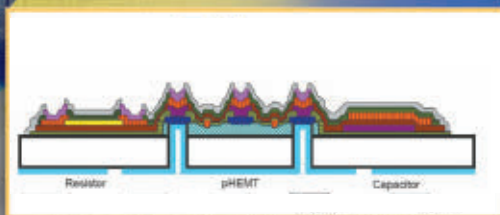
The step width w_2 and rim width w_1 are also chosen equal for both reflectors, or

$$w_1 = w_2 = 0.25 \lambda \quad (13)$$

Though the BFA with large reflectors R_{2S} and R_{2C} are equal in diameter, the phase-correction in the latter is slightly better and the antenna gain is a bit higher.² Naturally, the compound plane-parabolic reflector will

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have the best phase correction, but this would require more complex fabrication technology.

Note: The equations and experimental results for the antenna parameters presented next are applicable for backfire antennas having either type of big reflectors: R_{2R} or R_{2C} . The study concentrated on them only, because the BFA antenna with reflector R_{2R} is of simpler construction and has fairly low side and back lobes, while the BFA antenna with reflector R_{2C} produces higher gain, compared to the other antenna's reflectors.

SMALL REFLECTORS

The small reflector R_1 in all BFA antennas is usually a simple thin disk with a diameter D_1 . It has a great importance on the SW launch process and aperture field distribution. For very small values of D_1 , the BFA essentially radiates as an EFA. For a constant big reflector diameter and antenna length, the small reflector has an optimum diameter for which the BFA antenna reaches a maximum gain. If D_1 is bigger than its optimum size, the antenna gain reduces, and for values of D_1 close to the big reflector diameter, the antenna practically does not radiate as it is transformed into a very high quality-factor resonator. The experimental study has proved that, for all types of big reflector, the BFA small reflector optimum diameter can be found by⁷

$$D_1 = (0.25 \div 0.45) \lambda \sqrt{L / \lambda} \quad (14)$$

With the BFA length increasing, both the big and the small reflectors grow in diameter according to the quadratic relations in Equations 10 to 12 and 14. The minimum and maximum values in Equations 11, 12 and 14 define the optimum ranges of diameters D_{20} , D_{2S} (or D_{2C}) and D_1 in different practical BFA designs. They have been validated for BFA lengths from 2λ to 4λ .^{1-4,6,7}

DIRECTIVE GAIN AND BEAM WIDTH

In what follows, the empirically obtained equations for the directive gain G of EFA and BFA as a function of L/λ (the directive gain or directivity will be simply called the gain) are listed.

Gain of EFA

This antenna should be designed according to the original HW phase condition, where $L_e = L$ and the SW velocity $v(L/\lambda)$ satisfies the equation $\xi_s(L/\lambda) = 1 + 0.46 \lambda/L$. Under this condition, the gain of a very long homogeneous EFA is proportional to L/λ , or^{5,8}

$$G = 10 \log(7L / \lambda), \text{ dB} \quad (15)$$

If the design is based on the HW phase condition and the SW rod is tapered accordingly, the gain of the EFA for L between 3 and 8λ is^{5,8}

$$G = 10 \log(10L / \lambda), \text{ dB} \quad (16)$$

Gain of BFA

The BFA gain is much higher than the gain of EFA and can be found by the basic aperture antenna equation^{8,9}

$$G = (4\pi / \lambda^2) A_e \eta_e \quad (17)$$

where $A_e = \pi(D_e/2)^2$ is the effective aperture area, expressed by the effective aperture diameter D_e . In decibel form, Equation 17 is given by

$$G = 20 \log(\pi D_e / \lambda) + 10 \log \eta_e, \text{ dB} \quad (18)$$

In Equation 18, $D_e = D_{2R}$ for the rimmed disk reflector is calculated with Equation 10, and for a rimmed disk-conical reflector $D_e = D_{2C}$, by Equation 11; η_e is the radiation efficiency, which takes into account the field amplitude distribution in the BFA effective aperture.

Independently of the partial blockage by R_1 , the BFA has a relatively constant field distribution outside the blocked aperture area, which makes the aperture radiation efficiency too big. In accordance with the gain measurements, η_e may be set as $\eta_e = 0.6$ to 0.8.

The average antenna beamwidth may be defined as $B = \sqrt{B_E B_H}$, in degrees, where B_E and B_H are the E- and H-plane -3 dB beamwidths. If the BFA has a phase-corrected big reflector R_{2C} its average beamwidth can be found approximately by⁶

$$B = 22 \sqrt{\lambda / L}, \text{ deg} \quad (19)$$

Knowing B , the BFA gain can be computed by the following empiric equation, valid for a moderately high gain aperture antenna^{8,9}

$$G = 10 \log(33000 / B^2), \text{ dB} \quad (20)$$

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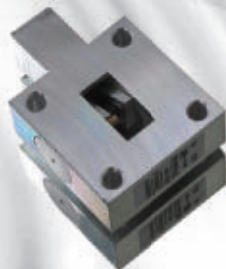
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Equation 19 is not valid for the BFA with a rimmed disk reflector R_{2R} , which for the same SW rod length has a much smaller effective aperture. Equation 19 was corrected as follows to match better the realistic beam-width and gain values in the case of a BFA having a reflector R_{2R}

$$B = 33\sqrt{\lambda} / L, \text{ deg} \quad (21)$$

Table 1 illustrates the gain property of BFA depending of the large reflector size and shape, and SW rod length. The gain values have been estimated by use of Equations 18 or 20 in the case of reflector R_{2C} or by Equations 18 or 21 and 20 for a BFA with reflector R_{2R} . From this table, it is evident that for all BFA lengths, the use of the plane-conical reflector R_{2C} leads to an approximately 3.5 dB higher gain, compared to a BFA with a plane reflector R_{2R} . On the other hand, if a gain of approximately 20 to 21 dB or less is needed, the more compact and simpler BFA having a reflector R_{2R} is to be preferred. For instance, the 2λ -long BFA with reflector R_{2C} has approximately the same gain as the 4λ -long BFA with a reflector R_{2R} , but the former is of more complex construction and occupies 1.5 times as much volume. The studies have shown that the more complex BFA with a phase-correcting reflector R_{2C} (or R_{2S}) should be considered only when gain values equal or greater than 22 to 24 dB are required.

DISK-ON-ROD (CIGAR) SURFACE-WAVE STRUCTURE

Feed Location and Design

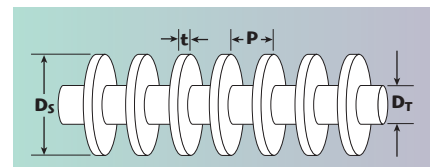
The phase velocity delay factor ξ_s (L/λ) of the SW rod is found from Equation 3 or Figure 2 (red line). For a given ξ_s (L/λ), the basic dimensions of the disk-on-rod (or

in fact disk-on-tube) structure (see **Figure 4**) are: DS or the outer diameter of the SW structure rings, DT or the inner rings' diameter (outer tube diameter), and P, the disk array period (inter-disk distance). They can be found by use of the known disk-on-metal rod design procedure.⁹⁻¹²

The metal disk-on-rod SW structure, known also as disk-on-rod SW waveguide, usually consists of rings welded on a tube T, which serves also as an outer (shield) conductor of the feed rigid coaxial line. In a heavy-duty BFA, the disk-on-tube assembly can be replaced by a single-piece corrugated rod (tube).

Next, the design procedure of disk-on-rod surface wave structure is summarized. For a given antenna length L and design wavelength λ , the phase delay factor ξ_s was calculated from Equation 3. In **Table 2** are some typical BFA values of ξ_s corresponding to different pairs of disk-on-rod dimensions $\Delta D = D_s - D_T$ and P. The table was prepared on the basis of two classical references on the subject.^{10,11} The thickness t of the disks (rings) is usually taken according to $0.01\lambda \leq t \leq 0.02\lambda$.

One of the possible ways of BFA



▲ Fig. 4 Sketch of the surface-wave disk-on-rod structure.

TABLE I

ESTIMATED GAIN OF A BFA WITH REFLECTOR R_{2R} OR R_{2C} FOR THREE ANTENNA LENGTHS

BF antenna length in wavelengths	2λ	3λ	4λ
Diameter of reflector R_{2R} , (m)	0.35	0.42	0.49
Diameter of reflector R_{2C} , (m)	0.52	0.64	0.73
Gain for reflector R_{2R} , (dB), eqs. (18) or (21)/(20)	17.7/17.8	19.5/19.6	20.7/20.8
Gain for reflector R_{2C} , (dB), eqs. (18)/(20)	21.2/21.3	23.0/23.1	24.2/24.4

TABLE II

COMBINATIONS OF $\Delta D/\lambda$ AND P/λ THAT MATCH SPECIFIC VALUES OF ξ_s

$\Delta D/\lambda$	0.200		0.225		0.250		0.275	
P/λ	0.125	0.250	0.125	0.250	0.125	0.250	0.125	0.250
ξ_s	1.02	1.01	1.02	1.01	1.03	1.01	1.05	1.02

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TABLE III

BACKFIRE AND PARABOLIC DISH ANTENNAS: COMPARATIVE DATA

Antenna Data	BFA (prototype)	PDA (commercial)
Design frequency f , GHz, wavelength λ , (m)	2.45/0.12245	2.45/0.12245
Design gain G , (dB)	24	24
Length L in wavelengths/in meters	4.0/0.49, eq. (5)	3.6/0.44
SW velocity delay factor $\xi_s(L/\lambda)$	1.02, eq. (3)	No
Diameter D_{20} , (m)	0.6, eq. (11)	No
Aperture diameter, m (D_{2C} in case of BFA)	0.73, eq. (12)	0.89
Diameter D_1 , (m)	0.11, eq. (14)	No
Step and rim widths $w_1 = w_2$, (m)	0.31, eq. (13)	No
Antenna cylindrical volume V_a , (m ³)	0.21	0.28
Outer tube diameter D_T (selected), (m)	0.012	No
Period P (selected), (m)	0.015	No
Diameter difference Δ_D , (m), by Table II	0.024	No
Outer ring diameter $D_S = \Delta_D + D_T$, (m)	0.036	No
Estimated gain, (dBi)	24.3, eq. (18)	—
Measured gain, (dBi)	23.8	24
Average beamwidth, (deg)	10.2	10
Max. E-plane sidelobe, (dB)	-22	-23
Max. H-plane sidelobe, (dB)	-26	—
Backlobe level, (dB)	-30	—
Linear polarization	V/H	V/H
Aperture efficiency	0.75	0.55
Maximum VSWR in 2.4 to 2.5 GHz band	1.5:1	1.5:1
Minimum Gain, dBi in 2.4 to 2.5 GHz band	23	23.5

feeding is by means of a dipole backed by a small reflector. All the results presented in this article have been obtained with BFA prototypes having the following feed configuration. An input coaxial-type connector is bonded at one side of a rigid feed coaxial line and fixed to the big reflector rear. The inner cylindrical conductor of the coaxial line is set along the antenna axis and is air-spaced from the outer tube conductor. On the opposite side, the feed coaxial line is short-circuited at the small reflector plane and the dipole feed F is connected to the coaxial line by means of a half-wave slot balun, known as a split coaxial line-dipole balun. This feed construction is a classical topic and can be found in many references.^{8,9}

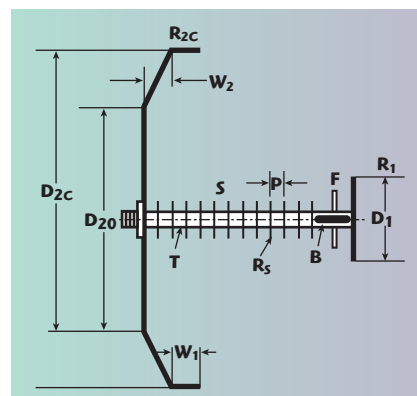


Fig. 5 Sketch of the BFA prototype constructed.

PRACTICAL BFA DESIGN AND STUDY

Based on the equations listed in this article, several backfire antennas with metal disk-on-tube SW struc-

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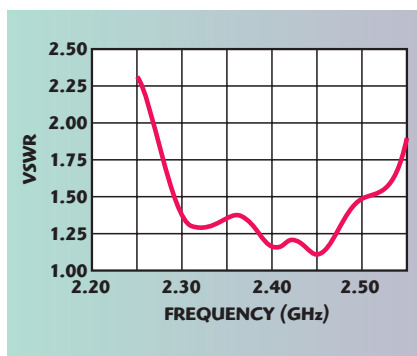
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▲ Fig. 6 Photograph of the BFA prototype.

tures of different resonant lengths ($L = 2\lambda$, 3λ and 4λ), tuned at the design frequency $f = 2.5$ GHz and working over the frequency band of 2.4 to 2.5 GHz, were built and examined experimentally. As an example, the BFA prototype that produced the largest gain is described. This is a 4λ -long backfire antenna with a big plane-conical reflector R_{2C} . The sketch of this antenna is shown in **Figure 5** and a picture of the prototype is shown in **Figure 6**.



▲ Fig. 7 Measured VSWR as a function of frequency.

Figure 7 illustrates the input match bandwidth of the experimental BFA antenna. Its dimensions, design and measured parameters are listed in **Table 3**. The equations used for obtaining the BFA table data are quoted in round brackets.

At the design frequency of 2.45 GHz, the VSWR curve has a bare minimum of about 1.1. The input frequency bandwidth is 11 or 8.5 percent at a VSWR level of 2.0 or 1.5, respectively. This band is more than double the whole WiFi/ISM spectrum that ranges from 2.4 to 2.5 GHz. For

comparison, the basic antenna data of a commercial WLAN parabolic dish antenna (PDA), operating in the same frequency band and having similar gain and radiation patterns,¹³ is also listed. Compared to the BFA, the PDA is not as compact and has a 35 percent less radiation efficiency. Obviously, the PDA is not acting in a typical quasi-optical manner, because its dimensions are relatively small compared to the design wavelength. ■

ACKNOWLEDGMENT

H.D. Hristov and R. Feick wish to acknowledge the financial support under the Chilean Conicyt Bicentenario Project ATC-11/2004.

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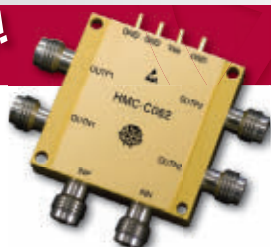
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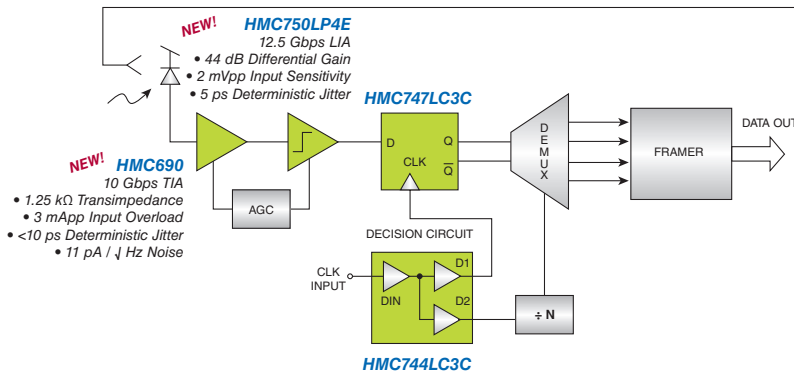
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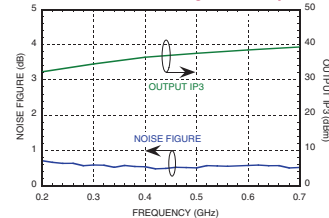
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NEW!	1.7 - 2.2	High IP3, DBL-BAL, 0 LO	DC - 0.5	-8	28	38	LP4	HMC785LP4E
	2.2 - 2.7	High IP3, DBL-BAL, 0 LO	DC - 0.45	-7.5	25	31	LP4	HMC688LP4E
	2.2 - 2.7	High IP3, DBL-BAL, 0 LO	DC - 0.45	-7.5	26	31	LP4	HMC689LP4E
	3.3 - 3.9	High IP3, DBL-BAL, 0 LO	DC - 0.6	-8.5	28	30	LP4	HMC666LP4E

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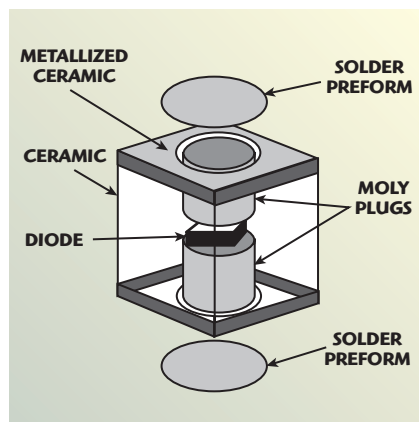
In today's global wireless industry, demands for semiconductor performance are becoming increasingly more challenging. Higher power and higher operating frequencies are two themes that permeate throughout this market space. Applications such as Magnetic Resonance Imaging (MRI) and UHF/VHF Tactical Radios require extremely high power handling PIN diodes at lower frequencies. Alternatively, broadband and high frequency applications such as Test Instrumentation, RADAR and Sensors require PIN diodes to push frequency ranges beyond 70 GHz.

PIN diodes typically come in several semiconductor flavors—Silicon, GaAs and AlGaAs. Not only does the semiconductor process play a significant role in the performance of PINs, but also the packaging medium. Many suppliers have subsequently developed unique process and packaging technologies designed to address the various frequency, power and mounting needs of customers. Three PIN diode products that have pioneered the diode industry are Silicon Metal Electrode Leadless Face (MELF) packaged PINs for high power applications, pack-

ageless PINs for broadband surface-mount applications, and flip chip AlGaAs PINs for ultra-high frequency applications. In this paper, the processes and packages of these devices will be explored, compared and contrasted.

MELF PIN DIODES

MELF package PIN diodes were designed with the intention of operating in high power, low frequency environments. The rugged MELF design hermetically encloses the PIN diode in ceramic, as shown in **Figure 1**. The diode is sandwiched between two Molybdenum plugs from the top and bottom. With a thermal conductivity at 20°C of 142 W/mK, these Moly plugs provide an optimal thermal contact with the diode die to facilitate heat conduction. A solder preform is then added on the external side of the plug. The combination of this RoHS solder preform and the metallized ceramic on the top and bottom of the package allows for these devices to be surface mounted using Sn63/Pb37 solder or some other RoHS compliant solders. The tin plated, rectangular construction was done intentionally to enhance



▲ Fig. 1 MELF package construction.

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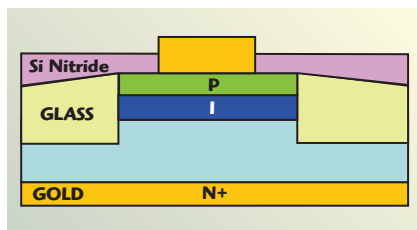
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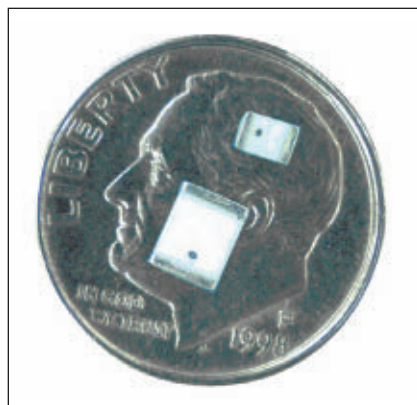
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▲ Fig. 2 Silicon PIN diode construction.

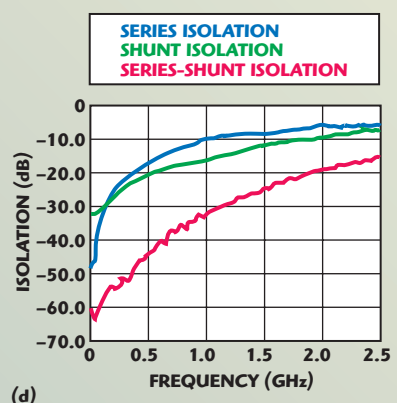
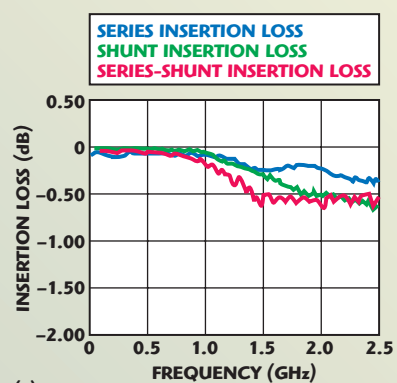
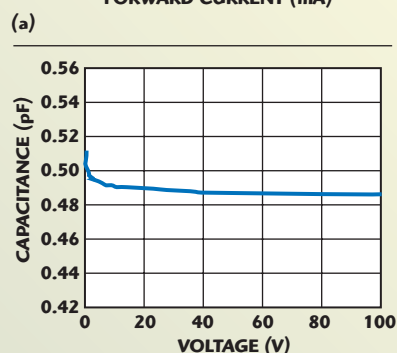
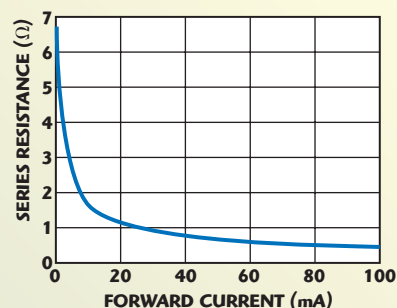


▲ Fig. 3 MELF package styles.

solderability and aid in high volume, pick and place environments.

The construction of the MELF PIN is critical to an RF designer due to the efficient heat dissipation and consequent power handling up to 200 W. In addition, PIN diodes with different I-region thicknesses ranging from 30 to 350 micron can be mounted into this package style. Thicker I-regions handle higher RF voltages and provide higher linearity (IIP3) due to the increased breakdown voltage (V_b). In contrast, thinner I-regions will have faster switching/settling speeds as well as lower series resistance (R_s). **Figure 2** shows the construction of the PIN diode. These MELF PINs work well down to 300 kHz and up to about 2 GHz before package parasitics impact their RF performance.

MELF PIN diodes have two package styles, as shown in **Figure 3**. The first is the smallest MELF with a parasitic capacitance of 0.16 pF and a parasitic inductance of 0.15 nH per Moly plug. **Figure 4** shows the DC and RF performance of a typical MELF PIN with the DC parameters measured by an impedance analyzer on a single diode, and the S-parameter performance measured on a vector network analyzer. The series resistance, capacitance, insertion loss and isolation are shown for a MELF PIN soldered



▲ Fig. 4 DC and RF performance of a MELF PIN diode.

down onto a Rogers 4350 microstrip line in series. Insertion loss and isolation are also shown for a shunt MELF PIN soldered to ground. Combining both series and shunt MELF PINs into a single configuration shows that

the isolation improves dramatically without significantly degrading the insertion loss.

The performance can be optimized for both bandwidth and high frequency performance very easily with additional matching elements. These PINs are typically used as building blocks for more complex circuits such as multi-throw RF switches and attenuators. The low R_s is critical for low insertion loss series switching applications while the low distortion versus forward current is equally as important for attenuator applications.

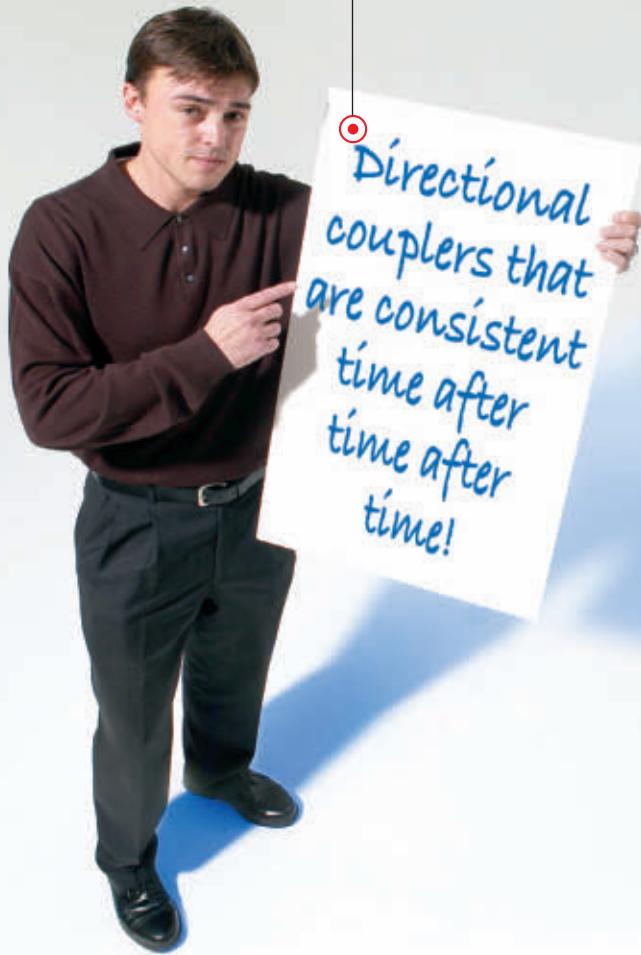
These diodes are also available in non-magnetic packages for MRI applications, which require high voltage handling below 1 GHz. The existence of magnetic materials in a PIN diode structure distorts the static magnetic fields associated with various coils and will interfere with calibration and accuracy. Consequently, non-magnetic MELFs have the ability to optimally receive low power return signals from the human body.

HMIC SURMOUNT PIN DIODES

M/A-COM Technology Solutions has developed a Heterolithic Microwave Integrated Circuit (HMIC) process. It is a silicon and glass-based process that uses silicon pedestals embedded in a low loss, low dispersion glass. Selective backside metallization is utilized with via connectivity to the topside RF traces and air-bridges to produce a surface-mount device. The topside of the die is fully encapsulated with silicon nitride, and has an additional polymer layer to help protect against damage during handling and assembly. This surface mountable solution effectively created is called "surmount" throughout this article. A cross-section of the HMIC process as applied to both series and shunt configured PIN diodes is shown in **Figure 5**.

The shunt diode is realized with the anode, cathode and "I" region contained within a silicon pedestal. The cathode of the PIN diode serves as an electrical contact to the ground plane, and since silicon has a thermal conductivity approximately one third that of gold, acts as a low thermal resistance heat spreader. In addition, HMIC provides a simultaneous cathode contact on the top surface

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XC0900A-05	0.8–1.0	250
XC0900A-10	0.8–1.0	250
XC0900A-20	0.8–1.0	200
XC0900B-30	0.8–1.0	355
XC1500A-20	1.0–2.0	150
1P510	1.7–2.0	20
1P520	1.7–2.0	25
XC1900E-10	1.7–2.0	175
XC1900A-05	1.7–2.0	200
XC1900A-10	1.7–2.0	175
XC1900A-20	1.7–2.0	150
JP506	2.0–2.3	20
JP510	2.0–2.3	20

Part Number	Frequency (GHz)	Power (W)
JP520	2.0–2.3	25
XC2100E-10	2.0–2.3	165
XC2100A-05	2.0–2.3	175
XC2100A-10	2.0–2.3	175
XC2100A-20	2.0–2.3	150
XC2100A-30	2.0–2.3	120
XC2100B-30	1.8–2.7	300
1P610	2.3–2.7	20
1P620	2.3–2.7	25
XC2500P-20	2.3–2.7	20
XC2500E-10	2.3–2.7	145
1M710	3.3–3.7	22
XC3500P-20	3.3–3.8	45
XC3500M-20	3.3–3.8	60
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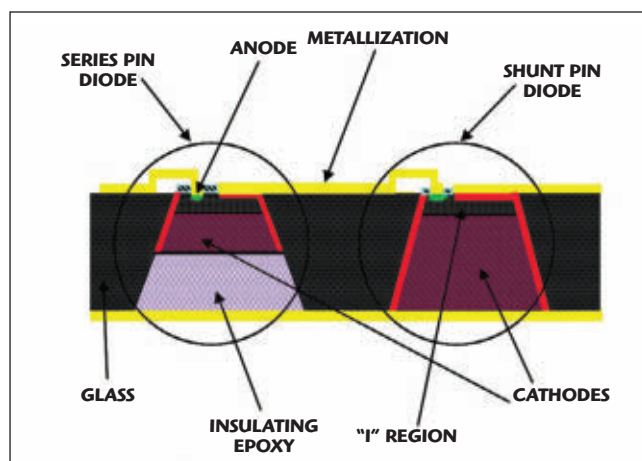
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▲ Fig. 5 HMIC process cross-section.

of the via enabling more complex switch configurations to be realized. Silicon vias to achieve vertical connections (front to back) are a natural consequence of the HMIC fabrication process. The top surface of these vias typically serves as the "active" layer for the formation of the required diode-based active devices and as interconnection paths for the requisite passive elements. The various circuit

is always the weak thermal link in the design since it has the lowest thermal conductivity. A thermally conductive but electrically insulating epoxy isolates the cathode of the diode from the backside of the entire structure. The formation of the series diode is initially identical in formation to the shunt diode. A cavity is created in the silicon cathode using a selective etch that is then packed with a low dielectric con-

elements, either active or passive, are then laterally linked using standard photolithography and metallization techniques.

The shunt diode has the highest power handling so it has a very high thermal conductivity from the surface to ground since its cathode is directly connected to the backside. A series diode, by contrast,

stant, high field strength, silica filled epoxy. This epoxy works very well as a DC and RF isolation medium. The limitation with the surmount diode lies with the silica filled epoxy used to isolate the diode when in series from the RF ground plane. The silica filled material is essentially a thermal open and the only heat sinking that is occurring in the series diode is a result of heat flow along the metallization structures to the nearest silicon via. Using 175°C as the maximum reliable operating junction temperature of the switch, which always occurs at the series diode, the diode insertion loss and thermal resistance become the limiting factors to incident power levels.

Combining glass and silicon enables the high frequency and high power handling properties of the two materials to be optimized while allowing true surface-mount device structures to be produced using standard semiconductor processing equipment and techniques. Glass has a low dielectric constant and a low, high frequency loss tangent, while silicon has high thermal conductivity and low electrical resistance. In addition, both materials have a nearly identical thermal coefficient of expansion.

When using this process to design discrete surmount PIN diodes, as shown in **Figure 6**, the shunt construction shown in Figure 5 is used. The anode connection at the top of the pyramid pedestal on the left is connected to an air-bridge. This air-bridge extends over to a via on the right. This via creates an RF connection from the anode through the air-bridge down the via to the backside of the device. The cathode of the diode is also connected to the backside of the device, yielding a direct cathode heatsink and provides for optimal heat transfer. These backside connections also provide for the surface mountable ability. In addition, thermal conductivity and dissipated power are optimized because these diodes are



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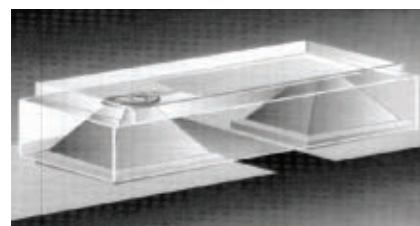
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▲ Fig. 6 Discrete surmount PIN diode.

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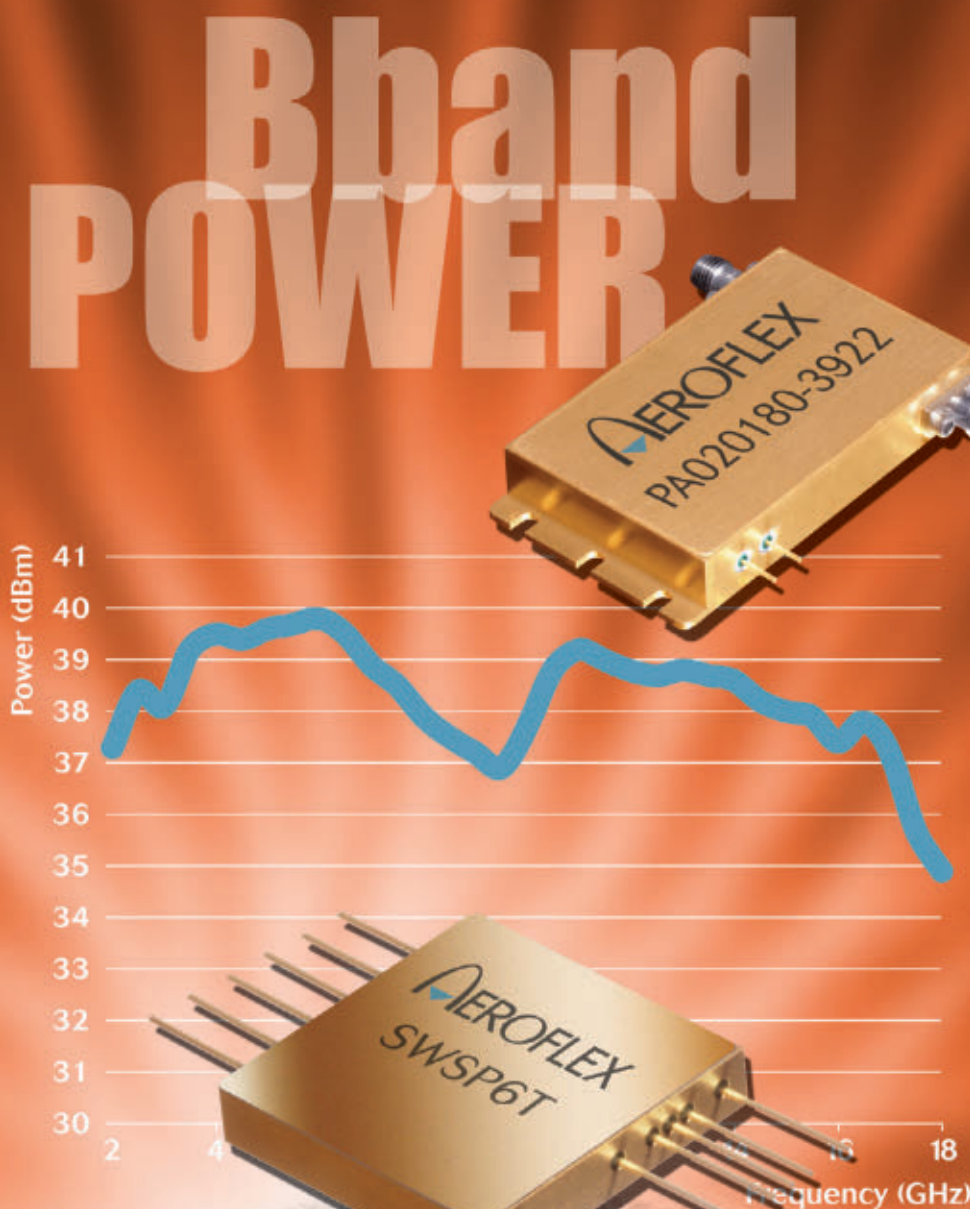
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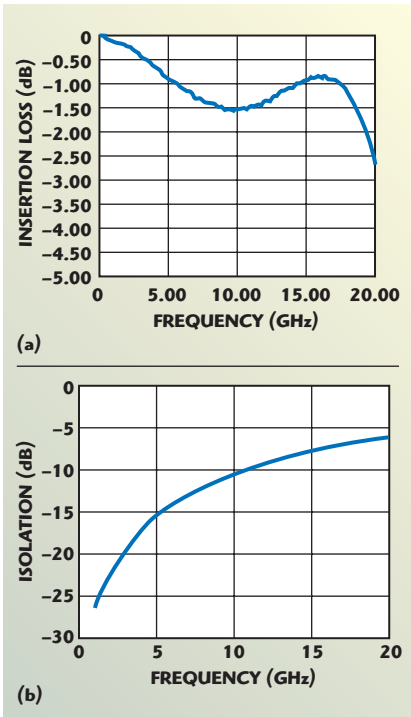
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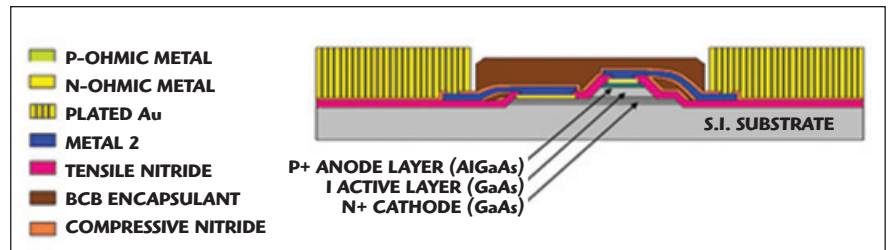


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▲ Fig. 7 S-parameters of a surmount diode.

electrically in series, but thermally in shunt. Surmount diodes have I-region



▲ Fig. 8 AlGaAs flip chip process.

widths that range from 10 to 50 microns are available in different sizes. HMIC surmount PINs are useable in MRI applications as they are non-magnetic devices.

Surmount PIN diodes can exceed 100 W CW power handling at 2 GHz. The “packageless” surmount construction minimizes parasitic capacitances and inductances to minimal values, resulting in performance from 50 MHz to 26 GHz. **Figure 7** demonstrates the broadband small-signal performance of a series mounted surmount diode. Power and bandwidth are two critical attributes and are major differentiators for the HMIC surmount PIN diode option.

FLIP CHIP AlGaAs PIN DIODES

One chip type that currently transcends multiple semiconductor platforms is flip chip PIN diodes. The AlGaAs diodes combine Aluminum (in the P+ region) and Gallium Arsenide (in the I and N regions), which improves the insertion loss significantly at higher frequency ranges. Due to the reduced recombination rate for electrons and the higher carrier injection rate with an Aluminum-GaAs heterojunction, a greater number of carriers can flow through the I-region, thereby lowering the effective resistivity of the I-region. Fabricated AlGaAs diodes effectively have lower diode “ON” resistance than conventional GaAs devices by as much as 25 percent. Consequently, AlGaAs PIN diodes outperform silicon beam leads and chip devices for a variety of broadband switching applications. **Figure 8** shows the vertical construction of the PIN diode and **Figure 9** shows several flip chips from the top view.

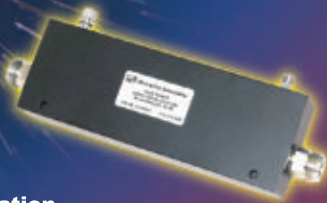
A flip chip PIN diode connects to a substrate from the top pads of the package. Consequently, the chip has to be flipped and epoxied down to a medium using electrically conductive Ag epoxy. The BCB encapsulant covering the die acts as protection upon the flipping of the diode. This flip chip package construction combined with the AlGaAs process yields a device with capacitance as low as 0.025 pF and operational frequencies beyond 70 GHz. The AlGaAs PIN diode flip chip has good broadband high frequency performance and the fastest switching performance because of its low parasitics and thin I-regions. A common tradeoff with high frequency performance is lower power handling capability, as is the case with flip chips. The PIN diodes are rated up to 23 dBm of CW input power. **Figure 10** shows small-signal S-parameter data for a typical AlGaAs flip chip in a series configuration. The device pro-

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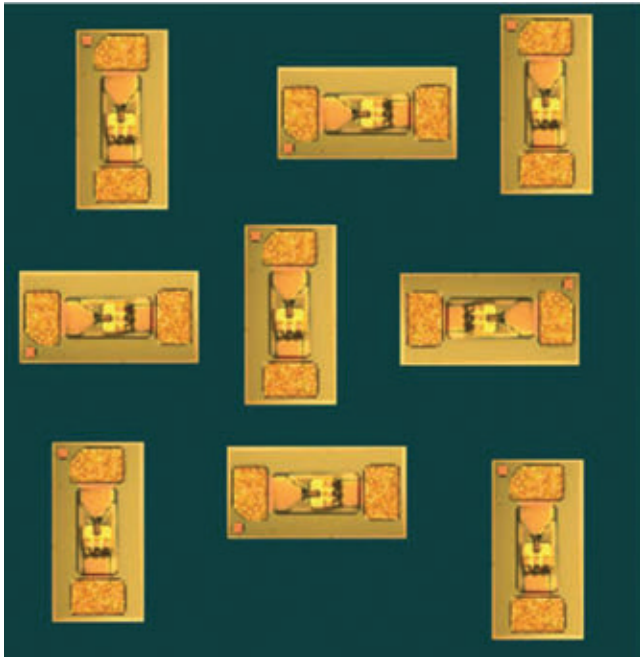


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▲ Fig. 9 Flip chips—top view under magnification.

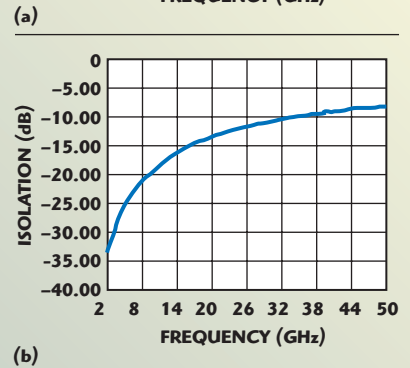
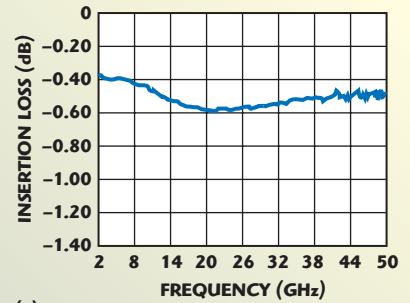
vides significant circuit tuning advantages due to the low total capacitance C_t (< 18 fF), series resistance R_s (4 ohms at 20 mA) and series inductance

are the most basic, but there are also designs with multiple cascaded series diodes and multiple shunt diodes on a single arm.

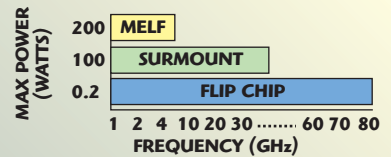
L_s (0.5 nH). These specifications provide a 0.072 ps RC time constant that affords greater operating bandwidth.

COMPARISON OF TECHNOLOGIES

One major advantage to discrete PIN diodes is that customers are able to easily and quickly customize their diode topology to meet their RF performance needs. **Table 1** shows three popular PIN diode switch topologies and each of their strengths and weaknesses. These three switch topologies



▲ Fig. 10 S-parameters of a AlGaAs flip chip.



▲ Fig. 11 Diode comparison, frequency vs. power.

Figure 11 shows how the three diode processes and packaging technologies compare with each other over frequency and maximum CW input power. The trend in performance is typically the maximum operating frequency and maximum CW incident power are inversely related. The MELF PIN diode can handle up to 200 W of CW incident power, but has the narrowest and lowest frequency band of operation. Alternatively, the flip chip PIN diode has been shown to operate beyond 80 GHz with the broadest bandwidth performance, but with limited power handling of 0.2 W incident power. The optimal compromise between frequency and power was described with the HMIC surmount PIN diodes, which can han-

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TABLE I**SWITCH TOPOLOGY STRENGTHS AND WEAKNESSES**

Parameter	Switch Design Configurations		
	Series Diodes	Shunt Diodes	Series-shunt Diodes
Insertion Loss	Best at Higher Freq.	Best at Lower Freq.	Moderate
Isolation	Worst	Moderate	Best
Return Loss	Moderate	Worst	Best
RF Incident Power	Worst	Best	Moderate
RF Power Dissipation	Worst	Best	Moderate
Switching Speed	Worst	Best	Moderate
DC Power Consumption	Best	Moderate	Worst
PIN Diode Driver Simplicity	Best	Moderate	Worst

dle up to 100 W of incident power while still achieving broadband performance up to 26 GHz.

CONCLUSION

MELF, surmount and AlGaAs flip PIN diodes were described and com-

pared against each other. Each type of PIN diode has clear advantages, depending on the end application. The PIN starting material, I-region thickness and packaging technology play major roles in the diode performance.



Kevin Harrington holds his MS degree in Electrical Engineering from the University of Massachusetts, Amherst. He brings to M/A-COM Technology

Solutions more than 13 years of experience in GaAs RF IC design and five years of product management. He is currently Product Development Manager responsible for HMIC diode & GaAs IC product development across multiple markets.



Scott Vasquez holds his MS degree in Electrical Engineering from Tufts University. He has been an applications engineer with M/A-COM

Technology Solutions for over two years. He is currently a Product Manager responsible for diode-based products.

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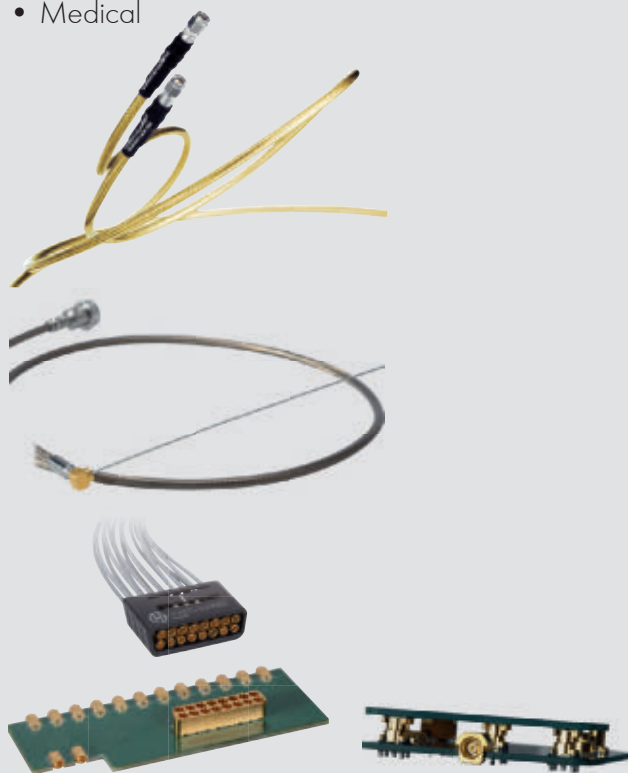


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THEORY AND PROPOSED METHOD FOR DETERMINING LARGE-SIGNAL RETURN LOSS OR “HOT S_{22} ” FOR POWER AMPLIFIERS

Power amplifiers (PA) are a critical functional block in today's wireless communications. They are found in every cell phone, cordless phone, RF remote controller, etc. Any application requiring the wireless transmission of analog or digital signals will require a PA. In wireless equipment, the PAs are usually placed as close as possible to the antenna to minimize RF losses, maximize power efficiency and maximize battery life. RF systems engineers need to determine the PA return loss under actual output power drive levels. This so-called “Hot S_{22} ” is needed to calculate the mismatch loss at the antenna interface and to determine the actual wireless system transmit power (a key requirement for regulatory bodies, such as the FCC).

The verification of a PA output return loss has proven to be a problematic and challenging endeavor when the PA is delivering high output power. High power PAs will inadvertently heat up as the output power levels are increased.

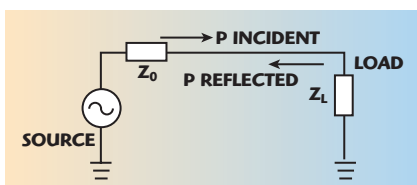
Under high output power conditions, the power transistor's parameters may significantly change as temperature and bias conditions change.¹ Therefore, the PA output return loss may be substantially different when operated under low output power versus high output

power. Most PA suppliers will only publish return loss values under small-signal conditions. These values should be checked against actual high power conditions when conducting systems transmit power budgets. A number of test equipment suppliers have “off-the-shelf” test hardware for measuring the return loss of high power units,^{2,3} but these solutions are usually very expensive, and may not justify the investment for engineers conducting only occasional high power tests.

This article outlines a simple and cost-effective solution for determining the return loss of a high power PA. A test procedure is outlined, based on a mathematical approach, to determine the PA large- (or small-) signal return loss by measuring the insertion phase variation of the PA at specific VSWRs, using an inexpensive and simple test arrangement.

PA REFLECTION COEFFICIENT

Any RF test configuration can be expressed by a source impedance Z_L , and a characteristic impedance (Z_0), as shown in **Figure 1**. If the load impedance is equal to the source characteristic impedance then the reflected traveling



▲ Fig. 1 Power transmission from source to load.

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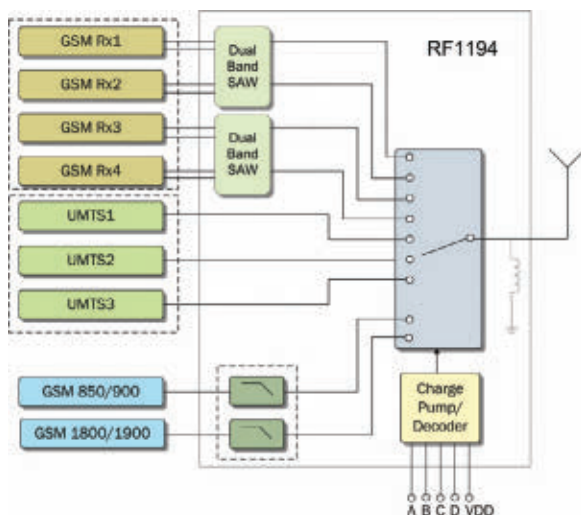


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						GSM LB (dBm)	GSM HB (dBm)	UMTS (dBm)	GSM LB Tx (dB)	GSM HB Tx (dB)	UMTS Tx (LB/HB) (dB)	UMTS Rx (LB/HB) (dB)	GSM Rx (LB/HB) (dB)					
RF1193 SP10T	ASM (QB GSM, QB UMTS)	GPIO	Yes	No	Not Required	35	33	26	1.05	1.3	0.5 / 0.75	0.5 / 0.75	0.8 / 1.2	<-78	<-78	110	65	3.0 x 3.8 x 0.85
RF1194 SP9T	SFM (QB GSM, TB UMTS)	GPIO	Yes	Yes	Not Required	35	33	26	1.2	1.3	0.75 / 1.0	0.75 / 1.0	2.3 / 3.1	<-78	<-73	110	65	4.5 x 4.5 x 1.3

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wave does not exist (as is the case for a matched load). However, when Z_L is not equal to the PA output impedance Z_0 , then the traveling wave V between the PA to the load contains two components: one is traveling in the +z direction and the other traveling in the -z direction.

$$V = V_+ e^{-\gamma Z} + V_- e^{+\gamma Z} \quad (1)$$

The traveling wave in the +z direction is the incident power, and the traveling wave on the -z direction is the reflected power.

$$V_{inc} = V_+ e^{-\gamma \bullet Z} \quad (2)$$

$$V_{ref} = V_- e^{+\gamma \bullet Z} \quad (3)$$

where γ is the propagation constant.

Now replace the source with an actual PA and the load with a phase tuner, which rotates the phase by 2π radians and causes, in theory, full reflection back to the PA, as illustrated in **Figure 2**. The reflection coefficient is determined to be the ratio between the reflected and the incident vector as follows:

$$\Gamma_L = \frac{V_-}{V_+} e^{j\theta} \quad (4)$$

$$\Gamma_{PA} = \frac{V'_+}{V_-} e^{j\psi} \quad (5)$$

where:

Φ is the shifted phase caused by the PA

Θ is the phase angle of the reflection coefficient Γ_L

Ψ is the phase angle of the reflection coefficient Γ_{PA}

The summing vector, V , in the coupled port contains three vectors that are directed from three different paths, that is:

$$V_1 = V_{inc} \cdot CF \quad (6)$$

$$V_2 = V_{inc} \cdot \Gamma_{PA} \cdot \Gamma_L \cdot CF \quad (7)$$

$$V_3 = V_{inc} \cdot \Gamma_L \cdot CF \cdot DR \quad (8)$$

where CF is the bidirectional coupling factor and DR is the directivity for the bidirectional coupler.

$$V = V_1 + V_2 + V_3 \quad (9)$$

$$V = CF \cdot V_+ e^{j\omega_0 t + \phi} + CF \cdot \Gamma_{PA} \cdot \Gamma_L \cdot V_+ e^{j\omega_0 t + \phi} + CF \cdot DR \cdot \Gamma_L \cdot V_+ e^{j\omega_0 t + \phi} \quad (10)$$

Using directional couplers with $DR > 20$ dB, ensures that V_3 is much smaller than V_2 , that is:

$$V_2 \gg V_3 \quad (11)$$

It is recommended that the directivity for the bidirectional coupler should be higher than the PA return loss by 15 dB. This will ensure that the vector V_3 will remain negligible.

Directivity \geq PA R.L. + 15 dB

If V_3 is negligible, then the vector V can be reduced to:

$$V = V_1 + V_2 \quad (12)$$

$$V = CF \cdot V_+ e^{j\omega_0 t + \phi} (1 + |\Gamma_{PA}| \cdot |\Gamma_L| \cdot e^{j(\theta + \psi)}) \quad (13)$$

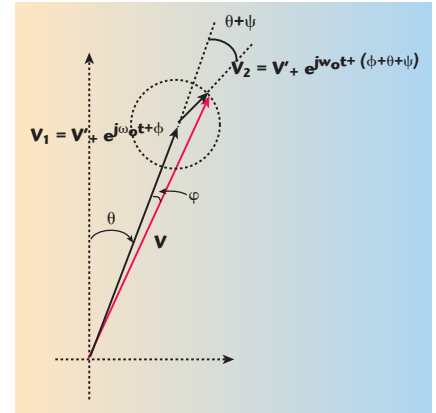
$$\Gamma_{Total} = \Gamma_{PA} \cdot \Gamma_L = \frac{V'_+ e^{j\omega_0 t + (\theta + \phi + \psi)}}{V_+ e^{j\omega_0 t + \phi}} \quad (14)$$

$$V = CF (V_+ e^{j\omega_0 t + \phi} + V'_+ e^{j\omega_0 t + (\theta + \phi + \psi)}) \quad (15)$$

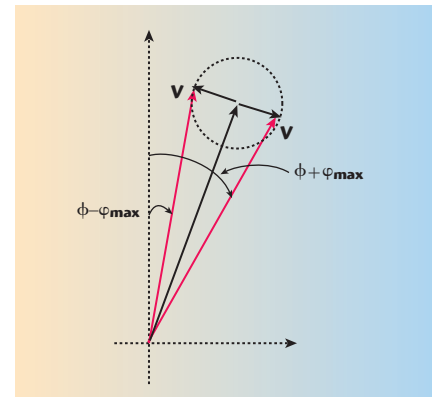
The summing vector V , as illustrated in **Figure 3**, contains the vector V_1 , which represents the incident wave and the vector V_2 , which represents the reflected wave.

The angle φ is the angle between the incident vector V_1 to the summing vector V and is also determined as the variation in PA insertion phase between the PA insertion phase at VSWR=1:1 to the PA insertion phase when the phase tuner is shifted with in 2π radians with VSWR>1.

There are two locations on the phase tuner where the maximum and minimum PA insertion phase is achieved. At these two locations, the reflected vector is perpendicular to the incident vector



▲ Fig. 3 The reflected wave vector is rotating 2π radians across the incident wave vector.



▲ Fig. 4 Vector diagram for maximum and minimum insertion.

$$(\theta + \Psi = \frac{\pi}{2} \text{ or } \theta + \Psi = -\frac{\pi}{2})$$

and the angle φ reaches the highest value, φ_{MAX} , as shown in **Figure 4**. At these two locations of 90° insertion phase, the product of the load and PA reflection coefficients can be written as:

$$\Gamma_{Total} = \Gamma_L \cdot \Gamma_{PA} = \frac{V'_+ e^{j\omega_0 t + (\phi + \frac{\pi}{2})}}{V_+ e^{j\omega_0 t + \phi}} = \frac{V'_+ e^{j\omega_0 t + (\phi - \frac{\pi}{2})}}{V_+ e^{j\omega_0 t + \phi}} = \tan \varphi_{max} \quad (16)$$

$$-20 \log |\Gamma_{Total}| = -20 \log \tan \varphi_{max} \quad (17)$$

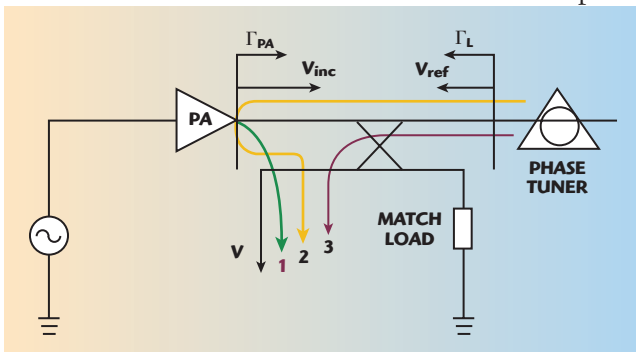
$$-20 \log |\Gamma_{PA}| - 20 \log |\Gamma_L| = -20 \log \tan \varphi_{max} \quad (18)$$

$$-20 \log |\Gamma_{PA}| = -20 \log \tan \varphi_{max} + 20 \log |\Gamma_L| \quad (19)$$

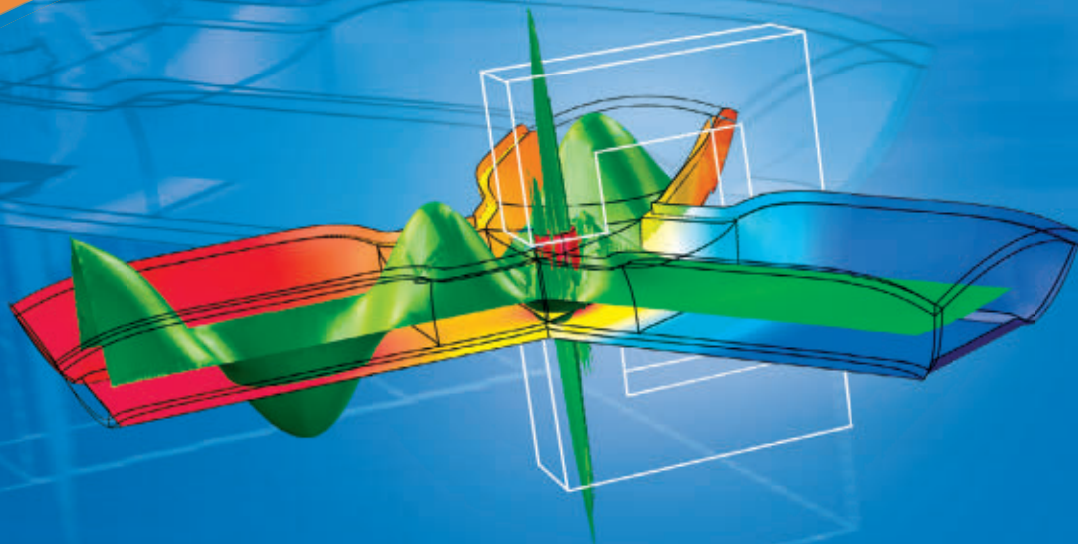
Since the phase tuner has a full reflection then $\Gamma_L = 1$ and the PA return loss (in dB) can be expressed as:

$$PA_R.L. = -20 \log \tan \varphi_{max} \quad (20)$$

φ_{MAX} can be found by rotating the

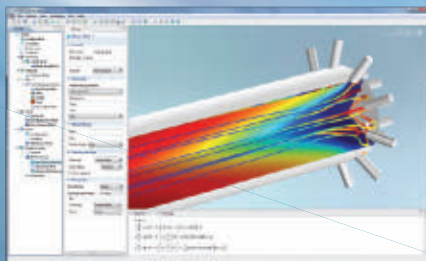


▲ Fig. 2 PA in a mismatch system.



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phase tuner within 2π radians and the maximum insertion phase can be searched using a phase detector with the test setup shown in **Figure 5**.

PA REFLECTION COEFFICIENT WITH A DETERMINED MISMATCH LOAD

In practice, PAs are specified over a limited VSWR range. The PA can be damaged or unstable with a load VSWR above what has been specified by the vendor.

Therefore, the same analysis will be given when the load phase tuner is connected to the PA through an attenuator in order to limit the VSWR that will reflect on the PA (see **Figure 6**).

$$V = V_1 + V_2 \quad (21)$$

$$V = CF \cdot (V_+ e^{j\omega_0 t + \phi} + (Att)^2 \cdot V_+ e^{j\omega_0 t + (\theta + \phi + \psi)}) \quad (22)$$

$$\tan \varphi_{\max} = (Att)^2 \cdot \frac{V_+ e^{j\omega_0 t + (\theta + \phi + \psi)}}{V_+ e^{j\omega_0 t + \phi}} =$$

$$(Att)^2 \cdot \Gamma_L \cdot \Gamma_{PA} \quad (23)$$

$$\Gamma_{PA} = \frac{\tan \varphi_{\max}}{(Att)^2 \cdot \Gamma_L} \quad (24)$$

$$PA_R.L. = -20 \log \Gamma_{PA} = -20 \log \left(\frac{\tan \varphi_{\max}}{(Att)^2 \cdot \Gamma_L} \right) \quad (25)$$

Since the phase tuner has a full reflection, $\Gamma_L = 1$, the PA return loss can be expressed as:

$$PA_R.L. = -20 \log \Gamma_{PA} = -20 \log \left(\frac{\tan \varphi_{\max}}{(Att)^2} \right) \quad (26)$$

or

$$-20 \log (\tan \varphi_{\max}) = PA_R.L. (dB) + 2 \cdot Att (dB) \quad (27)$$

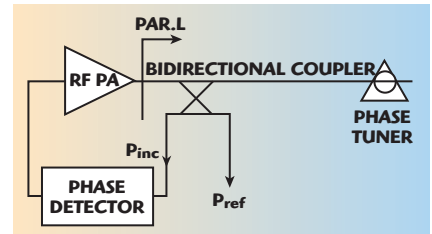
If the PA return loss is high and the attenuator used between the PA to the phase tuner is high, then the phase angle φ_{\max} may be small and difficult to measure in order to have accurate results. Therefore, it is suggested to use a small attenuator (1 to 3 dB) between the PA and the phase tuner.

TEST METHOD

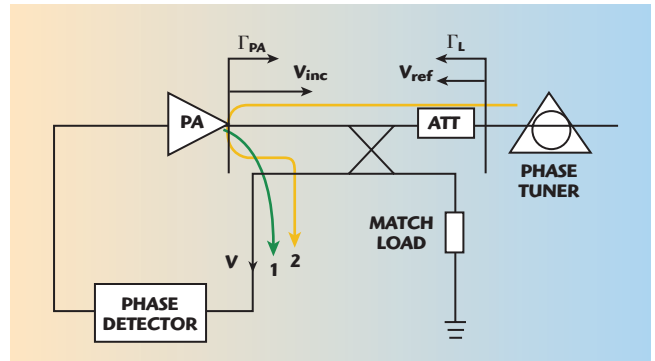
Step 1:

Connect the PA as illustrated in **Figure 7** using a 50 Ω load at the output of a bidirectional coupler (additional attenuation can be connected in front of the phase detector whenever it is desired to measure the return loss for a very high power PA).

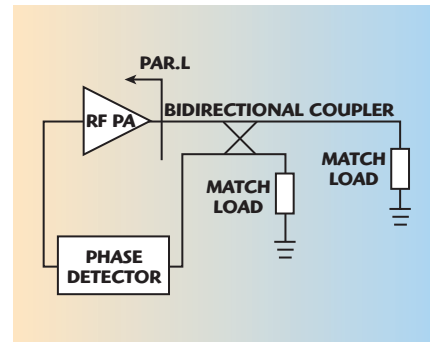
Measure the insertion phase at the various frequencies of interest using small-signal or large-signal input power. The insertion phase with a 50 Ω load will be the reference insertion phase before loading the PA with different VSWRs.



▲ Fig. 5 Test setup for measuring maximum insertion phase.



▲ Fig. 6 Test setup for measuring maximum insertion phase with limited VSWR.



▲ Fig. 7 Test setup for matched load.

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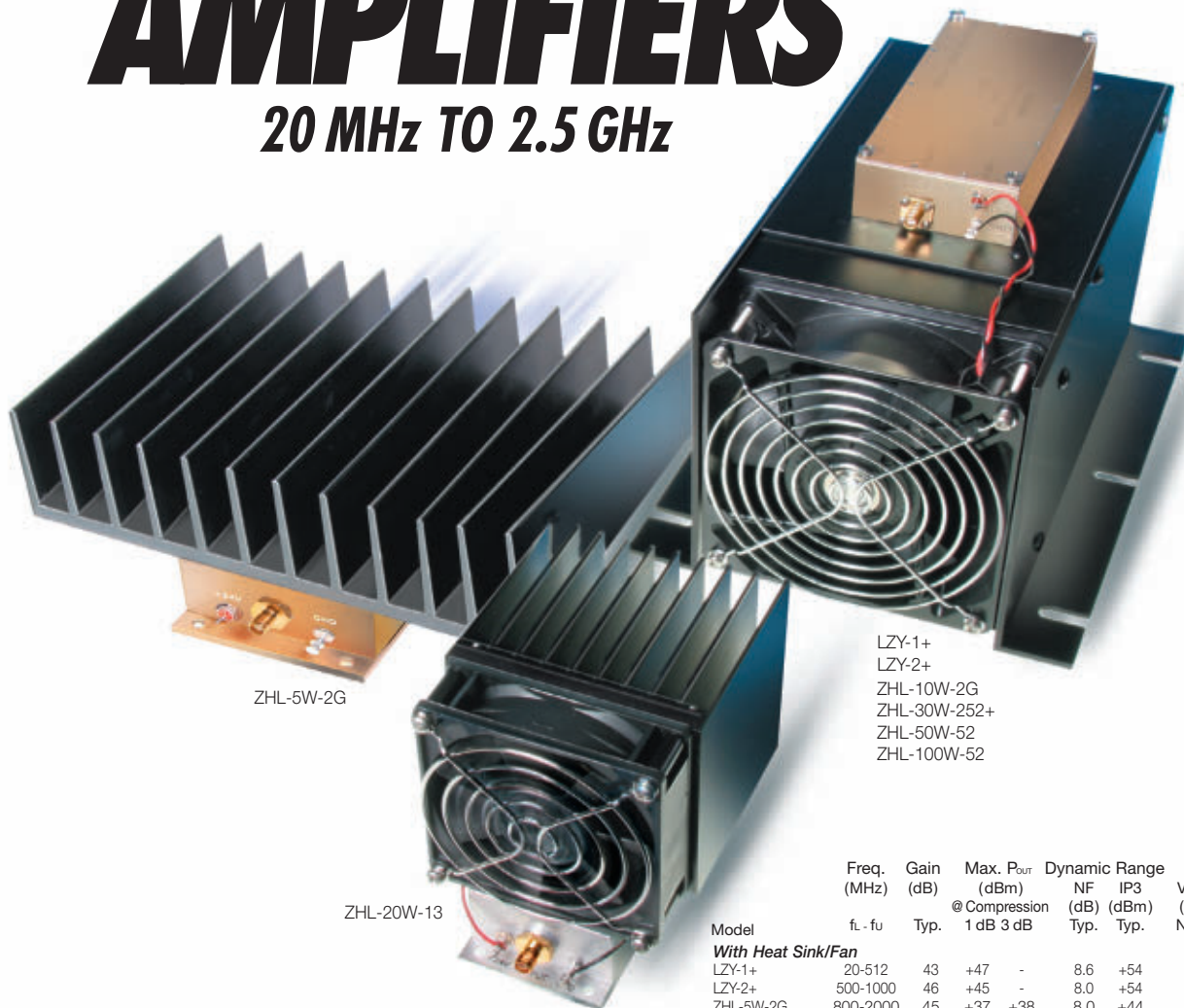
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For many years Tecdia has produced top of the line high current (5, 10 and 20A) bias tee models capable of handling a DC bias voltage of 30V, and RF power of 50W. Now, to meet the higher voltage and power requirements of GaN devices, Tecdia is introducing this new design that has the following specifications :

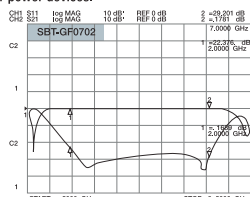
SPECIFICATION

Series	SBT	
Model	SBT-GF0702	
Frequency Range	2~7GHz	
Insertion Loss	0.5dB max.	
VSWR (Return loss)	1.22 max. (20dB min.)	
Connectors	RF	APC-7
	DC	BNC-R (Female)
RF Power	50W max.	100W max.
Bias Current	20A max.	10A max.
Bias Voltage	30V max.	150V max.
Dimensions (mm)*	50 x 52 x 20	
Weight	200g	

* Excluding Connectors

Typical VSWR & Insertion Loss

SBT-GF0702
These Bias-Ts are the optimum choice for measurement of high-power devices.



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In **Table 1**, the measured value for a high power (2 W), 350 to 470 MHz, Skyworks' PA (SKY65141), is shown.

Step 2:

Disconnect the 50 Ω load at the output of the bidirectional coupler and connect a 1.5 dB pad in order to present the PA with a VSWR = 6. Place a phase tuner after the fixed attenuator pad. The phase tuner must be capable of continuously varying the insertion phase from 0 to 360°. The test setup is illustrated in **Figure 8**. Adjust the phase tuner in order to find the highest and lowest insertion phase and calculate at each frequency what the maximum phase variation is, compared to the insertion phase at 50 Ω , as indicated in **Table 2**. Note that the attenuator value is selected to be within the specified PA load VSWR range. The total output insertion loss should be measured at each maximum insertion phase location on the phase tuner in order for the return loss to be calculated accurately.

In theory $\varphi_{MAX} = \varphi_{MIN}$, therefore the following equation is valid:

$$\frac{\varphi_{max} - \varphi_{min}}{2} = \varphi_{max} - \varphi_{50\Omega} = \varphi_{50\Omega} - \varphi_{min} \quad (28)$$

However, in practice φ_{MAX} and φ_{MIN} may not be equal since the phase tuner may not be ideal and symmetric. Therefore, the insertion phase at VSWR = 1 ($\varphi_{50\Omega}$) is subtracted from the absolute value for the maximum phase variation ($\phi - \varphi_{MAX}$ or $\phi + \varphi_{MAX}$).

The return loss of the PA is calculated according to the following formula:

$$PA_R.L. = -20 \log \left[\frac{\tan \varphi_{max}}{(Att)^2} \right] \quad (29)$$

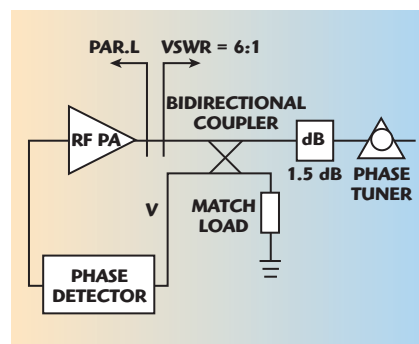
where θ_{MAX} is in degrees and Att is the measured attenuation from the PA output to the phase tuner input.

TEST RESULTS

The theoretical analysis shown in

TABLE I INSERTION PHASE WITH VSWR=1 FOR A SKYWORKS PA	
Frequency (MHz)	Insertion Phase at VSWR 1:1 and Pin=4 dBm @50 Ω
350	171.4
410	71.2
470	-30.5

TABLE II MEASURED MAXIMUM AND MINIMUM INSERTION PHASE WITH VSWR=6			
Frequency (MHz)	Minimum Insertion Phase ($\phi - \varphi_{max}$)	Maximum Insertion Phase ($\phi + \varphi_{max}$)	Maximum Insertion Phase Variation φ_{max}
350	157.1	179.9	12.2
410	62.3	75	6.7
470	-42	-26.2	8.6



▲ Fig. 8 Test setup for mismatched load.

the above sections was verified using a high power 2 W SMT PA from Skyworks (SKY65141). The PA was tested over its entire operating frequency range, 350 to 470 MHz. The actual return loss measurement was made with a network analyzer at small input signal and the results are given in **Figure 9**.

The measurement results are compared to the calculated return loss using the proposed phase measurement procedures outlined in the above sections.

The new test procedure was done using different load VSWRs to demonstrate that the return loss measurements are repeatable at different VSWRs. The return loss obtained using the new proposed phase technique is shown in **Figures 10** and **11**.



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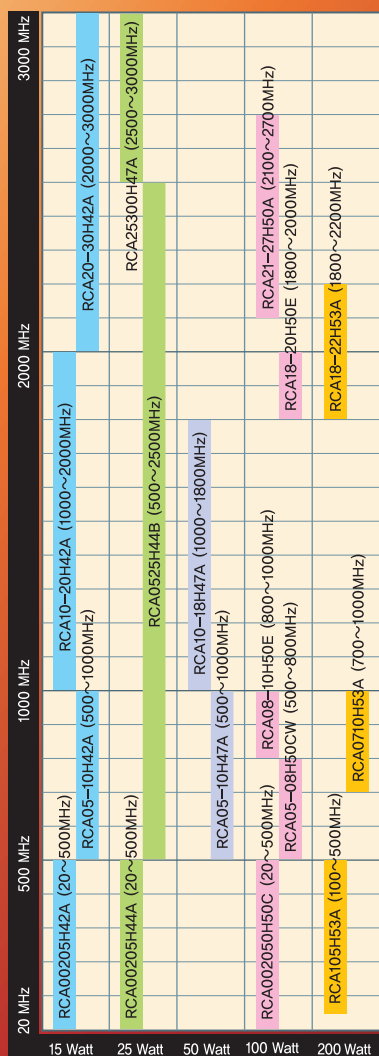
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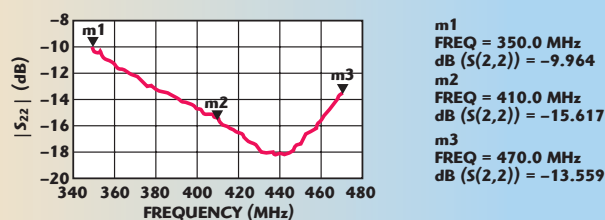
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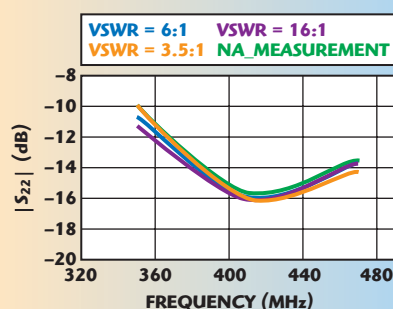
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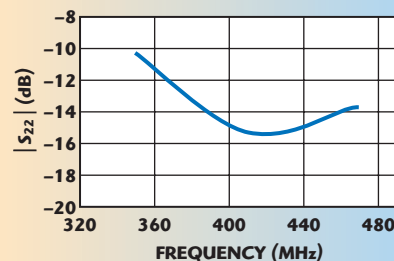
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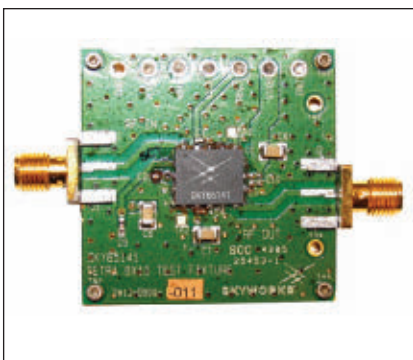
▲ Fig. 9 Return loss measured at low power.



▲ Fig. 10 Calculated PA return loss at $P_{in} = -30$ dBm.



▲ Fig. 11 Calculated return loss $P_{in} = -4$ dBm and VSWR = 3.5.



▲ Fig. 12 Photo of high power PA (SKY65141) mounted in its test fixture.

The same method was used to calculate the PA return loss using higher input signal with VSWR = 3.5. A photo of the PA mounted in its test fixture is shown in **Figure 12**.

CONCLUSION

A PA return loss is a parameter, which can vary depending on the PA output power, the PA bias current, etc. Therefore, the PA return loss under high output power conditions should be measured and not be assumed to be the same as the return loss measured under small-signal output power conditions. The PA

return loss can be calculated from the phase between the summing (incident and reflected vectors) to the incident vector, which is measured with a matched-load.

This article demonstrates that the "hot" PA return loss can be accurately calculated by measuring the maximum insertion phase variation at any given VSWR, and at any given input drive level. The proposed return loss measurement technique can be implemented using low cost test components, eliminating the need for costly network analyzers. ■

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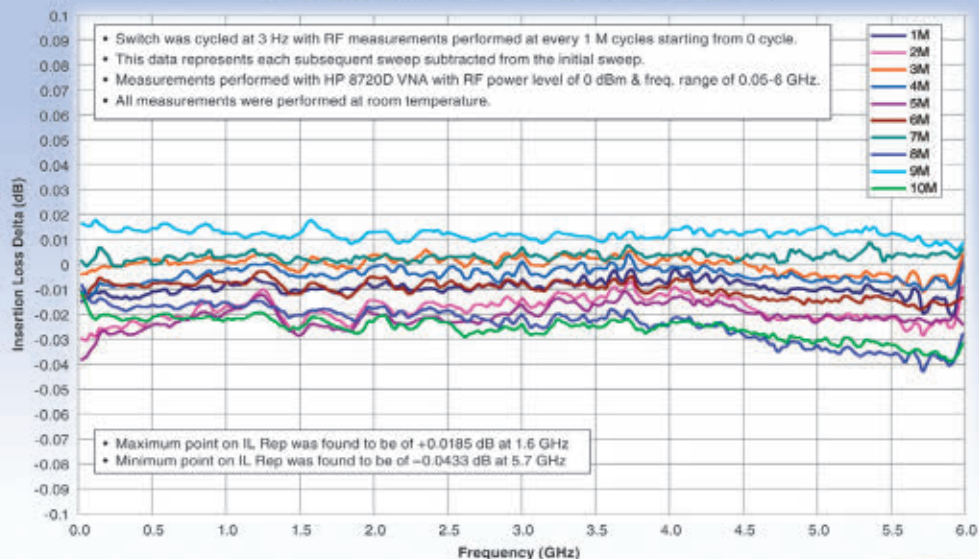


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KA-BAND BANDPASS FILTER USING A CPW STRUCTURE TECHNOLOGY WITH COPPER ON AN Al_2O_3 SUBSTRATE

This article presents the performance of a Ka-band bandpass filter (BPF) using a coplanar waveguide (CPW) topology on an Al_2O_3 substrate. A copper (Cu) metallization was also used in this investigation to improve the characteristics of the filter. The measured results of the BPF, with a chip size of $2423 \times 424 \mu\text{m}$, show a return loss of 25.3 dB and an insertion loss of 0.6 dB at 27 GHz. A comparison between the simulated and experimental results shows good agreement. The overall filter characterization exhibits a broad bandwidth of 18.8 to 38.2 GHz, a high return loss and a low insertion loss, which illustrate that the BPF shows favorable RF characteristics in Ka-band with a compact circuit size.

The communication applications have increased noticeably in recent years. Apparently, the RF channel bandwidth allocated to communication system applications is approaching saturation. The providers of communication systems are now interested in the microwave band for the next-generation terrestrial systems, including military and satellite communication systems in Ka-band. Several researchers^{1,2} have reported that microwave monolithic integrated circuits (MMIC) using coplanar waveguide have been adopted in transmitter communication systems. In the

CPW structure, the ground plane is placed on the top surface of the substrate. Thus, many advantages have been obtained with this CPW schematic layout, such as unnecessary back-side fabrication, good electronic isolation property and compact drawing in the circuit layout.¹⁻³

As clearly shown in some review papers, CPW has been extensively studied for MMIC applications. However, little attention has been devoted to the conductor losses in the signal transmission path.^{2,3} A copper metal, with an extremely low electrical resistivity ($1.7 \times 10^{-8} \Omega\text{m}$), could significantly improve the insertion loss in the BPF.⁴ This study investigated a Ka-band BPF circuit using a CPW structure and a copper metallization on the Al_2O_3 substrate. A Ka-band BPF was fabricated and its S-parameters were measured with a vector network analyzer. The results demonstrated that the fabricated Ka-band BPF exhibited favorable MMIC characteristics within a small size.

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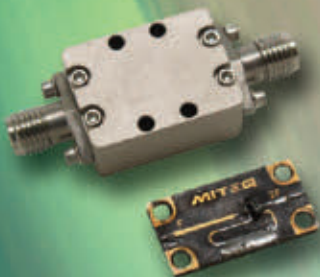
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DM0052LA2	0.5 – 2	DC – 0.5	7 – 13	6.5/8.5	30
DM0104LA1	1 – 4	DC – 1	7 – 13	5.5/7	30
DM0208LW2	2 – 8	DC – 2	7 – 13	7/8	30
DM0408LW2	4 – 8	DC – 2	7 – 13	5/6	30
DM0812LW2	8 – 12	DC – 4	7 – 13	4.5/6	30
DM0416LW2	4 – 16	DC – 4	7 – 13	7/8	30
DB0218LW2	2 – 18	DC – 0.75	7 – 13	6.5/8.5	22
DB0226LA1	2 – 26	DC – 0.5	7 – 13	9/10	20
DB0440LW1	4 – 40	DC – 2	10 – 15	9/10	20
M2640W1	26 – 40	DC – 12	10 – 15	10/12	28
TRIPLE-BALANCED VERSIONS					
TB0218LW2	2 – 18	0.5 – 8	10 – 15	7.5/9.5	20
TB0426LW1	4 – 26	0.5 – 8	10 – 15	10/12	20
TB0440LW1	4 – 40	0.5 – 20	10 – 15	10/12	18

PASSIVE DOUBLERS



Model Number	Input Frequency (GHz)	Input Power (dBm)	Output Frequency (GHz)	Conversion Loss (dB) Typ./Max.	Rejection (dBc) Typ. Fund. Odd Harm.
DROP-IN VERSIONS					
SXS01M	0.5 – 3	8 – 12	1 – 6	13/16	-20 -25
SXS04M	2 – 9	8 – 12	4 – 18	13/15	-20 -25
SXS07M	3 – 13	8 – 12	6 – 26	13/18	-18 -25
CONNECTORIZED VERSIONS					
SXS2M010060	0.5 – 3	8 – 12	1 – 6	13/16	-20 -25
SXS2M040180	2 – 9	8 – 12	4 – 18	13/15	-20 -25
SXS2M060260	3 – 13	8 – 12	6 – 26	13/17	-18 -25
MX2M130260	6.5 – 13	8 – 12	13 – 26	11/13	-15 -15
MX2M004010	0.02 – 0.5	8 – 12	0.04 – 1	10.5/13	-25 -25



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DESIGN AND FABRICATION OF A KA-BAND BANDPASS FILTER

The Ka-band BPF circuit was designed using a CPW structure. **Figure 1** shows the schematic layout of the Ka-band BPF, which uses two series open stubs with a characteristic impedance $Z_0 = 50 \Omega$ and a length (l), which was designed to be approximately a quarter wavelength at the Ka-band center frequency (λ_{eff}), that is, $l = \lambda_{\text{eff}}/4$.⁵ Ports 1 and 4 are the input and output of the filter, while Ports 2, 3, 5 and 6 are connected to ground. The lumped equivalent circuit model of the BPF is shown in **Figure 2**. In effect, each open stub is equivalent to three LC tanks (L_1/C_1 , L_2/C_2 and L_3/C_3) with an air-gap (C_0) series connection. This circuit permits a low transmission loss and easy fabrication.³ These resonators, with LC tanks, can operate in a wideband BPF. The resonators are operating in a mixed coupled mode, meaning partially magnetically and partially electrically coupled.

The S-parameters of the coupled resonating filter were simulated with the Advanced Design System (ADS), and the effect of the electric-magnetic coupling within the Ka-band BPF layout were computed with the HP-Momentum. Subsequently, the Ka-band BPF was laid-out and fabricated on an Al_2O_3 substrate 0.5 mm thick and with a conductor layer 2 μm thick, consisting of a Ti layer, 300 Å thick, to enhance adherence, the copper layer and a thin Au layer, 2000 Å thick, to prevent oxidation. **Figure 3** shows a microphotograph of the Ka-band BPF, with a chip area of $2423 \times 424 \mu\text{m}$.

THE S-PARAMETERS OF A KA-BAND BANDPASS FILTER

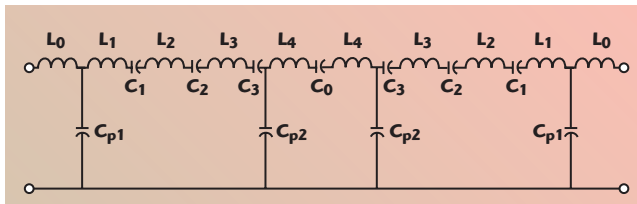
Figures 4 and **5** show the measured and simulated S-parameters of the Ka-band BPF. A simulated insertion loss (S_{21}) of -0.6 dB and return loss (S_{11}) of -10 dB were obtained within a bandwidth of 21.6 GHz, in the range 17.2 to 38.8 GHz. The BPF showed an input return loss exceeding -20 dB, from 25 to 35 GHz, in both measurements and simulation, as well as a maximum simulated return loss of -55 dB at 30 GHz.

The results indicate that the measured return loss is slightly degraded and shifted in frequency, compared with the simulation. The most likely explanation was that the variations in fabrication might be the cause of the negligible shift in the center frequency and the small degradation in the return loss. The simulated and measured S_{21} results agree fairly well, with the insertion loss remaining approximately constant in the range of 20 to 35 GHz. Overall, the S-parameters characterization confirms the low insertion loss and high return loss in this Ka-band BPF.

Finally, the S-parameters of the Ka-band BPF are summarized in **Table 1**.



▲ Fig. 1 Schematic of the CPW Ka-band bandpass filter.



▲ Fig. 2 Equivalent circuit of the Ka-band bandpass filter.

TABLE 1

SUMMARY OF MEASURED AND SIMULATED S-PARAMETERS OF THE KA-BAND BANDPASS FILTER

Ka-band Bandpass Filter	Simulated	Measured
Center frequency	30 GHz	27.7 GHz
Bandwidth	21.6 GHz @ 17.2 to 38.8 GHz	19.4 GHz @ 18.8 to 38.2 GHz
Return loss (S_{11})	-57 dB @ 30 GHz	-25.3 dB @ 27.7 GHz
Insertion loss (S_{21})	-0.6 dB @ 30 GHz	-0.6 dB @ 27.7 GHz

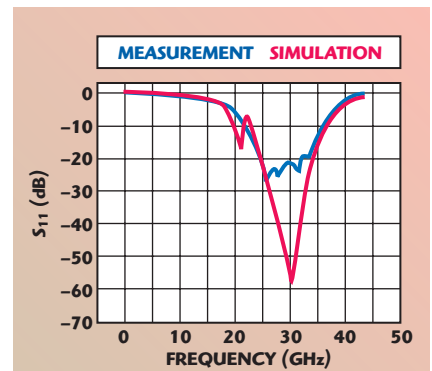
The experimental results appeared to be consistent with the simulation values. These S-parameter results indicate that the Ka-band BPF filter was well designed, demonstrating that the CPW structure with copper metallization on an Al_2O_3 substrate is adequate for the MMIC applications.

CONCLUSION

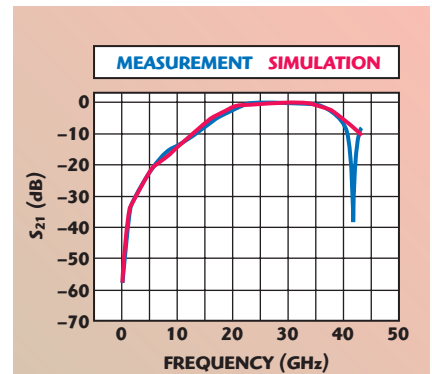
In this article, a Ka-band bandpass filter, using a CPW structure on an Al_2O_3 substrate with a copper metallization, was described. The use of copper metallization, which has a high conductivity, can reduce the insertion loss and improve the return loss of the circuit. The Ka-band BPF design uses two series open stubs with a characteristic impedance $Z_0 = 50 \Omega$, whose lumped element equivalent circuit consists of three LC tanks. The measured S-parameters agreed well with the simulation values. The Ka-band BPF exhibits a low insertion loss and a high return loss, which shows that a



▲ Fig. 3 Microphotograph of the Ka-band bandpass filter fabricated on an Al_2O_3 substrate.



▲ Fig. 4 Measured and simulated S_{11} of the bandpass filter.



▲ Fig. 5 Measured and simulated S_{21} of the bandpass filter.



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CPW structure with copper metallization on an Al_2O_3 substrate should be adopted for MMIC applications. ■

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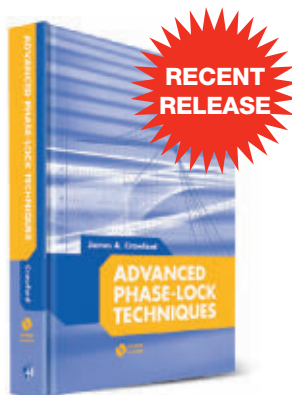
department of Vanung University. His current research is on microwave and millimeter-wave integrated circuits.

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Yi-Feng Lin received his MS degree in electronic engineering from Chang Gung University, Tao Yuan, ROC, in 2007. He is now a technology research engineer at Cyntec Corp., Hsinchu. His research interests include RFIC design and measurements and microwave passive devices.

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This paper presents a new compact and comprehensive design methodology for RF CMOS source degenerated cascode dual functionality low noise amplifier (LNA) and power amplifier (PA) for the IEEE 802.15.4 standard (commercially known as ZigBee). Due to the need to meet the far apart performance requirements of both the LNA and the PA, the proposed design methodology is based on simultaneous graphical visualization of the relationship between all relevant performance parameters and the corresponding design parameters. To demonstrate the effectiveness of the proposed methodology, a design example is presented. The simulated performance of the designed amplifier at 2.4 GHz satisfies both the requirements of the ZigBee LNA and PA with noise figure (NF) of 1.6 dB, input third-order intercept point (IIP3) of 6 dBm and a 1 dB compression point (P1dB) of -3.5 dBm. At the high input power of 0 dBm,

the amplifier achieves 24 percent power added efficiency (PAE) with 8 dB gain and 22 mW power consumption.

INTRODUCTION

Over the years, the design of low noise amplifiers in CMOS technology has attracted the attention of many researchers. This is attributed to the rapidly improving CMOS technology as a result of transistor scaling. In designing a LNA the following should be considered: Power gain, noise figure, impedance matching, reverse isolation, stability, distortion and power

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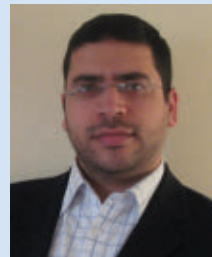
consumption. On the other hand, the design of the power amplifier is the most challenging task in a wireless communication transceiver. This is attributed to the trade-offs between the DC power supply voltage, output power, power efficiency and linearity. In designing a PA the following should be considered: High transmitted power, low power consumption, power added efficiency (PAE) nonlinear amplifier characteristics and design parameters, like third-order input intercept point (IIP3), carrier-to-intermodulation ratio (C/I), the input 1 dB gain compression point (P1dB) and adjacent channel power ratio (ACPR). Therefore, the LNA and PA designers are in front of a difficult trade-off among the competing goals of high performance in both amplifiers. In modern wireless communication systems, these two amplifiers are designed separately. No attempt has been reported, so far, for combining the two amplifiers in one.

In the IEEE 802.15.4 (ZigBee) standard, since the output power requirement is relatively modest, it is possible to consider the design of a single amplifier block that can act as a LNA in the receiver chain and a PA on the transmitter side. This would reduce the power consumption, chip area and size leading to cost savings of the transceiver that is vital to the widespread utilization of the ZigBee standard. However, since the achievable performances of the LNA and the PA are mainly limited by the CMOS transistors' parameters and operating conditions, the selection and implementation of a design methodology, leading to the solution of several design problems, is the crucial point in the design of such a dual functionality LNA/PA.

This article presents a new design methodology for a dual functionality LNA/PA. The proposed design methodology is based on simultaneous 3D graphical visualization of the relationship between all relevant performance parameters and corresponding design parameters. In this regard, it is intended to generate and provide a set of design graphs that can be used by the designer. A design example is then presented to demonstrate the effectiveness of the proposed methodology and the quality of trade-offs it allows the designer to make.

To read this article in its entirety, please visit the online version of the June issue at www.mwjournal.com. ■

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Dr. Ali Muhammad Abuelma'atti, Device Modeling Engineer at RFMD (UK), talks about the design and optimization of low power, low noise and power amplifiers.



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NETWORK ANALYSIS DUO OFFERS EXTENDED FEATURES

The R&S ZVA24 network analyzer and the new R&S ZVAX24 extension unit combine to form a solution that adapts to user requirements. This combination facilitates faster and easier measurements on active components because it does not require any additional equipment or rewiring. Depending on the application, the extension unit can be equipped with combiners, harmonic filters, pulse modulators and power couplers. It is a scalable and compact test and measurement solution. Although the R&S ZVAX24 has been tailored to the R&S ZVA24, it can also be used with all other network analyzers of Rohde & Schwarz' R&S ZVA and R&S ZVT families.

PLUG IN AND MEASURE

The combination of a network analyzer and the R&S ZVAX24 extension unit is suitable for use in the development and production of active components. This powerful and modular test solution especially benefits developers and manufacturers of amplifiers for mobile phones and base stations as well as of components for the automotive sector, e.g. car radar.

It facilitates complex measurements and can be used for measurements to satisfy aerospace

and defense requirements or for tests on antennas or amplifiers under pulsed conditions. The R&S ZVAX24 occupies only two height units in a 19-inch rack and can be easily placed underneath the R&S ZVA. Semi-rigid cables connect the instruments so that they constitute a single unit.

The extension unit and the components it contains are basically looped into the generator or receiver path by using the direct generator/receiver access. Only a USB cable (for path switching) and an LVDS (LAN) cable (for controlling the pulse modulators) are required as control lines. The unit is operated from the R&S ZVA network analyzer using a block diagram, shown in **Figure 1**, and dialog windows.

Depending on the measurement task, the required RF components such as combiners, pulse modulators or harmonic filters can be switched into the measurement path. The T&M solution's high level of integration means that both present and future functions of the R&S ZVA can be used to perform complex lin-

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ear and nonlinear measurements, in particular on active components (intermodulation measurements, pulse profile measurements, etc.).

INTERMODULATION MEASUREMENTS

Intermodulation products are unwanted spectral components that are caused by nonlinear circuit elements and a two-tone signal is required to measure them. If a conventional network analyzer with only one internal generator is used, an external generator and a combiner must be added to the test setup. This is not necessary with the R&S ZVA and R&S ZVAX24 combination because the internal combiner of the extension unit uses the two sources of the four-port network analyzer and generates a two-tone signal for intermodulation measurements. **Figure 2** shows a typical intermodulation output signal from the Rohde & Schwarz solution in blue and from a conventional one in yellow.

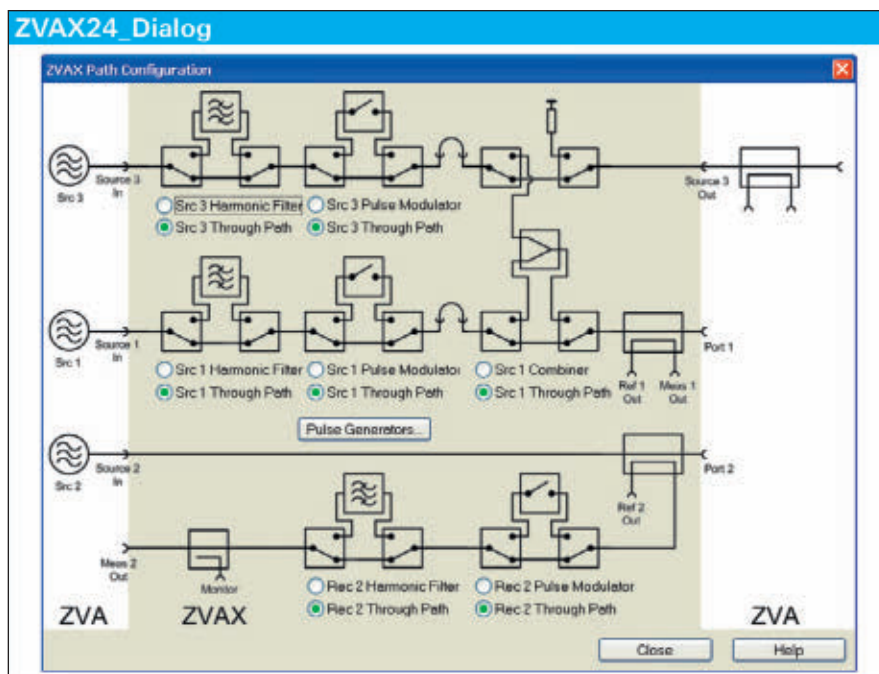
This signal is directly output on one of the four ports. This feature plus the intermodulation wizard make it very easy and convenient to measure the intermodulation parameters of amplifiers or mixers as a function of frequency and power. The combiner can also be used to measure the group delay of mixers without LO access.

PULSE MODULATORS

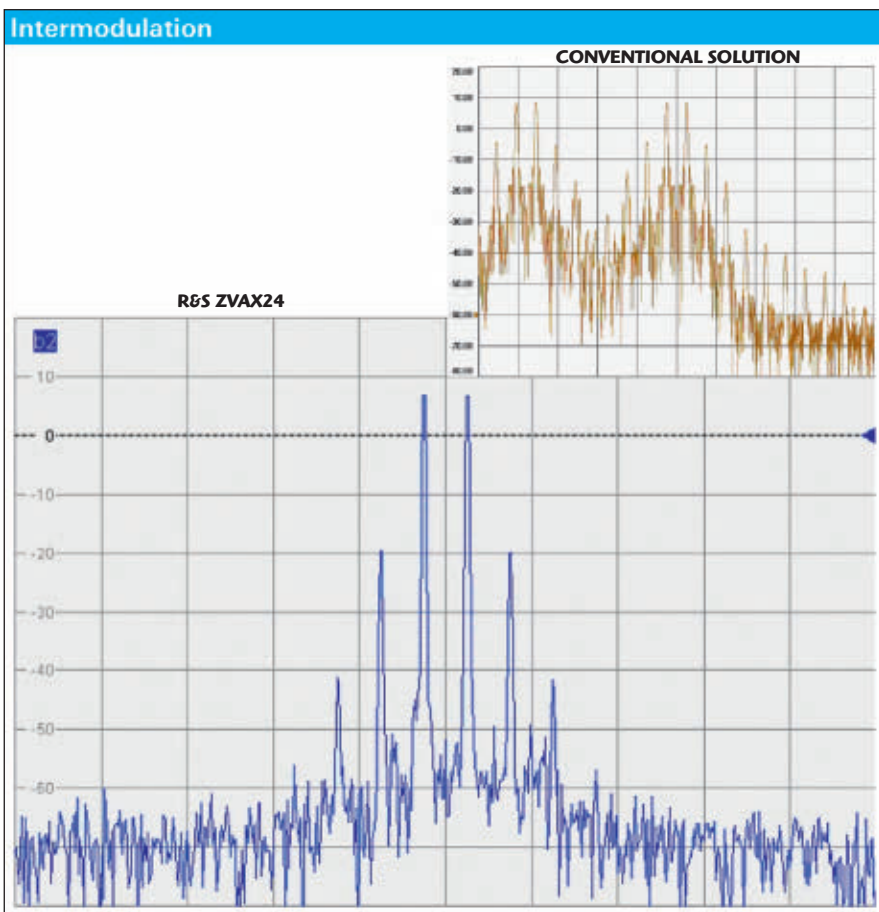
Many applications require that DUTs be characterized by using pulsed signals instead of CW signals. The pulse width for these applications typically varies between a few hundred nanoseconds and the upper microsecond range. To be able to characterize the pulse profile distortion of components, the network analyzer must have a time resolution that is considerably higher than the pulse duration.

For applications where the DUT requires a pulse-modulated input signal, either a pulse modulator or a generator with pulse modulation can be used. Since the R&S ZVA-B16 hardware option enables direct access to the network analyzer generator path, the pulse-modulated RF signal (instead of the unmodulated signal) is directly fed to the network analyzer test set.

The pulse modulators of the R&S ZVAX24 offer even more measure-



▲ Fig. 1 Easy and convenient control of the R&S ZVAX24 extension unit using the graphical user interface of the R&S ZVA.



▲ Fig. 2 Comparison of intermodulation signals: R&S ZVAX24 (blue curve) and conventional solution (yellow curve).

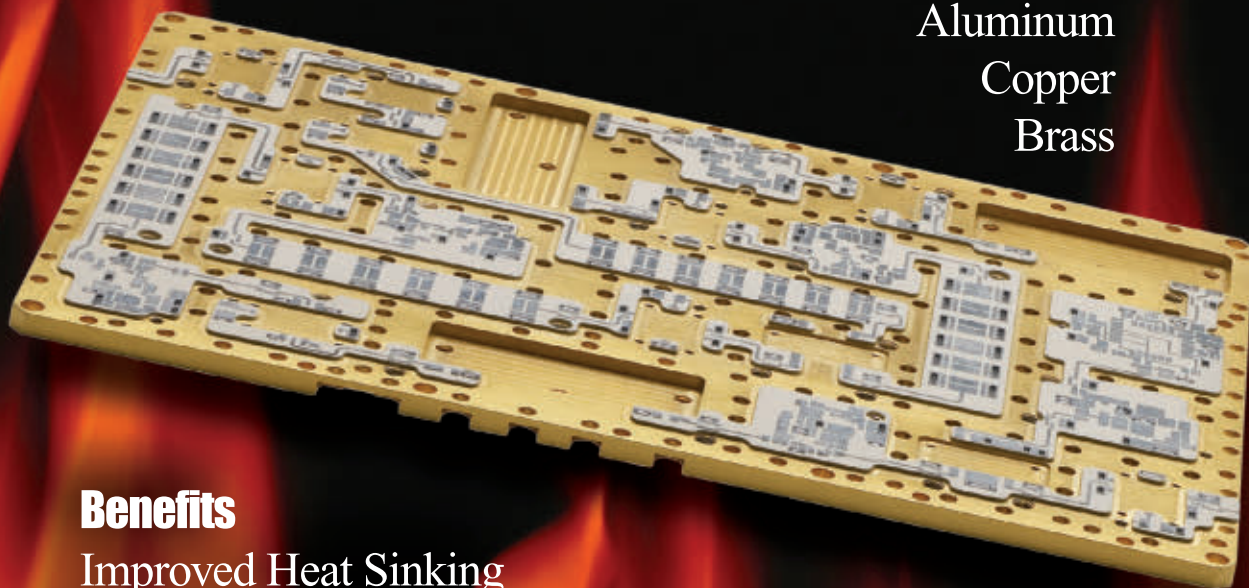
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RF Power Amplifier

A801M302-5353R

Frequency: 800M-3000MHz
Power: 200W and more.....

Model	Frequency	P@1dB (min)
A101K102-4141M/R	100k-1000MHz	+41dBm
A001M102-4141M/R	1M-1000MHz	+41dBm
A001M102-4343M/R	1M-1000MHz	+43dBm
A001M102-4747M/R	1M-1000MHz	+47dBm
A001M102-5050M/R	1M-1000MHz	+50dBm
A020M102-5353M/R	20M-1000MHz	+53dBm
A080M102-5757 R	80M-1000MHz	+57dBm
A080M102-6060 R	80M-1000MHz	+60dBm
A201M102-6363 R	200M-1000MHz	+63dBm
A501M272-3737M/R	500M-2700MHz	+37dBm
A501M272-4040M/R	500M-2700MHz	+40dBm
A501M272-4343M/R	500M-2700MHz	+43dBm
A501M272-4747M/R	500M-2700MHz	+47dBm
A501M272-5050 R	500M-2700MHz	+50dBm
A801M202-3737M/R	800M-2000MHz	+37dBm
A801M202-4040M/R	800M-2000MHz	+40dBm
A801M202-4343M/R	800M-2000MHz	+43dBm
A801M202-4747M/R	800M-2000MHz	+47dBm
A801M202-5050 R	800M-2000MHz	+50dBm
A801M202-5353 R	800M-2000MHz	+53dBm
A801M202-5757 R	800M-2000MHz	+57dBm
A801M202-6060 R	800M-2000MHz	+60dBm
A801M252-3737M/R	800M-2500MHz	+37dBm
A801M252-4040M/R	800M-2500MHz	+40dBm
A801M252-4343M/R	800M-2500MHz	+43dBm
A801M252-4747M/R	800M-2500MHz	+47dBm
A801M252-5050 R	800M-2500MHz	+50dBm
A801M252-5353 R	800M-2500MHz	+53dBm
A801M252-5757 R	800M-2500MHz	+57dBm
A801M252-6060 R	800M-2500MHz	+60dBm
A801M302-3737M/R	800M-3000MHz	+37dBm
A801M302-4040M/R	800M-3000MHz	+40dBm
A801M302-4343M/R	800M-3000MHz	+43dBm
A801M302-4747M/R	800M-3000MHz	+47dBm
A801M302-5050 R	800M-3000MHz	+50dBm
A801M302-5353 R	800M-3000MHz	+53dBm

* M-Module type, R-Rack type

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Pulse-Generator-Menu

The screenshot displays the 'Pulse-Generator-Menu' software interface. It consists of three main windows:

- Define Pulse Train:** This window allows users to define a sequence of pulses. It features a table with columns for '# Active', 'Start High Signal', and 'Stop High Signal'. The table contains six rows of data, including pulse widths (e.g., 0 s, 12.5 ns, 50 ns, 112.5 ns, 200 ns, 212.5 ns, 500 ns) and segment durations (e.g., 12.5 ns, 50 ns, 112.5 ns, 200 ns, 212.5 ns, 500 ns). Buttons for 'Recall Pulse Train...', 'Save Pulse Train...', 'Add Segment', 'Delete Segment', 'Del All Segments', 'Auto Arrange', 'Close', and 'Help' are present.
- Define Pulse Generator:** This window allows users to define the parameters of a single pulse or a pulse train. It includes options for 'Pulse Type' (Single Pulse, Pulse Train, Constant High, Constant Low), 'Pulse Parameters' (Pulse Width, Single Pulse Period, Pulse Train Period), and 'Settings valid for' (Active Channel, All Channels (Continuous Mode)). Buttons for 'Define Pulse Train...', 'Define Sync Generator...', 'Chopped Pulse Profile...', 'Close', and 'Help' are included.
- Chopped Pulse Profile:** This window allows users to define the profile of a chopped pulse. It includes a 'Time Resolution' field (set to 12.5 ns) and a section for 'The following settings will be adjusted automatically: Sweep Type, Number of Points, IF Bandwidth, Sync Width, Single Pulse Period (or Pulse Train Period)'. Buttons for 'Activate', 'Off', 'Chopped Pulse Profile is active', 'Close', and 'Help' are present.

▲ Fig. 3 The R&S ZVA-K27 option offers two independent, integrated pulse trigger generators in the R&S ZVA that deliver single pulses and user-configurable pulse trains.

ment convenience. They are configured and controlled via the graphical user interface of the network analyzer, shown in **Figure 3**, so that no additional switches or trigger generators are required. For measurements with pulsed signals, the extension unit contains two modulators for pulse generation (see Figure 1). Single pulses, periodic pulses or variable pulse trains can be generated.

The R&S ZVA-K7 pulsed measurements option with easy setup enables direct recording of amplitude and phase versus time. This functionality makes it possible to analyze the time-dependent behavior in T/R modules, amplifiers and mixers with a resolution of 12.5 ns. This high resolution, ten times higher than any solution currently available on the market, enables a more accurate characterization of short pulses. At a maximum IF bandwidth of 30 MHz, the signal rise/fall time can be determined with a resolution of up to 33 ns.

Since the pulse generators support user-configurable pulse trains (see Figure 3), the user can generate arbitrary sequences of any width, duration and power, and also characterize components under real-world conditions. Significantly, this measurement does not require a repetitive signal because the user can work with any pulse trains.

The high dynamic range and measurement speed of the new solution are complemented by an easy test setup and straightforward operation. In addition to typical measurements such as high-PRF-mode or point-in-pulse measurements, the R&S ZVA-K7 option offers a very convenient pulse profile measurement facility.

A third modulator in the receiver path, shown in Figure 1, 'chops' the pulses. This can be useful in antenna measurements (e.g. in the case of pulsed radar cross-section [RCS] measurements), for example, because time gating allows direct crosstalk be-

RF Power Amplifier

A010K401-5353R

Frequency: 10k-400MHz
Power: 200W and more.....

Model	Frequency	P@1dB (min)
A001K101-4444M/R	1k-100MHz	+44dBm
A010K251-4444M/R	10k-250MHz	+44dBm
A010K401-4444M/R	10k-400MHz	+44dBm
A001K101-4747M/R	1k-100MHz	+47dBm
A010K251-4747M/R	10k-250MHz	+47dBm
A010K401-4646M/R	10k-400MHz	+46dBm
A001K101-4949M/R	1k-100MHz	+49dBm
A010K251-4949M/R	10k-250MHz	+49dBm
A010K401-4848M/R	10k-400MHz	+48dBm
A001K101-5353M/R	1k-100MHz	+53dBm
A010K251-5353M/R	10k-250MHz	+53dBm
A010K401-5353M/R	10k-400MHz	+53dBm
A010K101-5757 R	10k-100MHz	+57dBm
A101K251-5757 R	100k-250MHz	+57dBm
A010K101-6060 R	10k-100MHz	+60dBm
A101K251-6060 R	100k-250MHz	+60dBm
A101K080-6363 R	100k- 80MHz	+63dBm
A101K251-6363 R	100k-250MHz	+63dBm
A101K080-6767 R	100k- 80MHz	+67dBm
A101K251-6767 R	100k-250MHz	+67dBm
A101K080-7070 R	100k- 80MHz	+70dBm
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* M-Module type, R-Rack type

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tween transmit and receive antennas with short delay and high amplitude. Pulse profile measurements can be implemented very easily by using the conventional high-PRF-mode.

The pulse modulators of the R&S ZVAX24 can be controlled either via an external trigger generator or directly by the R&S ZVA24 using the new R&S ZVA-K27 internal pulse generator option. The trigger signals are fed in via BNC connectors (if an external trigger generator is used) or via an RJ-45 cable (if the internal R&S ZVA pulse generators are used).

GROUP DELAY MEASUREMENTS

Mixers and frequency converters form the core of wireless and satellite communications systems. Especially in satellite systems, these frequency converters have to satisfy ever more demanding requirements regarding frequency response and phase linearity. Therefore, the measurement of relative and absolute group delay, of relative phase and of the group de-

lay derivations (dispersion and scattering) in T/R modules is playing an increasingly important role.

Since there is no access to the local oscillator (LO), Rohde & Schwarz has developed the R&S ZVA-K9 option as a new method for characterizing the group delay and derived parameters without exactly knowing the LO signal. This option makes it possible to determine absolute and relative group delay, relative phase and scattering (group delay derivations).

This innovative method requires a four-port network analyzer with two sources for feeding a two-tone signal to the converter. The R&S ZVA24 measures the phase deviation between the two signals at the input and at the output of the DUT and determines the group delay. Neither the frequency drift nor the frequency modulation of the internal and unknown LO influences the measurement results. The R&S ZVA-K9 calculates the relative phase by integrating the group delay, and it calculates the DUT scattering by group delay derivation.

The conventional methods for determining group delay require a complicated test setup and a calibration. They are also associated with a significant level of uncertainty because they depend on the stability of the LO. Moreover, it is almost impossible to perform group delay measurements on converters having multiple mixer stages. This new approach, however, offers easy setup and calibration, and is independent of the LO's frequency stability. This method is ideal for investigating DUTs with multiple mixer stages.

HARMONIC AND INTERFERENCE TEST FILTERS

Two harmonic filters in the generator paths, shown in the block diagram of Figure 1, improve the spectral purity of the signals. Harmonic suppression is typically 60 dBc for the second and 70 dBc for the third harmonic. An additional filter in the receive path (see Figure 1) expands the receiver's dynamic range at test port 2, which is a crucial advantage when measuring harmonics or in-

terference signals. The filter also allows very low harmonic levels to be measured. Harmonic measurements are carried out using the R&S ZVA-K4 option.

COUPLERS

The R&S ZVAX24 can also be equipped with two high-power couplers, shown in Figure 1, to cover power levels up to 43 dBm (standard test port: 27 dBm). Preamplifiers can be inserted into the source path using connectors on the unit's rear panel in order to further increase the available power levels. A coupler in the measurement path allows the signals of port 2 to be monitored in parallel using a spectrum analyzer or power meter. Signal monitoring is a very helpful feature for complementary measurements or when controlling signals during S-parameter or intermodulation measurements. All these features enable the user to measure DUTs without reconnecting them.

CONCLUSION

The scalable T&M solution that consists of the R&S ZVAX24 extension unit and the R&S ZVA24 vector network analyzer (or any other R&S ZVA or ZVT network analyzer) enables linear and nonlinear measurements on active components without extra equipment and without reconnecting the DUT. This is a big step toward higher efficiency and measurement accuracy. Depending on the measurement task to be solved, users can customize a powerful test solution by adding combiners, harmonic filters, pulse modulators and high-power couplers in line with their needs.

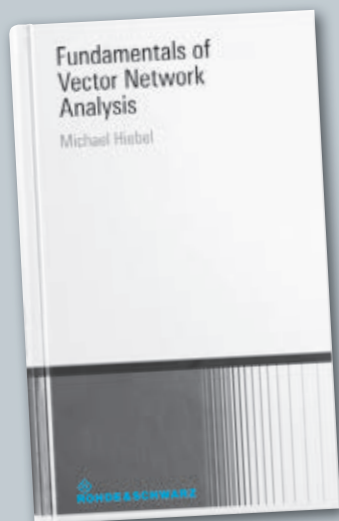
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Wireless communications has revolutionized the way our society functions. It is a key element of modern life and its reach is extending far and wide, with new applications constantly coming to the fore. To address the increasing demand to connect the various types of devices and networks, HUBER+SUHNER has developed the new SENCITY® SWA-0825/360/5/30/DFRX30 antenna, which is a rugged omni-directional multiband antenna for GSM 900, GSM 1800, GSM 1900, UMTS, 2.4 GHz band and GPS/Galileo, aimed specifically at industrial and transportation applications.

The need for and proliferation of antennas in the transportation and industrial sectors is increasing rapidly. For instance, a modern car is equipped with numerous antennas for different tasks: mobile communication, GPS navigation, Bluetooth connection between the mobile phone to the radio, the car key, etc. Also, more and more antennas are being used in industrial applications such as industrial automation, sen-

sor data transfer, heavy vehicles like mine trucks, fork lifts, wind turbines, trains and ships.

In car applications the focus is primarily on short-range communication and the need for antennas to be as small and as cheap as possible, whereas in the industrial sector the need is for high reliability, protection against vandalism, high electrical performance (gain, VSWR) and the need to resist the impact of vibration, water, salt, dust and chemicals.

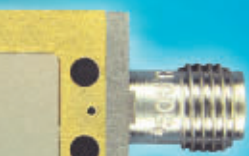
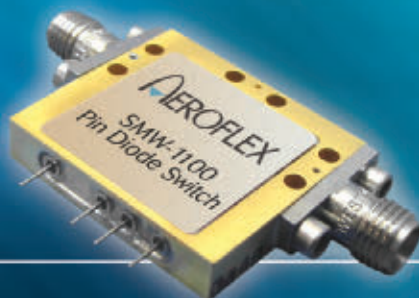
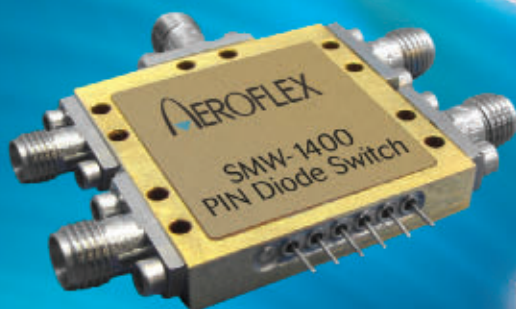
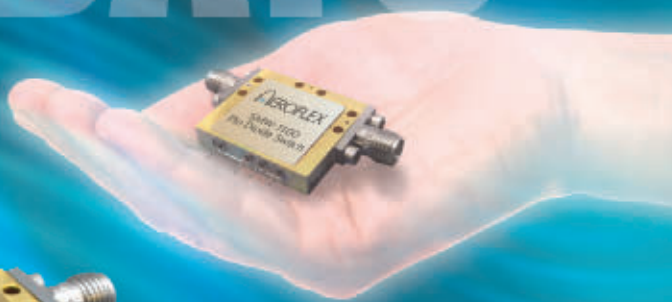
Antennas are used for mobile communication, WiFi, ZigBee/Bluetooth, WiMAX or RFID applications. There is a large variety of existing products that focus on the car industry and these products have been used in the industrial environment as well. However, there are often issues with both electrical performance and mechanical stability.

HUBER+SUHNER AG
Herisau, Switzerland

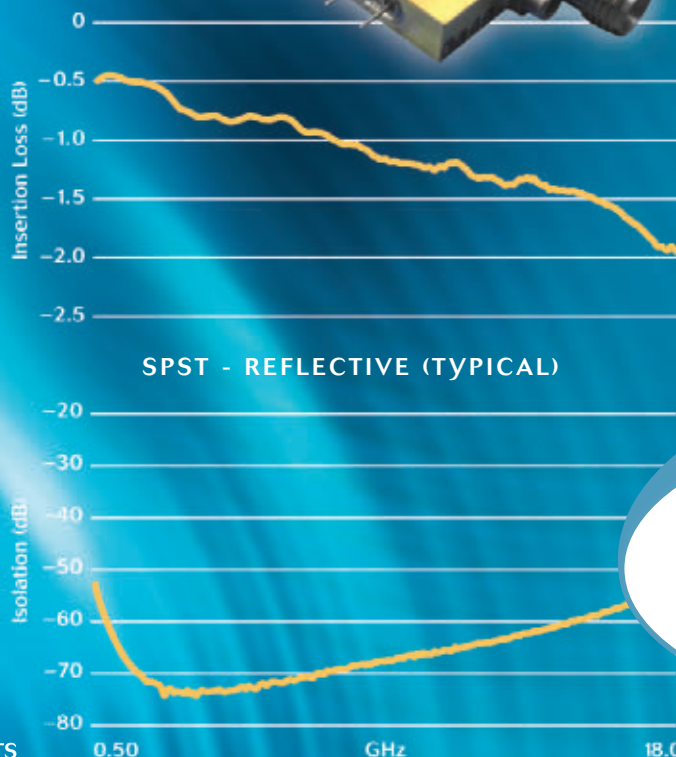
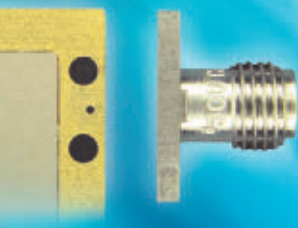
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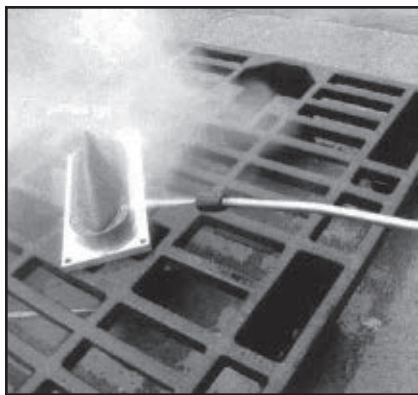
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▲ Fig. 1 Water testing of SENCITY antenna.



▲ Fig. 2 Effect of galvanic corrosion.

are often hosed down with a high-pressure cleaning device. This is the case when cleaning the roofs of trains. Thus, the higher IP rating of the SENCITY SWA-0825/360/5/30/DFRX30 antenna is significant. **Figure 1** shows an antenna being water tested.

The antenna is also protected against high voltage impacts. This could be a lightning strike or, for trains, contact with the catenary line that can carry up to 28 kV. In fact, for the roof-top application of antennas on trains there has to be protection in case of a contact with the catenary line (UIC Code 533). If the catenary line breaks, it could damage the radome of the antenna and detach the metallic radiator and the high voltage could create a fire inside the vehicle.

Another serious consideration when designing the new antenna was galvanic corrosion, which often reduces the lifetime of an installed product in an outdoor environment. **Figure 2** shows the effect of galvanic corrosion. Choosing the right material mix helps to reduce the corrosion effect. Thus, the SENCITY SWA-0825/360/5/30/DFRX30 antenna has been developed following the MIL-F-14072A (EL) standard with regards to surface combinations.

Other design considerations were fire and rain (and hail). With regards to the antenna's behavior in a fire, the design goal was to limit any toxic materials and to reduce the flammability of the product (NF F101-16, DIN 5510 or BS 6853). Also, trains running at up to 400 km/h or antennas on industrial vehicles will not stop running in bad weather, so the SENCITY antenna has passed tests against hail and rain.

ACCESSORIES

Cables, connectors, filters and the radio unit also have to meet



▲ Fig. 3 The selection of the cable assembly for the antenna is critical.

strict requirements. As a specialist for connector solutions, HUBER+SUHNER provides a particular solution for the contact between connector and radiator. It avoids completely the soldering process to guarantee optimal breakout.

The selection of the cable assembly (shown in **Figure 3**) is also significant. Usually, the cable will be selected by the parameters related to loss and bending radius. Additionally, in the industrial and transportation environment, the shock and vibration requirements need to be considered. H+S offers EN 50155 railway approved diplexer products to split mobile applications from WiFi or WiMAX frequencies. Also, the integrated GPS antenna is protected by the mechanical design of the broadband radiator antenna.

CONCLUSION

Antennas in industrial and transportation applications are special products that have to meet tough requirements and the electrical performance and mechanical performance can be more important than price. For the SENCITY SWA-0825/360/5/30/DFRX30 antenna the design goal is to ensure high reliability and to cope with different installation scenarios. The product has been designed to withstand vandalism, corrosion, UV radiation, temperature drops, vibration, hail impact, rain, snow and cleaning over a long period without maintenance.

HUBER+SUHNER AG, Herisau, Switzerland, +41 71 353 41 11, www.hubersuhner.com.

ANTENNA SPECIFICATIONS

The SENCITY® SWA-0825/360/5/30/DFRX30 antenna addresses these issues. It measures 145 by 100 by 40 mm and can operate in a temperature range of -40° to +85°C. In multiband its frequency ranges are 870 to 960 MHz, 1710 to 2170 MHz and 2400 to 2500 MHz. Impedance is 50 Ω and VSWR is 1.7. Polarization is linear, vertical and the maximum power is 100 W (CW) at 50°C.

In GPS/Galileo the frequency range is 1575.42 MHz \pm 1.023 MHz, impedance is 50 Ω and VSWR is 1.6. The operating voltage is 3.0 to 5.0 VDC feed at the center conductor of the GPS antenna. Polarization is RHCP, gain LNA is 27 dB and the noise figure is 1 dB.

The antenna is 2002/95/EC (RoHS) compliant and also meets: IP68 (when correctly installed) EN50155, high current protection according to DB specifications (protection against short circuit of 40 kA) and electromagnetic compatibility (EN50121-3-2) standards.

These standards are particularly significant for industrial and transportation applications. It is important to put them into context for antennas operating outdoors and in harsh environments. A high level of salt in the air can cause corrosion of the product. It may be subject to shock and vibration and needs to be resistant to water and dust ingress, all of which are covered by EN 50155.

IP RATINGS

Most products meet an IP65 or even IP66 level, but vehicles

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Output Power	+9 dBm (Min.)	
Spurious Suppression	60 dB (Typ.)	
Harmonic Suppression	15 dB (Typ.)	
Typical Phase Noise	Offset	dBc/Hz.
	1 kHz	-93
	10 kHz	-96
	100 kHz	-110
Settling Time	Within 1 kHz	<22 mSec
	Within 10 Hz	<36 mSec
Operating Temperature Range	-20 to +70 °C	

MTS2500-200400-10

Output Frequency	2000 - 4000 MHz	
Bandwidth	2000 MHz	
External Reference	10 MHz	
Step Size	Programmable to 1 Hz	
Bias Voltage	+5 / +3.3 V	
Output Power	+5.5 dBm (Min.)	
Spurious Suppression	60 dB (Typ.)	
Harmonic Suppression	10 dB (Typ.)	
Typical Phase Noise	Offset	dBc/Hz.
	1 kHz	-88
	10 kHz	-87
	100 kHz	-100
Settling Time	Within 1 kHz	<10 mSec
	Within 10 Hz	<20 mSec
Operating Temperature Range	-20 to +70 °C	

MTS2500-300600-10

Output Frequency	3000 - 6000 MHz	
Bandwidth	3000 MHz	
External Reference	10 MHz	
Step Size	Programmable to 1 Hz	
Bias Voltage	+5 / +3.3 V	
Output Power	+2 dBm (Min.)	
Spurious Suppression	60 dB (Typ.)	
Harmonic Suppression	20 dB (Typ.)	
Typical Phase Noise	Offset	dBc/Hz.
	1 kHz	-87
	10 kHz	-83
	100 kHz	-108
Settling Time	Within 1 kHz	<6 mSec
	Within 10 Hz	<12 mSec
Operating Temperature Range	-20 to +70 °C	

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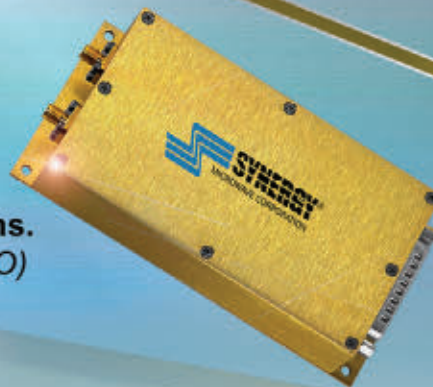
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RF/Microwave Products

VENDORVIEW

Anatech Electronics announced it has launched three new websites that allow RF and microwave designers to more easily select from its families of RF and microwave filters and other components, and to order many products online. Anatech Microwave (AMC) (www.anatechmicrowave.com) covers the company's standard products. Anatech Electronics (AEI) (www.anatechelectronics.com) covers the company's custom products. AMCrF (www.amcrf.com) is an e-commerce site that features specific standard products that can be ordered online.

Anatech Electronics Inc.,
70 Outwater Lane, Garfield, NJ 07026

www.amcrf.com



AR's Bargain Corner

VENDORVIEW

There is more than one way to get the quality equipment you need. If your budget is tight, the AR Bargain Corner is a good place to find some great values. Discontinued and demonstration equipment is available at a fraction of its original price. Visit AR's website to view the company's Bargain Corner.

AR RF/Microwave Instrumentation,
160 School House Road,
Souderton, PA 18964

www.ar-worldwide.com



RF Coaxial Cable Assemblies

VENDORVIEW

The website features an easy-to-use product selector, broken down by cable type. Each cable type is available in a wide range of standard and custom lengths with a variety of connector choices. All connector/cable combinations can be reviewed using the company's Fast Quote tool, which also appears on each product page. The tool allows users to virtually design their own cable assemblies, with the ability to specify the cable type, length, connectors on both ends, and test requirements.

Electronic Assembly Manufacturing Inc.,
126 Merrimack Street,
Methuen, MA 01844

www.eamcableassemblies.com



ICs, Modules, Subsystems & Instrumentation

VENDORVIEW

Hittite's redesigned website includes crisp webpage designs and a dynamic homepage featuring full specifications for over 740 products across 20 product lines, press releases and featured articles. Comprehensive individual product "Splash Pages" containing in-depth product information and technical content are located on one easy to navigate page. Engineers will find improved Product Support and streamlined Quality & Reliability pages containing invaluable reference materials.

Hittite Microwave Corp.,
20 Alpha Road, Chelmsford, MA 01824

www.hittite.com



Filtering Solutions

K&L Microwave's redesigned website features improved product navigation and an integrated quote cart that enhances the customer's ability to review available products, simplify identification and specification of custom design solutions, and speed direct communication with the factory. Also, the new product catalog is available to download. The entire catalog or specific sections of interest can be downloaded by using provided links.

K&L Microwave,
2250 Northwood Drive,
Salisbury, MD 21801

www.klmicrowave.com
www.klfilterwizard.com



Component and Connectivity Products

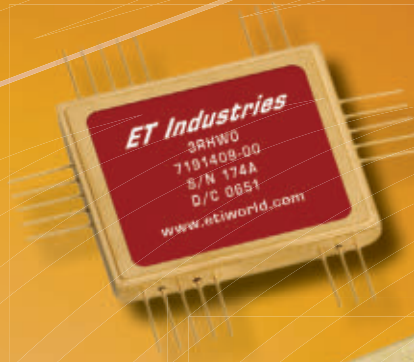
VENDORVIEW

Response Microwave Inc. announced the launch of its new website selection guide. The new site has migrated to a products focus and provides an overview of corporate capabilities and selection tables of the company's passive component and connectivity product offering that covers DC to 60 GHz. The site also offers application notes on the company's HYBRIDLINE series of drop-in quad hybrids and couplers.

Response Microwave Inc.,
94 Jackson Road, Suite 110,
Devens, MA 01844

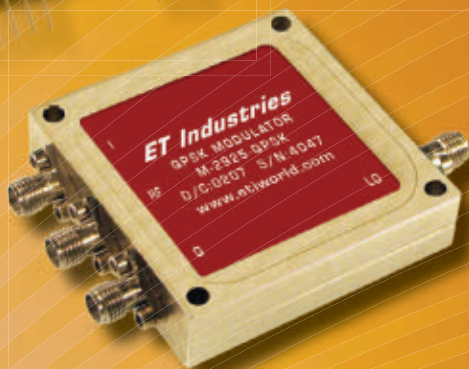
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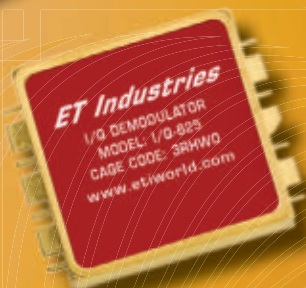
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email: sales@etiworld.com website: www.ETIworld.com

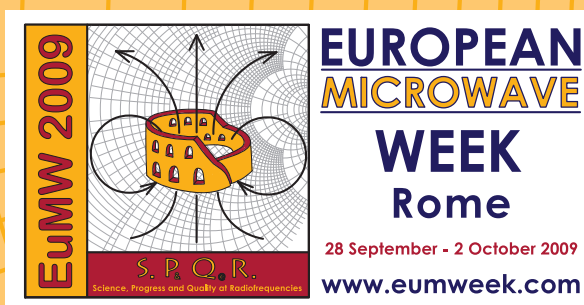
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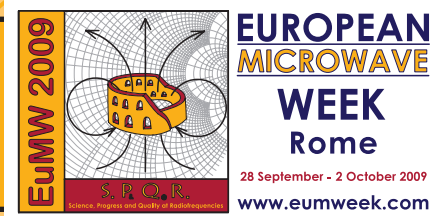
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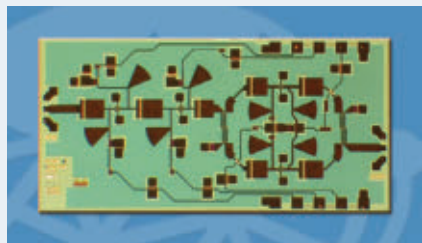
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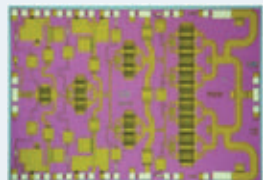


The HMC-ALH508 is a three-stage GaAs HEMT MMIC low noise amplifier (LNA) chip that operates between 71 and 86 GHz, replacing the HMC-ALH459. The HMC-ALH508 features 13 dB of small-signal gain, 4.5 dB of noise figure and an output power of +7 dBm at 1 dB compression. The HMC-ALH508 operates from two supply voltages at 2.1 and 2.4 V respectively, while consuming only 30 mA of supply current. All bond pads and the die backside are Ti/Au metallized and the amplifier is fully passivated for reliable operation. This versatile LNA is compatible with conventional die attach methods, as well as thermocompression and thermosonic wire bonding, making it ideal for MCM and hybrid microcircuit applications.

Hittite Microwave Corp.,
Chelmsford, MA (978) 250-3343,
www.hittite.com.

RS No. 217

MMIC High Power Amplifier



This GaAs MMIC high power amplifier (HPA) features +37 dBm saturated output power and 27 dB small-signal

gain. This HPA, identified as XP1058-BD, uses a dual-sided bias architecture, covers 14.5 to 16 GHz, and achieves +44 dBm OIP3. The device is well suited for millimeter-wave military, radar, satellite and weather applications.

Mimix Broadband Inc.,
Houston, TX (281) 988-4600,
www.mimixbroadband.com.

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NEC Electronics (Europe) GmbH,
Düsseldorf, Germany +49 (0) 211 65 03 0,
www.eu.necel.com.

RS No. 218

Two-way Power Dividers



These ten new low cost SMD type two-way divider/splitter/combiners are designed for LTE and WiMAX frequencies. It is now proposed to have 2.6 GHz for Europe, 1800 to 2000 MHz for China, and 700 MHz for US LTE bands. PD09C2 (700 to 960 MHz), PD18C2 (1.7 to 1.9 GHz), PD20C2 (1.9 to 2.2 GHz), PD23C2 (2.2 to 2.4 GHz), and PD26C2 (2.5 to 2.7 GHz) has been released in an industry standard SOIC-8 type plastic package and is lead-free/RoHS compliant. All these devices will be available with SOT-23-6L package, which has the same footprint with SOT-6 and SOT-26. Cost advantage is increasingly becoming an important strategic advantage and this low cost divider can be the correct solution for many infrastructure telecommunication equipment manufacturers.

RFHIC Corp.,
Suwon, GyeongGi-do Korea 82-31-250-5011,
www.rfhic.com.

RS No. 231

Integrated Configurable Components



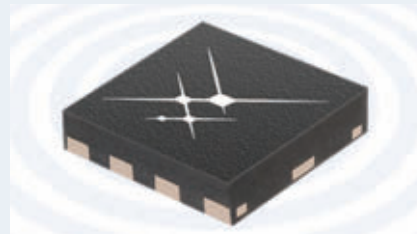
RFMD has extended its portfolio of integrated configurable components to include products for the cellular repeater and Wireless Local Area Network (WLAN) markets. The new integrated configurable components include the RF2057 RF synthesizer with integrated mixers and the RF2059 RF transverter. RFMD's integrated configurable components deliver unmatched levels of flexibility and functional integration to designers of radio systems. By integrating multiple common RF functions into highly integrated, size-reduced packages, the integrated configurable components enable designers to develop radio systems that operate

over a wide dynamic range and across a broad range of frequencies and channel bandwidths. The RF2057 and RF2059 join the RF2051, RF2052 and RF2053, which were introduced in April 2008 and have been adopted in markets as diverse as cellular, defense and broadband cable systems.

RFMD, Greensboro, NC
(336) 664-1233, www.rfmd.com.

RS No. 256

PHEMT GaAs IC SP3T Switch



This pseudomorphic high electron mobility transistor (PHEMT) gallium arsenide (GaAs) integrated circuit (IC) SP3T switch is designed for 0.1 to 6 GHz. The SKY13317-373LF symmetric switch offers low insertion loss and high isolation with a 44 percent reduction in size than SKY13309-370LF. Featuring higher overall transmit efficiency and linearity, less board space is used with greater design/layout flexibility, equating to a small and thin end product. Appropriate for high volume, consumer products — end users will also discover better linearity and a clearer signal. The SKY13317-373LF is currently being used with wireless local area network (WLAN) and Bluetooth® combo chipsets.

Skyworks Solutions Inc.,
Woburn, MA, (781) 376-3000,
www.skyworksinc.com.

RS No. 219

RF Power Transistors



HVVi Semiconductor introduces the HVV1011-500, the latest in its family of extremely rugged L-band (1030 to 1090 MHz) RF power transistors aimed at IFF, TCAS and transponder/interrogator markets. This robust 50 W device achieves output power over 500 W P1dB providing 19 dB gain and 50 percent drain efficiency under the following pulse condition (50 μ s P.W., 5 percent D.C.), while withstanding industry leading output load mismatch tolerance of 20:1 VSWR. The HVV1011-500 is a single-ended pulsed power transistor assembled in an HV800, two-lead, bolt-down, metal flanged package with LCP lid.

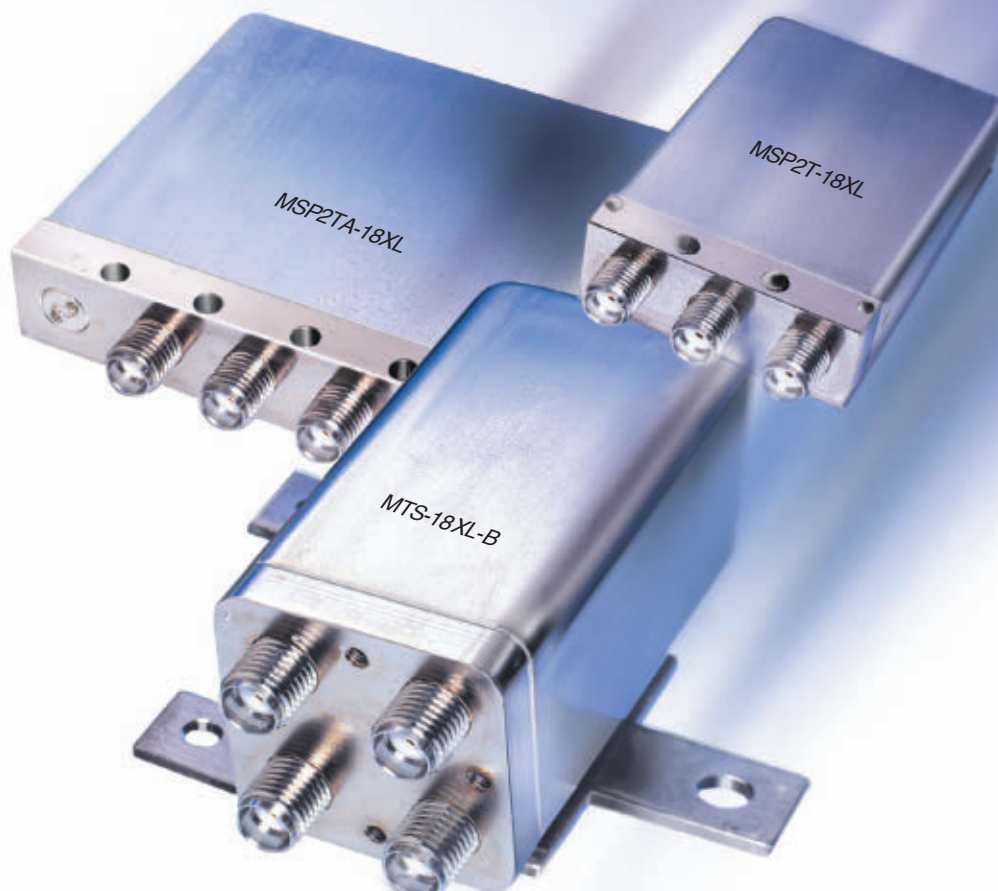
HVVi Semiconductors Inc.,
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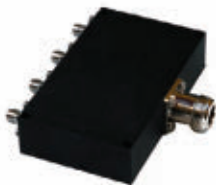
IF/RF MICROWAVE COMPONENTS

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Components

Four-way Power Divider



Model AM-900PD1196 is a four-way power divider designed for applications such as wireless and industrial scientific and medical (ISM)

that operate between 800 to 1000 MHz. The module splits an input signal into four separate outputs, and features low insertion loss and excellent amplitude and phase balance. The model AM900PD1196 operates over a frequency range of 800 to 1000 MHz, with insertion loss of 1.5 dB or less, isolation of at least 25 dB, amplitude balance of 0.3 dB or less, and phase balance of 5 deg. or less. Size: 4" x 2.15" x 1".

Anatech Microwave,
Garfield, NJ (201) 772-4242,
www.anatechmicrowave.com.

RS No. 220

E-band Components



The newly developed E-band (WR-12 waveguide band) component family enables the rapid development of short-haul communication links operating license-free from 71 to 86 GHz. The component family includes oscillators, multipliers, low noise and power amplifiers, subharmonically pumped mixers and up-converters, filters and diplexers. All products are available as separate components or combined as integrated assemblies.

Ducommun Technologies Inc.,
Carson, CA (310) 847-2859,
www.ducommun.com.

RS No. 221

Temperature Variable Chip Attenuator



The AN7 is a new solution for temperature compensation with an SMT planar style chip design. This

new AN7 offers a small 0805 package size for TPA line and has excellent frequency response from DC to 6 GHz. The AN7 is suitable for high volume, pick & place and targeted for telecom and WiMAX applications. The AN7 variable attenuator is available in designs of 1

through 6 dB in one dB increments with temperature attenuation coefficients (TCA) of -0.003 through -0.009 , dB/dB/deg C and an operating temperature range of -55° to $+125^{\circ}$ C. Size: $0.080" \times 0.050"$.

EMC Technology,
Stuart, FL (772) 286-9300,
www.emct.com.

RS No. 222

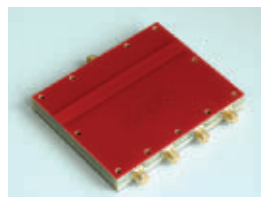
Voltage-controlled Oscillator

The RP-148258-01 model is designed to meet the stringent performance requirements of the aerospace industry. This model is compliant with MIL-PRF-38534 specification essential to high reliability, military and space applications. The operating frequency range is 1420 to 2500 MHz with an operating temperature range of -40° to $+85^{\circ}$ C. Tuning voltage is 1.85 to 12.65 V DC with 3.4 to 4.0 dBm power output. Modulation bandwidth is 5.5 MHz and typical phase noise is -96 dBc/Hz at 10 kHz.

Emhiser Research Inc.,
Verdi, NV (775) 345-0461,
www.emhiser.com.

RS No. 223

4 to 6 GHz RF Coupler



The low cost CP4060-4 four-way reactive power divider/combiner has a frequency range of 4 to 6 GHz, which has been developed

for splitting or combining four RF-signals in phase while providing isolation between the four signals. It has a maximum insertion loss of 0.9 dB (over 6 dB), isolation > 20 dB, comes in a small package measuring 85 by 70 by 10 mm and operates within the commercial ambient temperature range of 0° to $+70^{\circ}$ C. The configuration is a four-way in phase splitter/combiner with a maximum matched input power of 2 W and an impedance of 50 Ω .

eubus GmbH,
Munich, Germany +49(0) 89 4522 57811,
www.eubus.net.

RS No. 224

Solid-state Switches



The 50S-1820 and 50S-1821 are the latest innovations in JFW's high power solid-state RF switches. The 50S-1820 is capable of switching 100 W of RF power from 800 to 2700 MHz (cold switch), while the 50S-1821 will switch 75 W from 800 to 3000 MHz. Both switches boast 10 microsecond switching speeds and a minimum isolation of 55 dB. Available with SMA, N, BNC or TNC connectors.

JFW Industries,
Indianapolis, IN (317) 887-1340,
www.jfwindustries.com.

RS No. 225

808 MHz Bandpass Filter



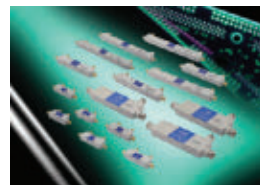
KR Electronics introduces part number 2907, a small surface-mount 808 MHz bandpass

filter. The filter has a typical insertion loss of 3 dB and minimum 3 dB bandwidth of 25 MHz (35 MHz typical). The filter is supplied in a surface-mount package measuring $0.52" \times 0.84" \times 0.44"$. The filter can be customized for other center frequencies and bandwidths.

KR Electronics Inc.,
Avenel, NJ (732) 636-1900,
www.krfilters.com.

RS No. 226

Directional Coupler Range



The new LYNX directional couplers cover the frequency range from 500 MHz to 18 GHz and are suitable for use in a wide variety of commercial and military applications.

They can be specified with a choice of SMA-type or N-type female connectors and are available with coupling values of 5, 6, 7, 10, 15, 20 or 30 dB. Featuring insertion losses as low as 0.4 dB, the couplers offer VSWR values from 1.2:1 to 1.6:1, a frequency sensitivity of ± 0.7 dB or ± 1.0 dB, and a directivity of 10, 12, 18 or 20 dB. The couplers have an operating temperature range of -55° to 85° C and are suitable for integration into mobile-phone infrastructure or satellite communications equipment.

Link Microtek Ltd.,
Basingstoke, UK +44 (0)1256 355771,
www.linkmicrotek.com.

RS No. 227

Band Reject Filter



Lorch model 6BRX-2257/X65-SR is a band reject filter with a center frequency of 2257 MHz. Insertion loss is 1 dB from 1400 to 2100 MHz and 3 dB from 2375 to 5500 MHz. Rejection is 40 dB from 2225 to 2290 MHz. Operating temperature is -40° to $+85^{\circ}$ C.

Lorch Microwave,
Salisbury, MD (410) 860-5100,
www.lorch.com.

RS No. 228

Reactive Power Splitters



Model Dx-19FN series is a collection of low cost two-, three- and four-way wideband reactive power splitters. The new series has been designed to a bandwidth of 700 to 2700 MHz, to

Phase Locked And Crystal Oscillators

Features:

- Band Coverage from VHF through Ka-Band
- Proven Performance in Various Applications
- Single and Dual Loop Models available with Internal and External Reference
- Small Modular Assemblies from 2.25" x 2.25" x 0.6"
- High Power and Low Harmonic Options available



Model	Frequency Range	Type	Typical Phase Noise						Output Frequency	Output Power (dBm, Min.)
			10	100	1K	10K	100K	1M		
XTO-05	5-130 MHz	Ovenized Crystal	-95	-120	-140	-155	-160	-	100 MHz	11
PLD	30-130 MHz	P.L. Crystal	-95	-115	-140	-155	-155	-	100 MHz	13
PLD-1C	130-1000 MHz	P.L. Mult. Crystal	-80	-100	-120	-130	-135	-	560 MHz	13
BCO	100-16.5 GHz	P.L. Single Loop	-65	-75	-80	-90	-115	-	16.35 GHz	13
VFS	1-14 GHz	Multiple Freq. Dual Loop	-60	-75	-110	-115	-115	-	12.5 GHz	13
DLCRO	8-26 GHz	P.L. CRO Dual Loop	-60	-85	-110	-115	-115	-138	10 GHz	13
PLDRO	2-40 GHz	P.L. DRO Single/Dual	-60	-80	-110	-115	-120	-145	10 GHz	13
CP	8-3.2 GHz	P.L. CRO Single Loop	-80	-110	-120	-130	-130	-140	2 GHz	13
CPM	4-15 GHz	P.L. Mult. Single Loop	-60	-90	-105	-110	-115	-130	12 GHz	13
ETCO	1-24 GHz	Voltage Tuned CRO	-	-	-70	-100	-120	-130	2-4 GHz*	13

* Octave band.

For additional information or technical support, please contact our Sales Department at (631) 439-9220 or e-mail components@miteq.com



100 Davids Drive, Hauppauge, NY 11788
(631) 436-7400 FAX: (631) 436-7430

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Visit <http://mwj.hotims.com/23286-79> or use RS# 79 at www.mwjjournal.com/info

include the common cellular, Wi-Fi and WiMAX frequencies, now being incorporated in indoor distributed antenna systems. An added benefit of this series is the guaranteed PIM performance of <-150 dBc when tested with two 20 W test signals. The extremely high reliability required of DAS systems is most easily met with a passive network approach.

Microlab, Wireless Telecom Group,
Parsippany, NJ (973) 386-9696,
www.wtcom.com.

RS No. 252

Precision Phase Shifters



These precision coaxial phase shifters are designed for 1 to 5 GHz and 1 to 12.4 GHz that provide a high level of accuracy with maximum phase shift of 180 deg. The model 3752 cov-

ers 1 to 5 GHz and provides 180 deg. of phase shift at 1 GHz. It has insertion loss of 0.5 dB or less and maximum VSWR of 1.25. The model 3753B covers 3.5 to 12.4 GHz and provides 180 deg. of phase shift at 3.5 GHz. It offers insertion loss of 0.7 dB and maximum VSWR of 1.4. Both models can handle 200 W average and 1 kW peak power, have accuracy of ± 0.5 dB/GHz, use Type N connectors, and have a digital dial display of phase shift.

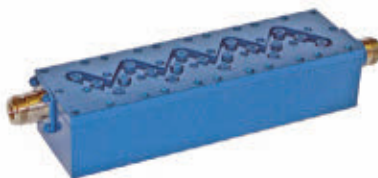
Narda Microwave-East,
Hauppauge, NY (631) 231-1700,
www.nardamicrowave.com/east.

RS No. 229

Wi-Fi Bandpass Filter



Reactel part number 8CX9-2436.5-X60N11 is a bandpass filter suitable for IEEE 802.1



applications. This unit is centered at 2436.5 MHz and has a minimum passband of 60 MHz and insertion loss of less than 0.75 dB. With high selectivity and a weather proof exterior, this unit is a great fit for your application.

Reactel Inc.,
Gaithersburg, MD (301) 519-3660,
www.reactel.com.

RS No. 230

Programmable Step Attenuators



RLC Electronics' PA Series Attenuators are binary programmable step attenuators designed to operate from DC to 20 GHz. Two basic models offer attenuation ranges of 15 and 70 dB. Control is in standard format: 1-2-4-8. The attenuators are available with failsafe or latching operation, 12 or 28 V coils and optional TTL drivers, with a choice of frequency ranges.

RLC Electronics Inc., Mount Kisco, NY
(914) 241-1334, www.rlcelectronics.com.

RS No. 232

Right Angle Adapters



The UG-27 C/U is a right angle adapter that features solderless construction. The solder-

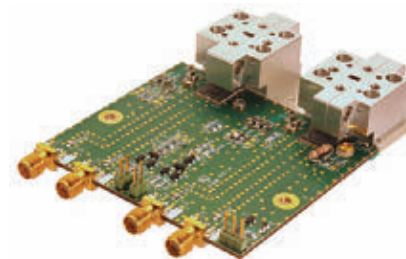


free construction offers dependability equal to a straight plug while achieving 90° bends. The solder-free adapters also address RoHS compliance issues by reducing lead content. The 50 ohm UG-27 C/Us perform efficiently up to 11 GHz and are rated for operating voltages of 1000 V RMS. The right angle adapters have a maximum dielectric withstanding voltage of 2000 V RMS at 60 Hz at sea level. They are designed for a temperature range of -65° to +165°C and meet interface standards in accordance with MIL-STD-348. VSWR is 1.15 from DC to 6 GHz, and 1.35 from 6 to 11 GHz.

San-tron Inc.,
Ipswich, MA (978) 356-1585,
www.santron.com.

RS No. 233

60 GHz Converter



The FC1001V/00 broadband converter is a versatile building block for 60 GHz applications. It combines an up-converter and a down-converter in a single unit. Both operate independently and can thus be used for both frequency

Radar System Analysis, Design and Simulation

Eyung W. Kang

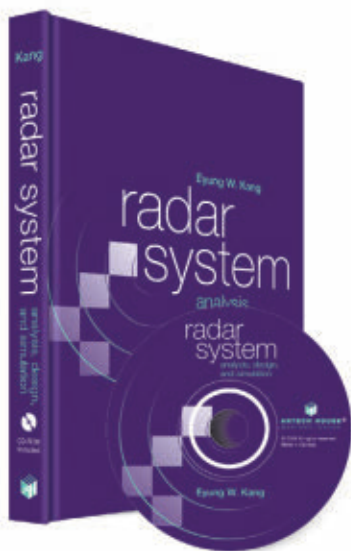
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Eamon Nash, Analog Devices

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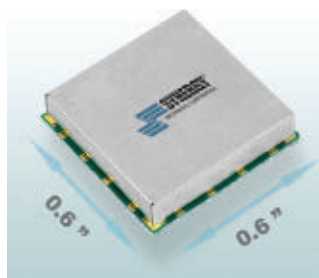
NEW PRODUCTS

multiplexed and time multiplexed applications. The converter has the advantage of using external LO sources, with the user having full control of phase noise and frequency selection. Frequency multipliers (x8) are integrated in both the up-converter and the down-converter. The LO injection is done at 7 GHz with +0 dBm power. Other features include: 57 to 63 GHz RF bandwidth, > 1 GHz IF bandwidth and +10 dBm typical output power. Applications include point to point or multipoint radio, EW, secure communication and measurement.

Sivers IMA AB,
Kista, Sweden +46-8-7036800,
www.siversima.se.

RS No. 234

Surface-mount Intelligent Synthesizers



The MFSH series of tiny surface-mount intelligent synthesizers with on-board microcontroller allows for self-programmable fixed frequency or wideband signal generation from a 0.6" package. Several models are available starting with frequencies from 1350 to 6500 MHz. Models are available with step size starting at 500 kHz.

Synergy Microwave Corp.,
Paterson, NJ (973) 881-8800, www.synergymicrowave.com.

RS No. 251

Surface-mount Feedthrus



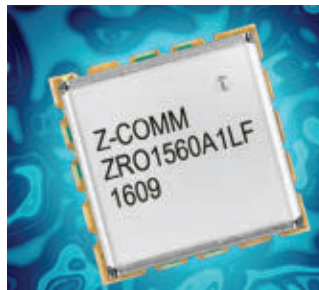
This mini surface-mount 50 ohm feedthru is based on Thunderline's successful initial SMT Bell Pin offering. This new product has been designed to emulate the existing design, but will be one third less in size and will be built with a smaller pin. The use of a smaller pin in its new mini surface-mount package will enable Thunderline customers to use this part in both J-band and K-band frequency ranges. Based on initial expectations Thunderline an-

ticipates this part will perform to limits somewhere between 22 and 25 GHz.

Thunderline-Z,
Hampstead, NH (603) 329-4050,
www.thunderlinez.com.

RS No. 235

Voltage-controlled Oscillator



This RoHS compliant voltage-controlled oscillator (VCO) model ZRO1560A1LF is designed for L-band. The ZRO1560A1LF operates at 1560 MHz with a tuning voltage range of 0 to 5 VDC. This VCO features a typical phase noise of -121 dBc/Hz at 10 kHz offset and a typical tuning sensitivity of 0.7 MHz/V. The ZRO1560A1LF is designed to deliver a typical output power of 0 dBm at 5 VDC supply while drawing 18 mA (typical) over

the temperature range of -40° to 85°C. This VCO features typical 2nd harmonic suppression of -30 dBc and comes in Z-Comm's industry standard MINI-16 package measuring 0.5" x 0.5" x 0.22".

Z-Communications Inc.,
San Diego, CA (858) 621-2700,
www.zcomm.com.

RS No. 236

2 W & 5 W DC to 18 GHz ATTENUATORS

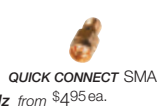
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Rugged Stainless Steel Construction, High Repeatability, Miniature Size, Low Cost, and Off-The-Shelf Availability are some of the features that make Mini-Circuits "BW" family of precision fixed attenuators stand above the crowd! This extremely broad band DC to 18 GHz series is available in 5 watt Type-N and 2 & 5 watt SMA coaxial designs, each containing 15 models with nominal attenuation values from 1 to 40 dB. Built tough to handle 125 watts maximum peak power, these high performance attenuators exhibit excellent temperature stability, 1.15:1 VSWR typical, and cover a wealth of applications. So contact Mini-Circuits today, and capture this next generation of performance and value! *Mini-Circuits...we're redefining what VALUE is all about!*

Now Available! Adapters (Prices: qty. 1-49)



MODELS (Add Prefix BW-)
2 W SMA 5 W SMA 5 W Type-N

			Attenuation (dB)	
			Nominal	Accuracy*
\$29.95	\$44.95	\$54.95		
S1W2	S1W5	N1W5	1	±0.40
S2W2	S2W5	N2W5	2	±0.40
S3W2	S3W5	N3W5	3	±0.40
S4W2	S4W5	N4W5	4	±0.40
S5W2	S5W5	N5W5	5	±0.40
S6W2	S6W5	N6W5	6	±0.40
S7W2	S7W5	N7W5	7	-0.4, +0.9
S8W2	S8W5	N8W5	8	±0.60
S9W2	S9W5	N9W5	9	-0.4, +0.8
S10W2	S10W5	N10W5	10	±0.60
S12W2	S12W5	N12W5	12	±0.60
S15W2	S15W5	N15W5	15	±0.60
S20W2	S20W5	N20W5	20	-0.5, +0.8
S30W2	S30W5	N30W5	30	±0.85
S40W2	S40W5	N40W5	40	-0.5, +1.5

*At 25°C includes frequency and power variations.



To order Attenuators as RoHS, add + to base model No. Example: BW-S1W2+
Adapters available as RoHS, see web site.

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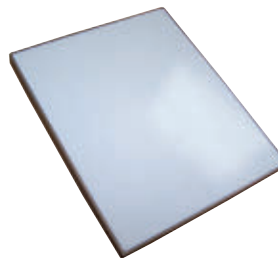
Herotek's model A402277 operates in a frequency range from 26 to 40 GHz and provides the user with an amplifier in its small package "1C" (size: 0.62" × 0.66" × 0.22"). It offers gain of 30 dB and gain variation of ±2.0 dB. Noise figure of 6.0 dB and P Out at 1 dB and compression is +16 dBm. Nominal DC current at 12 V is 400 mA. Application includes telecom infrastructure MW Radio and VSAT.

Herotek Inc.,
San Jose, CA (408) 941-8399,
www.herotek.com.

RS No. 237

Antennas

Flat Panel Antenna



Model FPA13-2.2R/1533 is a small (195 by 163 by 12.6 mm) flat panel antenna with directional beam pattern, 40° azimuth by 40° elevation. Its frequency range is 2.2 to 2.35 GHz and it has 13 dBi gain with right hand circular polarization. It is designed for use within an information system for telemetry applications in the defence and surveillance industries. It can be incorporated into an existing multi-sector framework, and conforms to

existing technical and environmental specifications. The antenna can be used in a range of applications, providing operators with flexibility when designing network systems, and may also be used in industries where data is commercially valuable.

Cobham Antenna Systems,
Microwave Antennas,
Cheveley, Newmarket, UK
+44 (0) 1638 732177,
www.cobham.com/antennasystems.

RS No. 238

Broadband Horn Antennas



Cobham Sensor Systems' H-1498 series broadband linear horn antennas provide superior performance for use in a wide variety of laboratory, commercial and military applications. With excellent input VSWR over the 2 to 18 GHz band, these antennas provide high gain across the frequency range and consistent pattern performance. They have become a laboratory

standard as a reference horn in anechoic chambers and outdoor ranges. The H-1498 is available with SMA female connector (standard) and TNC female connector (H-1498T). A further option is a radome/aperture cover (H-1498R) for outdoor use.

Cobham Sensor Systems,
Lansdale, PA (215) 996-2416,
www.cobhamdes.com.

RS No. 239

GPS Antenna Module

The A1035-H antenna module, with a footprint of 16.5 by 30.5 mm², is based on the company's A1084 GPS receiver. It is designed around the SiRFstar III GPS chip and is optimized for use with passive antennas. With the on-module antenna tuned to the receiver, a high level of sensitivity is



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For RoHS compliant requirements,

ADD + SUFFIX TO BASE MODEL No. Example: MCA1-85L+

Model	LO Level (dBm)	Freq. Range (MHz)	Conv. Loss (dB)	LO-RF Isol. (dB)	Price \$ ea. (Qty. 10)
MCA1-85L	4	2800-8500	6.0	35	9.45
MCA1-12GL	4	3800-12000	6.5	38	11.95
MCA1-24	7	300-2400	6.1	40	5.95
MCA1-42	7	1000-4200	6.1	35	6.95
MCA1-60	7	1600-6000	6.2	30	7.95
MCA1-85	7	2800-8500	5.6	38	8.95
MCA1-12G	7	3800-12000	6.2	38	10.95
MCA1-24LH	10	300-2400	6.5	40	6.45
MCA1-42LH	10	1000-4200	6.0	38	7.45
MCA1-60LH	10	1700-6000	6.3	30	8.45
MCA1-80LH	10	2800-8000	5.9	35	9.95
MCA1-24MH	13	300-2400	6.1	40	6.95
MCA1-42MH	13	1000-4200	6.2	35	7.95
MCA1-60MH	13	1600-6000	6.4	27	8.95
MCA1-80MH	13	2800-8000	5.7	27	10.95
MCA1-80H	17	2800-8000	6.3	34	11.95

Dimensions: (L) 0.30" x (W) 0.250" x (H) 0.080"
U.S. Patent # 7,027,795

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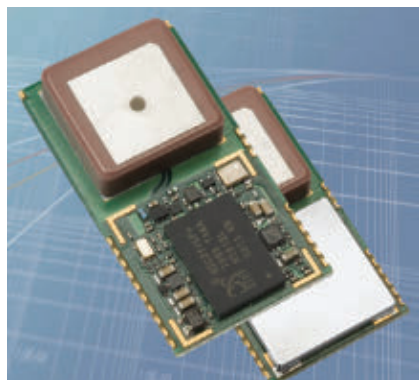


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RF/IF MICROWAVE COMPONENTS

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achieved. Furthermore, the A1035-H has been especially designed for an extremely low current draw (an average of 85 mW in tracking mode), fulfilling the latest requirements for more integration and cost-saving solutions.

Vincotech GmbH,
Unterhaching, Germany
+49 (0) 89 8780 670,
www.vincotech.com.

RS No. 240

Material

RFID Tag

MetalTag™ Impact is a Read-on-Metal EPC Gen 2 RFID tag. MetalTag Impact is constructed of a ruggedized outer coating, using a patent-

ed elastomer with a robust exoskeleton. The tag is ideal for challenging environmental conditions, such as severe weather, wide temperature variations, direct and prolonged UV exposure and significant physical impact. Its small form factor makes it amenable to a wide variety of surfaces often associated with asset tracking and supply chain applications. The tag is also available with an optional metallic ground plane for read on liquid applications, custom color coded labels and pre-encoded bar codes.

Emerson & Cuming Microwave Products Inc., Randolph, MA (781) 961-9600,
www.eccosorb.com.

RS No. 241

Software

Antenna Design Tool



Antenna Magus is an expert system for antenna design with a large database of antennas that makes it suitable for a broad range of applications. Its feature set is targeted at aiding engineers to get to the customization phase of an

antenna design quickly and reliably. Validated, parametric models of the initial design are exported seamlessly into CST MICROWAVE STUDIO or FEKO, where customization can be done in tried-and-trusted analysis tools. Antenna Magus will expand both the number of antennas it can design and export, as well as in the number of analysis tools it interfaces with. It will aid antenna design engineers, EMC engineers requiring antenna models and system integrators who require antenna models for antenna placement studies.

Computer Simulation Technology (CST) AG, Darmstadt, Germany
+49 6151 7303 0, www.cst.com.

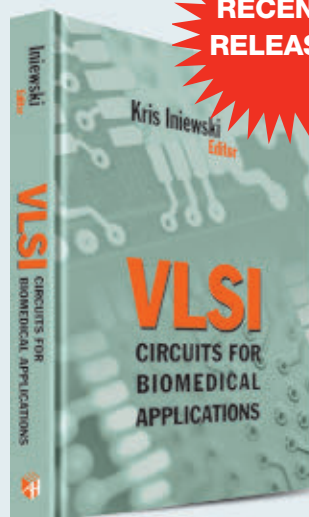
RS No. 242

Location Finding Software



New location finding software for the IZT R3000 receiver series for both commercial and military applications has been introduced. It is a low-cost method that enables users to add location finding capabilities to their monitoring stations. Using cost efficient Time-Difference-Of-Arrival (TDOA) methods, the software resides on a central station and connects multiple IZT R3000 receivers in different remote locations. Comparing their received signals results in accurate delay measurements that are then used to derive the location of the signal's source. Re-

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Subsystems and Systems

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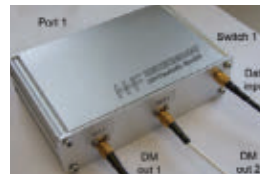


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RS No. 254

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The MiniTrans 2401 is an OEM 2.45 GHz radio modem for data rates up to 25 Mbit/s for point to point data transfer with

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RS No. 216

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VENDORVIEW



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MITEQ Inc.,
Hauppauge, NY (631) 436-7400,
www.miteq.com.

RS No. 245

Tactical Transceivers



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Pole/Zero Corp., West Chester, OH
(513) 870-9060, www.polezero.com.

RS No. 246

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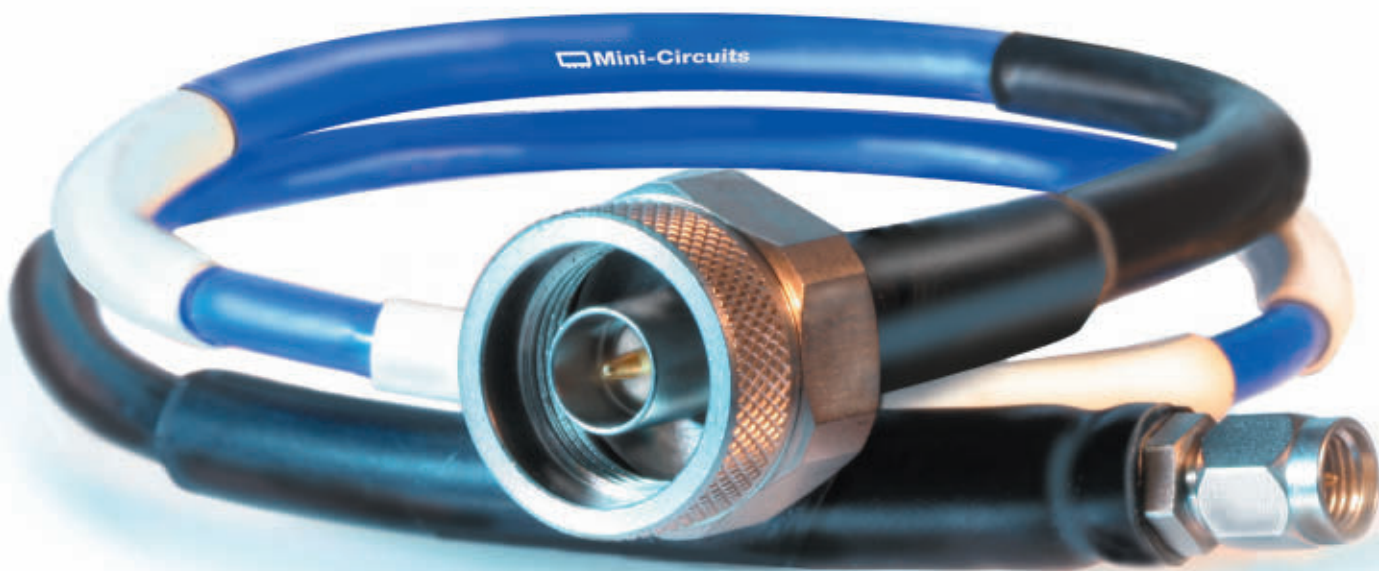
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CBL-3FT-SMSM+	SMA	3	1.5	27	72.95
CBL-4FT-SMSM+	SMA	4	1.6	27	75.95
CBL-5FT-SMSM+	SMA	5	2.5	27	77.95
CBL-6FT-SMSM+	SMA	6	3.0	27	79.95
CBL-10FT-SMSM+	SMA	10	4.8	27	87.95
CBL-12FT-SMSM+	SMA	12	5.9	27	91.95
CBL-15FT-SMSM+	SMA	15	7.3	27	100.95
CBL-25FT-SMSM+	SMA	25	11.7	27	139.95
Female to Male					
CBL-2FT-SMNM+	SMA to N-Type	2	1.1	27	99.95
CBL-3FT-SMNM+	SMA to N-Type	3	1.5	27	104.95
CBL-4FT-SMNM+	SMA to N-Type	4	1.6	27	112.95
CBL-6FT-SMNM+	SMA to N-Type	6	3.0	27	114.95
CBL-15FT-SMNM+	SMA to N-Type	15	7.3	27	156.95
Male to Male					
CBL-2FT-NMNM+	N-Type	2	1.1	27	102.95
CBL-3FT-NMNM+	N-Type	3	1.5	27	105.95
CBL-6FT-NMNM+	N-Type	6	3.0	27	112.95
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CBL-15FT-NMNM+	N-Type	15	7.3	27	164.95
CBL-20FT-NMNM+	N-Type	20	9.4	27	178.95
CBL-25FT-NMNM+	N-Type	25	11.7	27	199.95
Female to Female					
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CBL-3FT-SFNM+	SMA-F to N-M	3	1.5	27	124.95
CBL-6FT-SFNM+	SMA-F to N-M	6	3.0	27	146.95
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Male to Male					
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EM Research Inc.,
Reno, NV (775) 345-2411,
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RS No. 249

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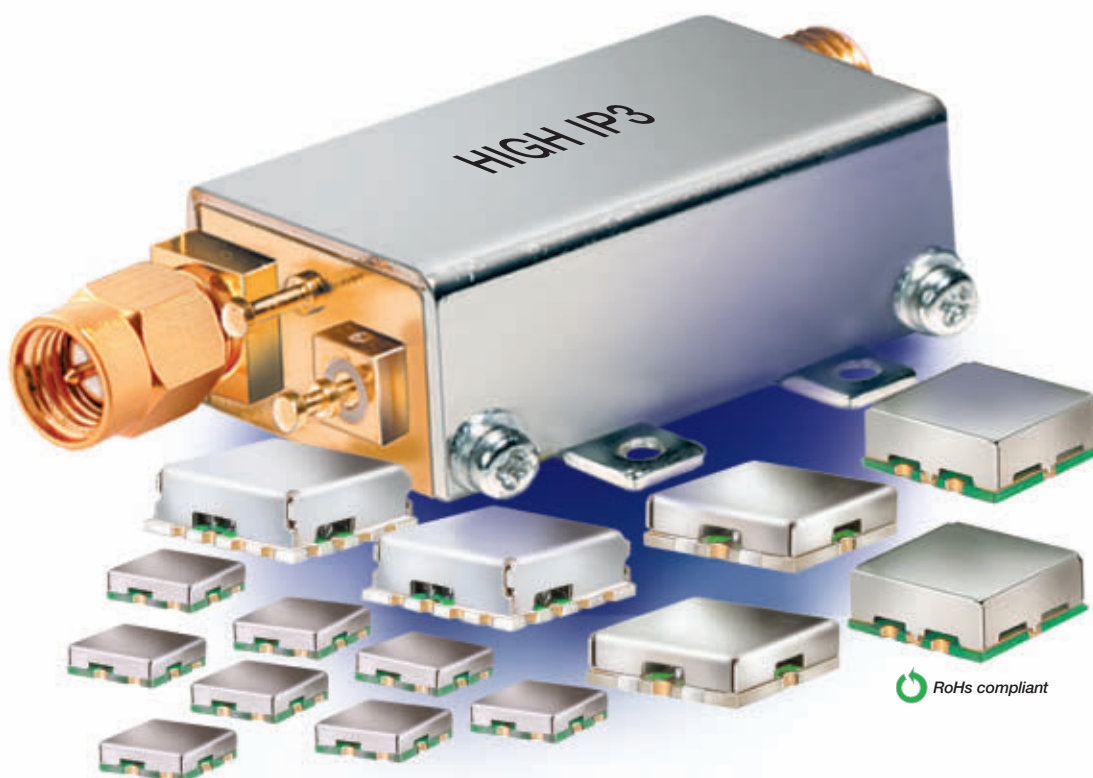


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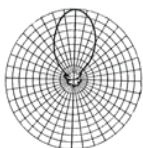


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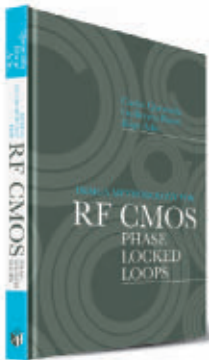


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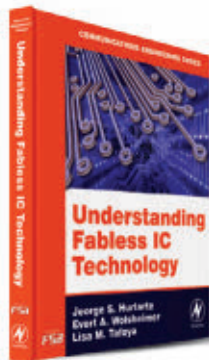
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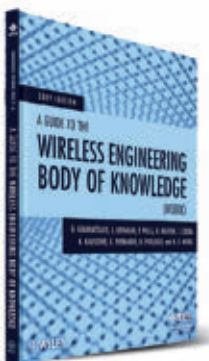
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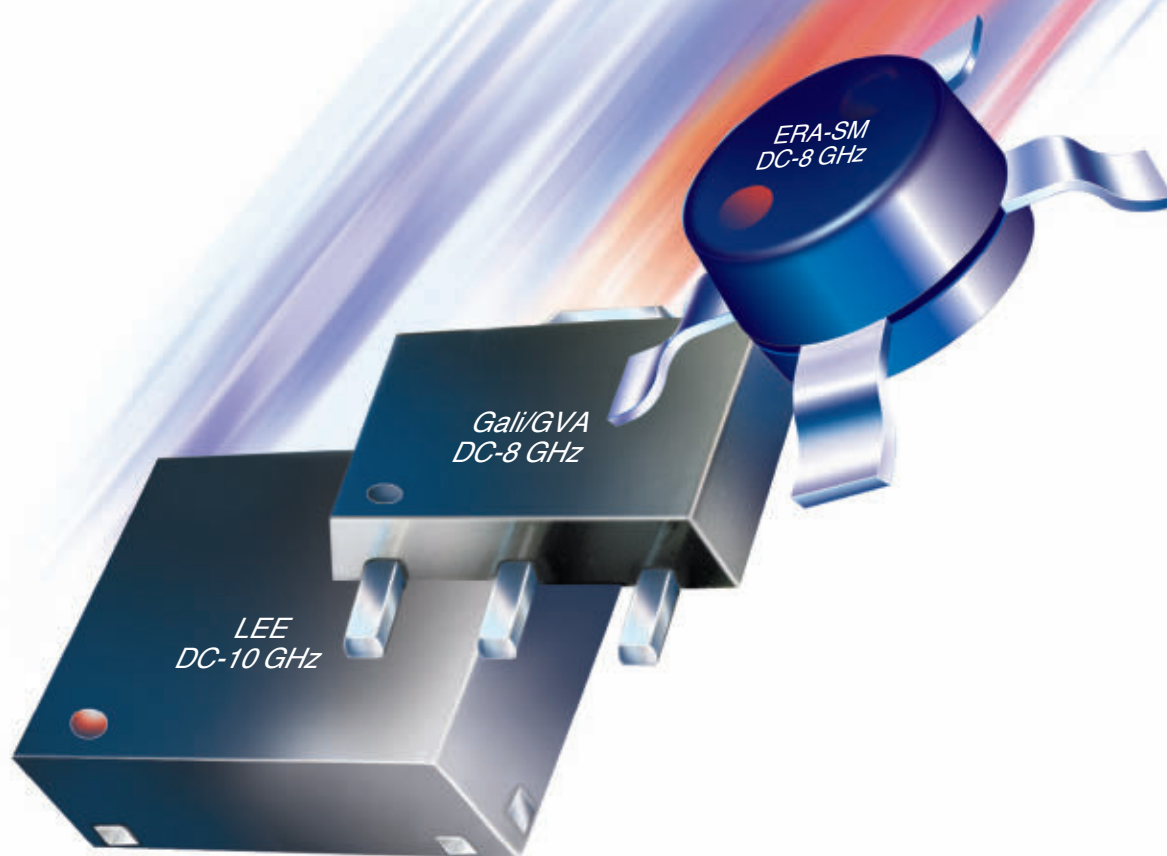
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RF/Microwave Candidate Pool

The shameful state of the RF/microwave candidate pool has again raised its ugly head. This reminds me of the recession from the early 1970s when we had very few universities, colleges and trade schools turning out graduates with skills in the electromagnetic field.

Our industry suffers when corporations are not supporting the educational systems to ensure a healthy crop of new technologists every year.

Now that we are in a recession, we still have thousands of career opportunities that we have no candidates to apply. The result is that contracts are late on delivery and our future through innovation is stalled.

It is up to industry and the educational system to keep the RF/microwave industry strong; they have to work together to support studies in this sector.

In the '70s, corporations like Raytheon, M/A-COM and many others supported several universities to develop microwave/RF studies. That solved the problem for a few years, but now we are back to square one.

If you are working with a company in this sector speak with your management and speak with your university, college, or trade school to promote education in the RF/microwave field.

I've seen similar times of shortage in engineering power and there is much to learn from what was done then.

Dave Germond

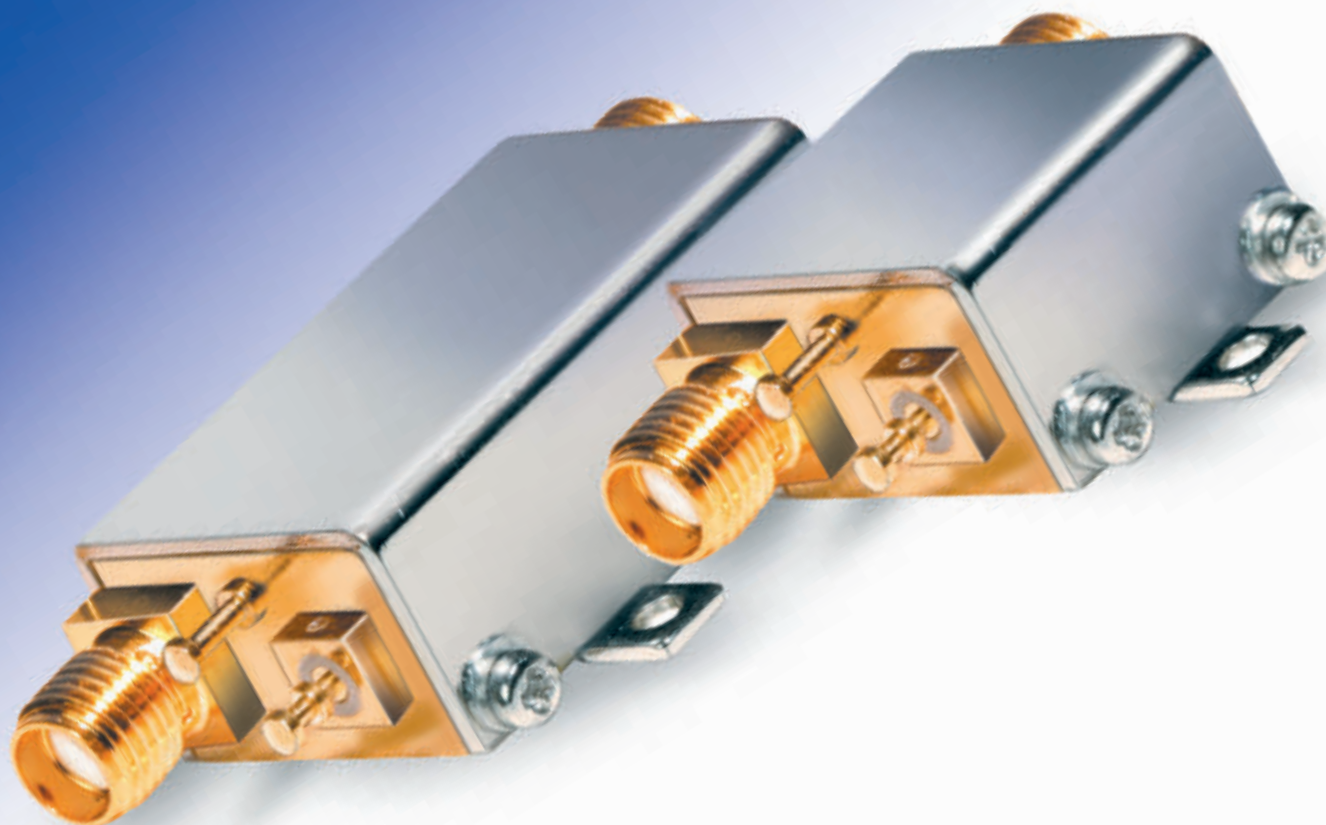
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IP3 (dBm)	15	20	9
Conv. Loss (dB)	5.0	6.67	7.1
L-R Isolation (dB)	55	47	36
L-I Isolation (dB)	40	45	37
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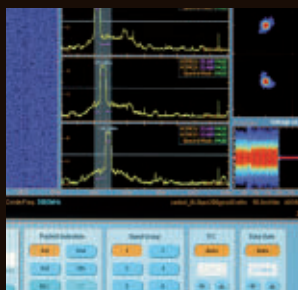
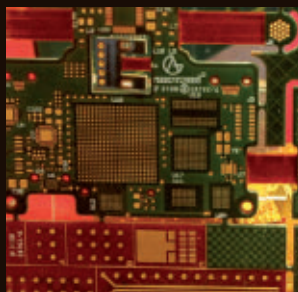
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AMPLIFIERS/SEMICONDUCTORS

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ACROSS

- 4** The vector ratio of voltage to current, the reciprocal of admittance
- 9** Wideband gap III-V material used to produce broadband, high power amplifiers
- 11** Undesired changes in a waveform that result in spurious content of the signal
- 14** A device or impedance that terminates the output of a device
- 15** Loss of signal resulting from the insertion of a device in a transmission line (2 words)
- 16** Material typically used to produce high frequency, broadband PIN diodes
- 17** PA return loss under actual output drive levels (2 words)
- 18** Energy at integral multiples of the frequency of the fundamental signal
- 21** The ratio of the input signal to noise ratio to the output signal to noise ratio for a circuit or system (2 words)
- 23** The process of varying the impedance seen by the output of an active device to other than 50 ohms in

order to measure performance parameters (2 words)

- 24** Measure of how much of the input power is usefully applied to the amplifier's output
- 25** The amount of power at which the amplitude of the output of a device or circuit is reduced by 1 dB from the expected small-signal gain

DOWN

- 1** Laterally diffused metal oxide semiconductor
- 2** Range of frequencies for which the amplifier gives "satisfactory performance"
- 3** The amount of electrical power converted to heat by a device (2 words)
- 5** The state of operation in which there is no interruption of the presence of a signal (2 words)
- 6** Undesired signals present at the output of a device under test that are neither harmonics nor intermodulation products
- 7** At a given point in a transmission system, the difference between the incident and reflected power (2 words)

8 The ratio between the amplitude of the output signal of a device or circuit compared to the amplitude of the input signal

10 Technique used to improve the linearity of amplifiers

12 The degree to which the impedance of a component differs from the transmission line or component to which it is connected

13 Amplifier class where the output filter blocks all harmonics to achieve very high efficiencies (2 words)

19 Amplifier configuration where the carrier amplifier is biased to operate in Class AB mode and the peaking amplifier is biased to operate in Class C mode to achieve higher efficiency

20 Metal Electrode Leadless Face package used for PIN diodes

22 Amplifier class widely used in SSB linear amplifier applications where low-distortion and high power-efficiency tend to both be very important (2 words)



CELEBRATING 2009: THE YEAR OF MMIX

2009 translates in Roman numerals to "MMIX." It only happens once, so Mimix Broadband is celebrating by declaring 2009... **the Year of MMIX**. During the year, we'll highlight key advances in our product portfolio, as well as pay tribute to other engineering feats – specifically the Seven Wonders of the Modern World as chosen by the American Society of Civil Engineers.

Toronto's CN Tower is a communications and tourist tower standing 553.33 meters (1,815.39 feet) tall. It is the tallest freestanding structure in the Americas and, amazingly, varies from true vertical accuracy by only 29 millimeters (1.1 inches) over the entire height of the tower. The CN Tower is a powerful communications tower for numerous radio and cellular media.

Here at Mimix, we have engineered an impressive range of power amplifiers (PAs) that tower above industry averages! Our PAs offer high power, excellent performance and efficiency, and are available in a selection of bare die and packaged versions.

MIMIX POWER AMPLIFIERS... TOWERING ABOVE INDUSTRY AVERAGES!

Description	Device	Frequency (GHz)	Gain (dB)	Gain Flatness (dB)	Output P1dB (dBm)	OIP3 (dBm)	Bias (mA @ V)	Package (mm)
Power Amplifier	XP9003	1.6	38.0	+/-0.5	+43.0	-	2.9 A @ 9.0	40x36
Power Amplifier (QFN)	XPI035-QH	5.9-9.5	26.0	+/-1.0	+29.0	+39.0	500 @ 6.0	4x4
Power Amplifier (QFN)	XPI050-QJ	7.0-9.0	15.0	+/-0.5	+34.5 Psat	+48.0	1.2 A @ 8.0	6x6
Power Amplifier (QFN)	XPI042-QT	12.0-16.0	21.0	+/-1.0	+25.0	+38.0	500 @ 5.0	3x3
Power Amplifier (QFN)	XPI043-QH	12.0-16.0	21.5	+/-1.0	+30.0	+41.0	700 @ 7.0	4x4
Power Amplifier	XPI057-BD	13.5-16.0	17.0	+/-1.0	+39.0	+48.0	3.7 A @ 7.5	DIE
Power Amplifier	XPI058-BD	14.5-16.0	27.0	+/-1.0	+36.0	+44.0	2.2 A @ 8.0	DIE
Power Amplifier	XPI072-BD	34.0-37.0	22.0	+/-2.0	+35.0 Psat	-	2.4 A @ 5.5	DIE
Power Amplifier	XPI073-BD	34.0-37.0	22.0	+/-2.0	+37.0 Psat	-	4.8 A @ 5.5	DIE

Explore our wide range of power amplifiers and download complete datasheets for all products at www.mimixbroadband.com.

Celebrate the Year of MMIX with us by visiting www.mimixbroadband.com/year-of-MMIX

Visit <http://mwj.hotims.com/23286-55> or use RS# 55 at www.mwjjournal.com/info

Mimix
BROADBAND™

providing optimal semiconductor solutions worldwide

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Wide bandwidth, HIGH POWER DEVICES

Unsurpassed quality + on-time delivery, is the Werlatone promise



WERLATONE



QUADRATURES



COUPLERS



DIVIDERS



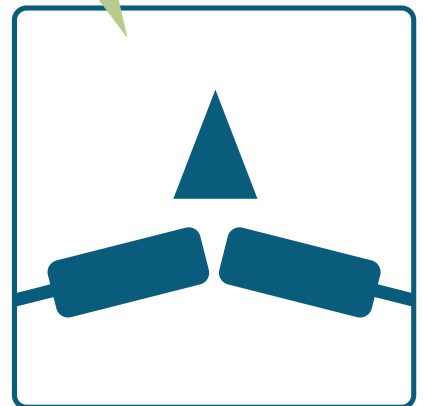
HYBRIDS

Breaking
all the
Rules

High Power Combiners



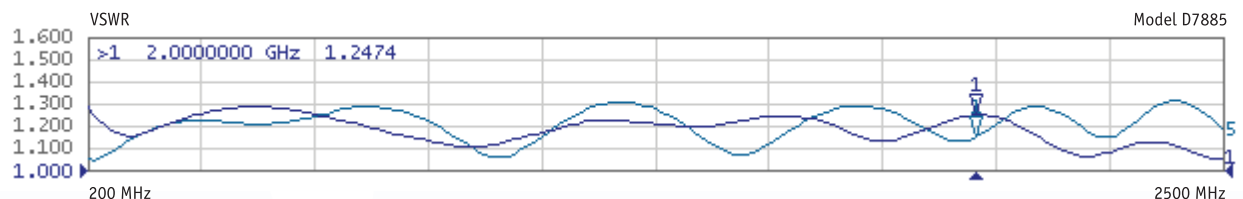
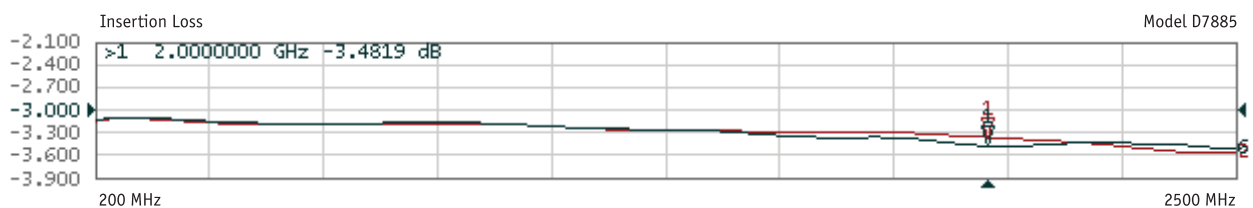
- 10:1 + Bandwidth
- Full Input Failure Protection
- Capable of Non-Coherent Combining



COMBINERS

**Multi-Section Power Dividers, first described by Seymour Cohn, employ a large number of floating, high value resistors, resulting in excessive high frequency roll-off and low unbalanced power capability.

**Werlatone's, Patent Pending "Collapsed Cohn" design requires only one or two, low value, high power resistors to provide the same port-to-port isolation and higher unbalanced power protection, while eliminating high frequency roll-off.



www.werlatone.com

Model	Type	Frequency (MHz)	Power (W CW)	Insertion Loss (dB)	VSWR	Isolation (dB)	Size (Inches)
D7885	2-Way	200-2500	200	0.65	1.40:1	15	7.7 x 1.6 x 1.1
D7823	2-Way	500-2500	200	0.4	1.35:1	15	4.7 x 2.0 x 0.8
D7630	2-Way	800-3000	200	0.4	1.35:1	15	3.7 x 1.9 x 0.87
D7539	4-Way	800-2800	200	0.6	1.35:1	17	5.5 x 4.1 x 1.1
D7695	4-Way	900-1300	100	0.4	1.30:1	20	4.0 x 3.3 x 0.8